Lecture 8

2017/2018

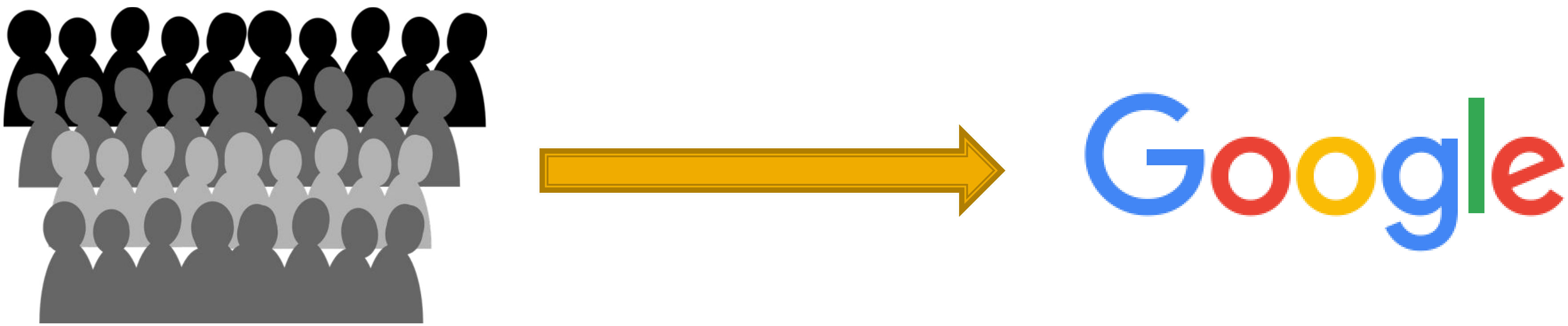
Microwave Devices and Circuits for Radiocommunications

Test

- Wisdom of the crowd ??

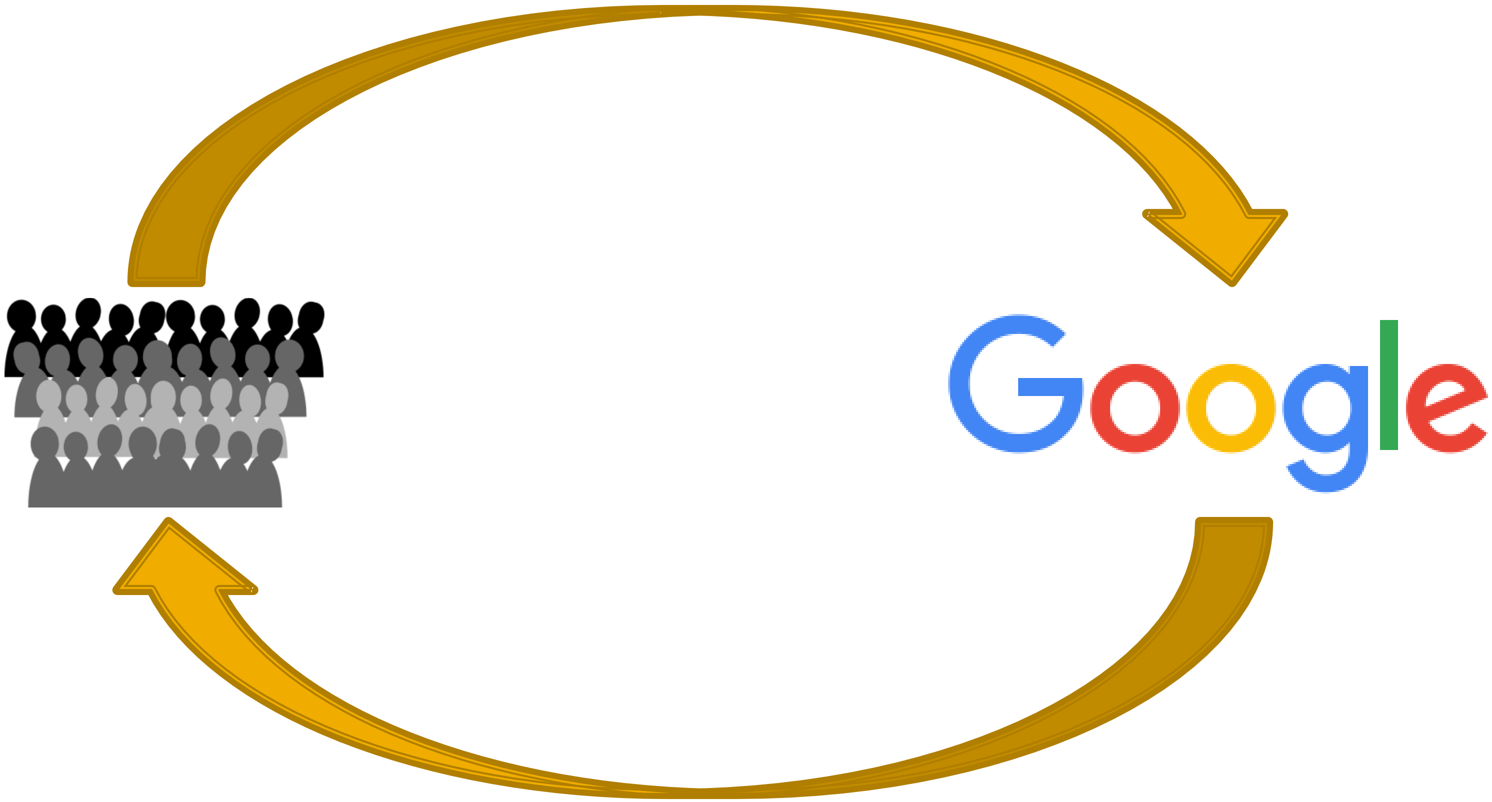
Test

- Wisdom of the crowd



Test

- Wisdom of the crowd **??**



Materials

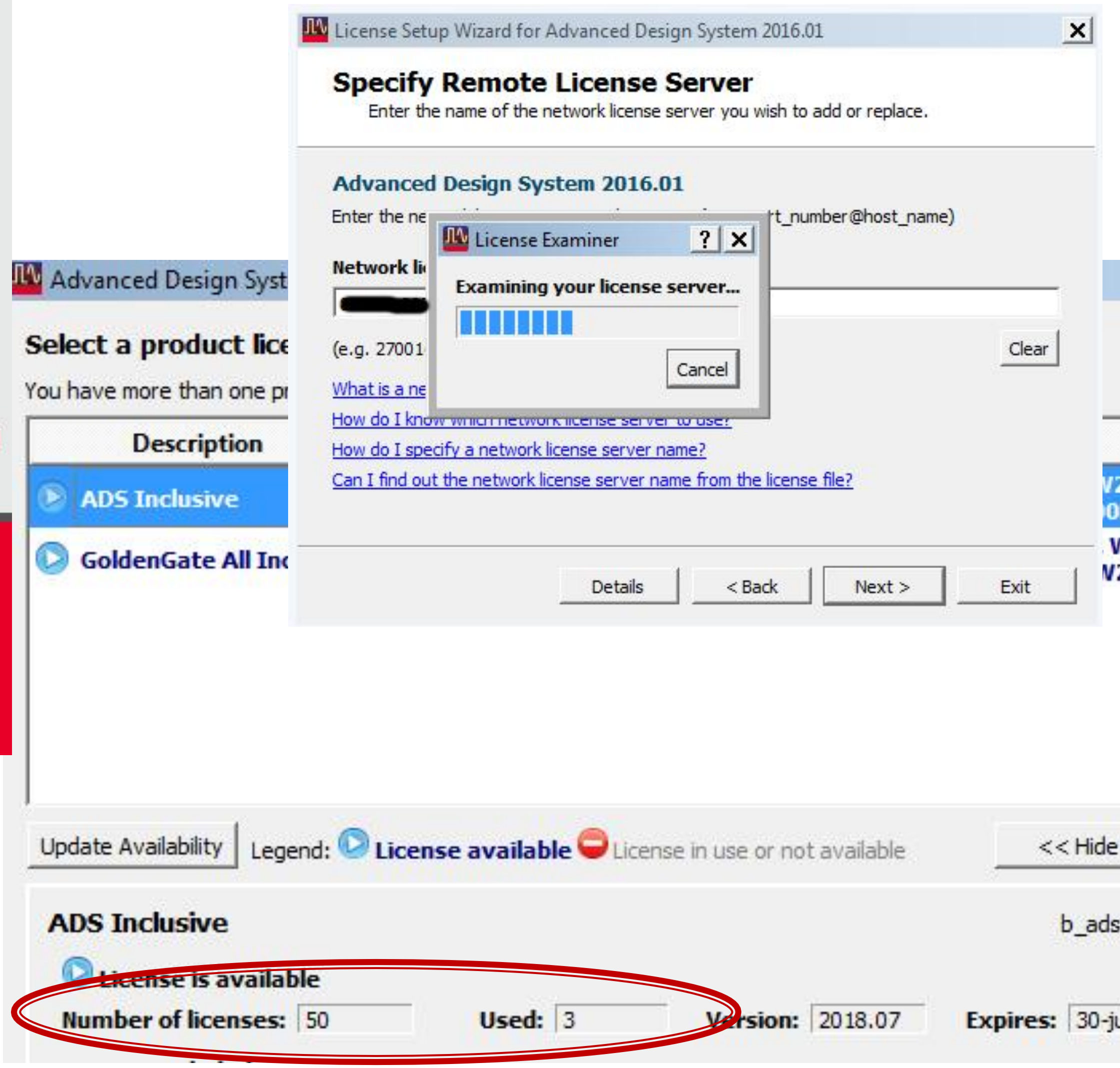
- RF-OPTO
  - **http://rf-opto.etti.tuiasi.ro**
- **David Pozar, "Microwave Engineering"**, Wiley; 4th edition , 2011
  - 1 exam problem ← Pozar
- Photos
  - sent by email: rdamian@etti.tuiasi.ro
  - used at lectures/laboratory

Software

- ADS ~~2016~~ **2017**
- EmPro ~~2015~~ **2017**
- based on IP from outside university or campus

Software


Advanced Design System
Premier High-Frequency and High Speed Design Platform
2016.01
KEYSIGHT TECHNOLOGIES
© Keysight Technologies 1985-2016


License Setup Wizard for Advanced Design System 2016.01
Specify Remote License Server
Enter the name of the network license server you wish to add or replace.
Advanced Design System 2016.01
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What is a ne
How do I know which network license server to use?
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Used: 3
Version: 2018.07
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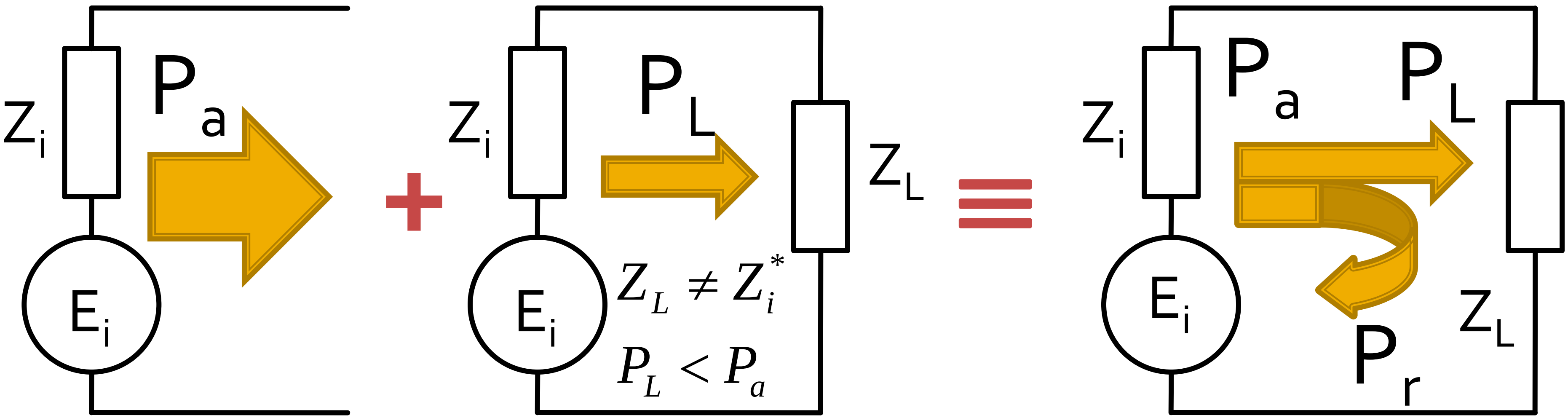
Reflection and power / Model

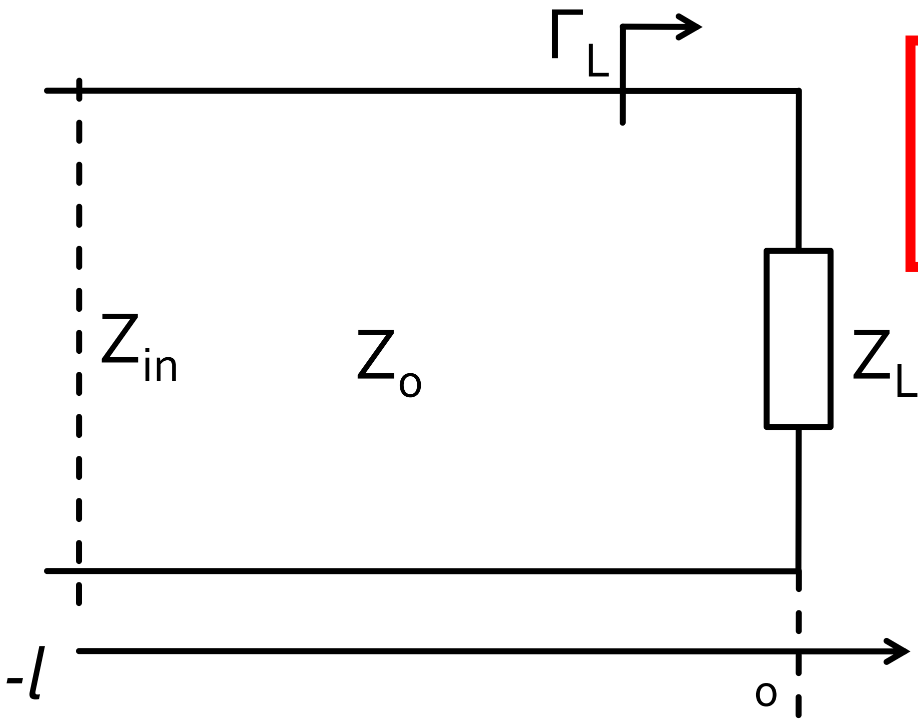


- The source has the ability to sent to the load a certain maximum power (available power) P_a
- For a particular load the power sent to the load is less than the maximum (mismatch) $P_L < P_a$
- The phenomenon is **"as if"** (model) part of the input power is reflected $P_r = P_a - P_L$
- The power is a **scalar !**

TEM transmission lines

The lossless line

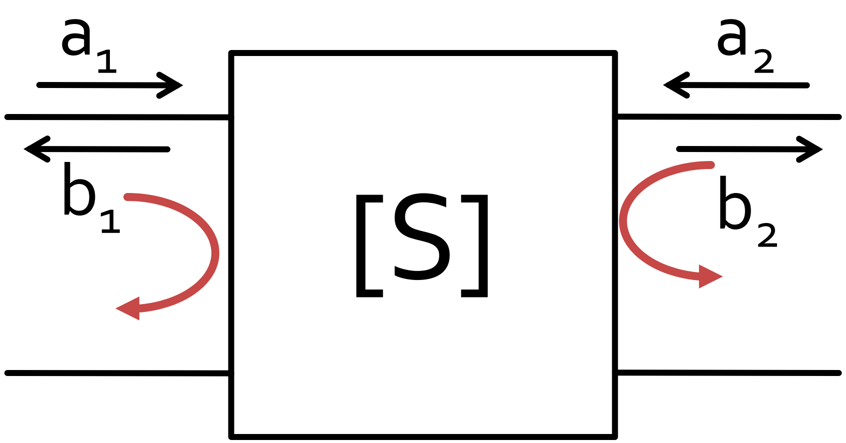
- input impedance of a length ***l*** of transmission line with characteristic impedance $\boldsymbol{Z_o}$, loaded with an arbitrary impedance $\boldsymbol{Z_L}$



$$Z_{in} = Z_0 \cdot \frac{Z_L + j \cdot Z_0 \cdot \tan \beta \cdot l}{Z_0 + j \cdot Z_L \cdot \tan \beta \cdot l}$$

Microwave Network Analysis

Scattering matrix – S

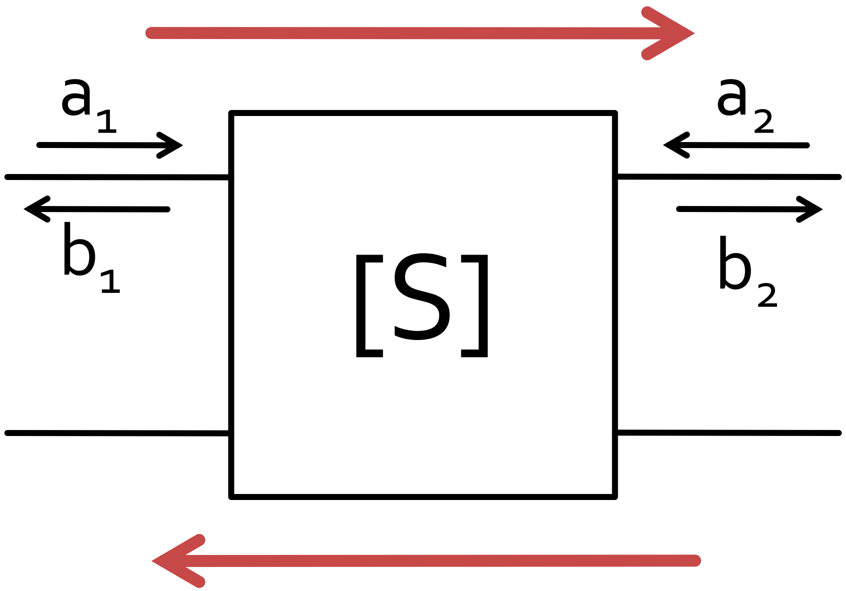


$$\begin{bmatrix} b_1 \\ b_2 \end{bmatrix} = \begin{bmatrix} S_{11} & S_{12} \\ S_{21} & S_{22} \end{bmatrix} \cdot \begin{bmatrix} a_1 \\ a_2 \end{bmatrix}$$

$$S_{11} = \left. \frac{b_1}{a_1} \right|_{a_2=0} \qquad S_{22} = \left. \frac{b_2}{a_2} \right|_{a_1=0}$$

- S_{11} and S_{22} are reflection coefficients at ports 1 and 2 when the other port is matched

Scattering matrix – S

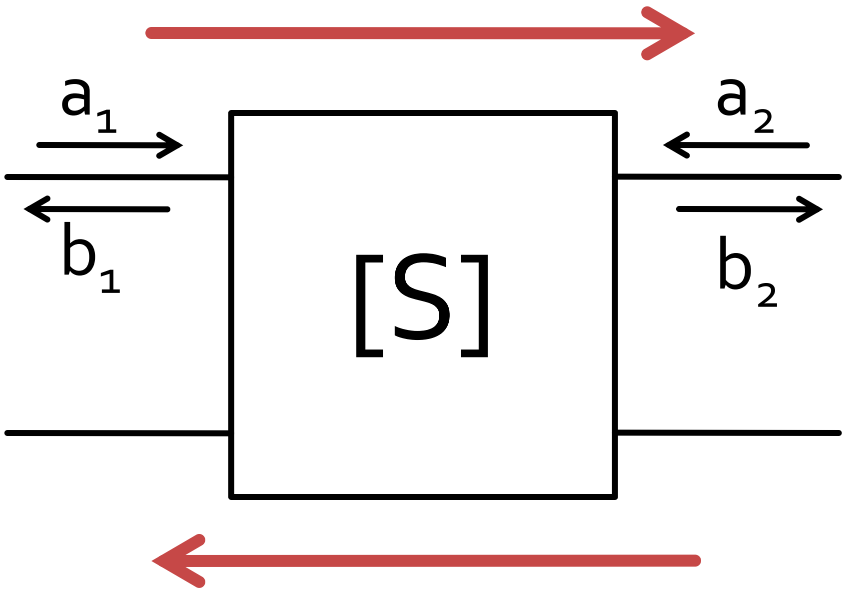


$$\begin{bmatrix} b_1 \\ b_2 \end{bmatrix} = \begin{bmatrix} S_{11} & S_{12} \\ S_{21} & S_{22} \end{bmatrix} \cdot \begin{bmatrix} a_1 \\ a_2 \end{bmatrix}$$

$$S_{21} = \left.\frac{b_2}{a_1}\right|_{a_2=0} \qquad S_{12} = \left.\frac{b_1}{a_2}\right|_{a_1=0}$$

- S_{21} and S_{12} are signal amplitude gain when the other port is matched

Scattering matrix – S



$$\begin{bmatrix} b_1 \\ b_2 \end{bmatrix} = \begin{bmatrix} S_{11} & S_{12} \\ S_{21} & S_{22} \end{bmatrix} \cdot \begin{bmatrix} a_1 \\ a_2 \end{bmatrix}$$

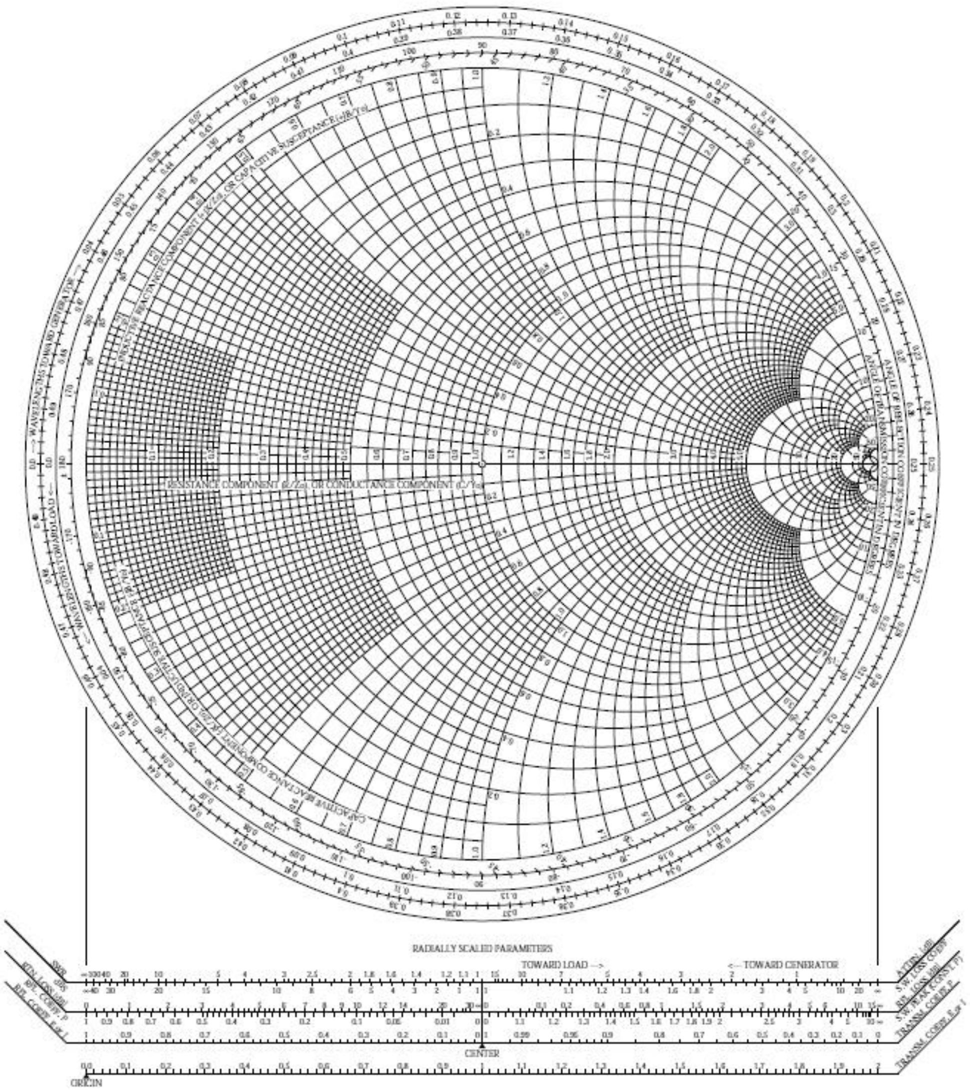
$$|S_{21}|^2 = \frac{Power\ in\ Z_0\ load}{Power\ \ from\ Z_0\ source}$$

- a,b
  - information about signal power **AND** signal phase
- S_{ij}
  - network effect (gain) over signal power **including** phase information

Impedance Matching

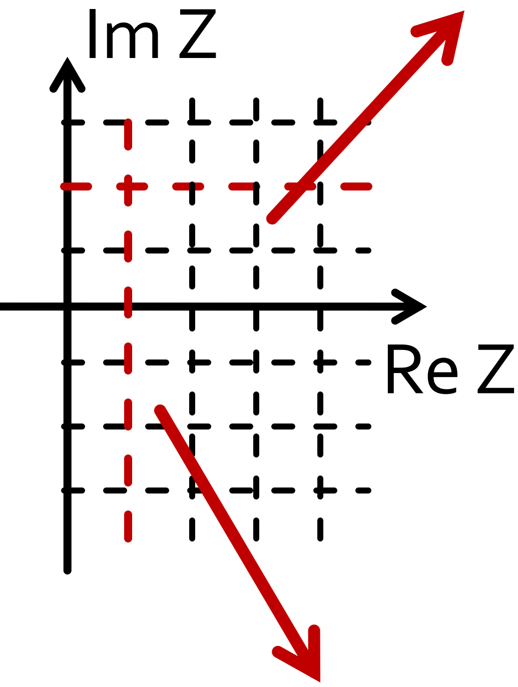
The Smith Chart

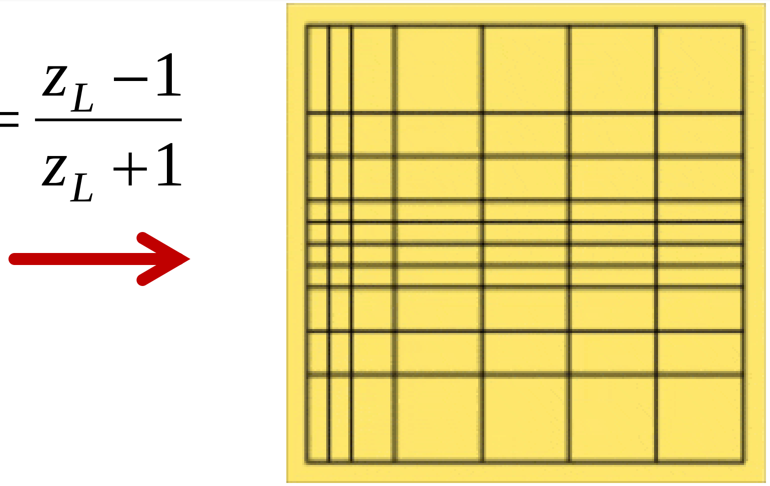
The Smith Chart

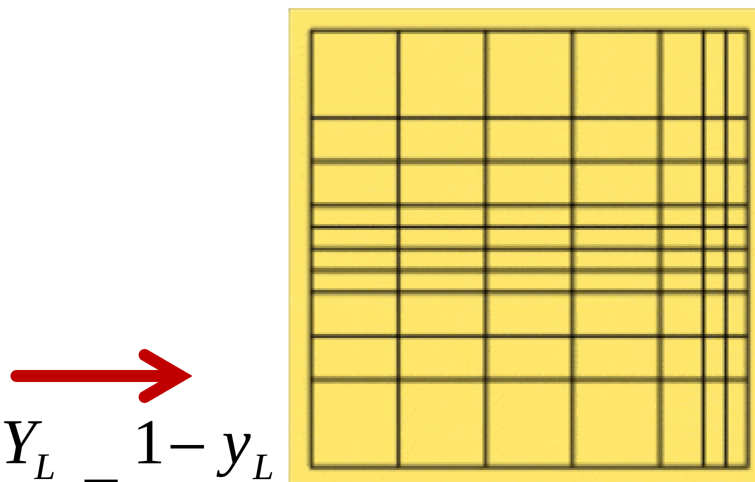


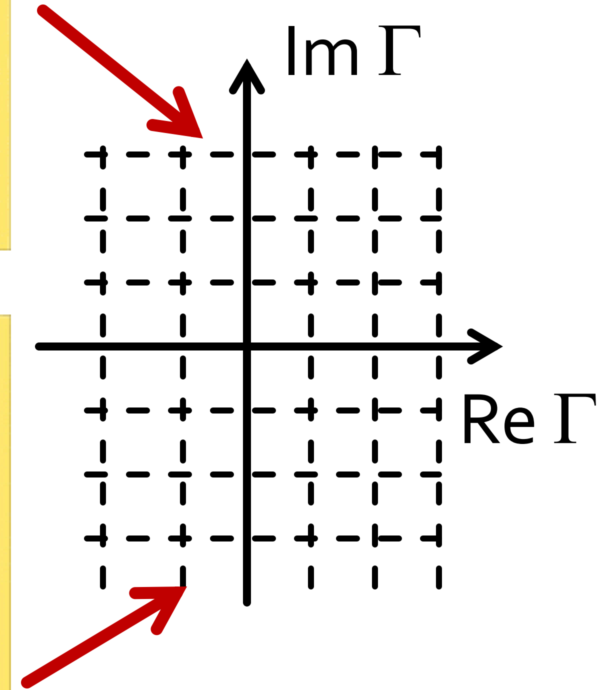
The Smith Chart

$$\Gamma = \frac{Z_L - Z_0}{Z_L + Z_0} = \frac{z_L - 1}{z_L + 1}$$



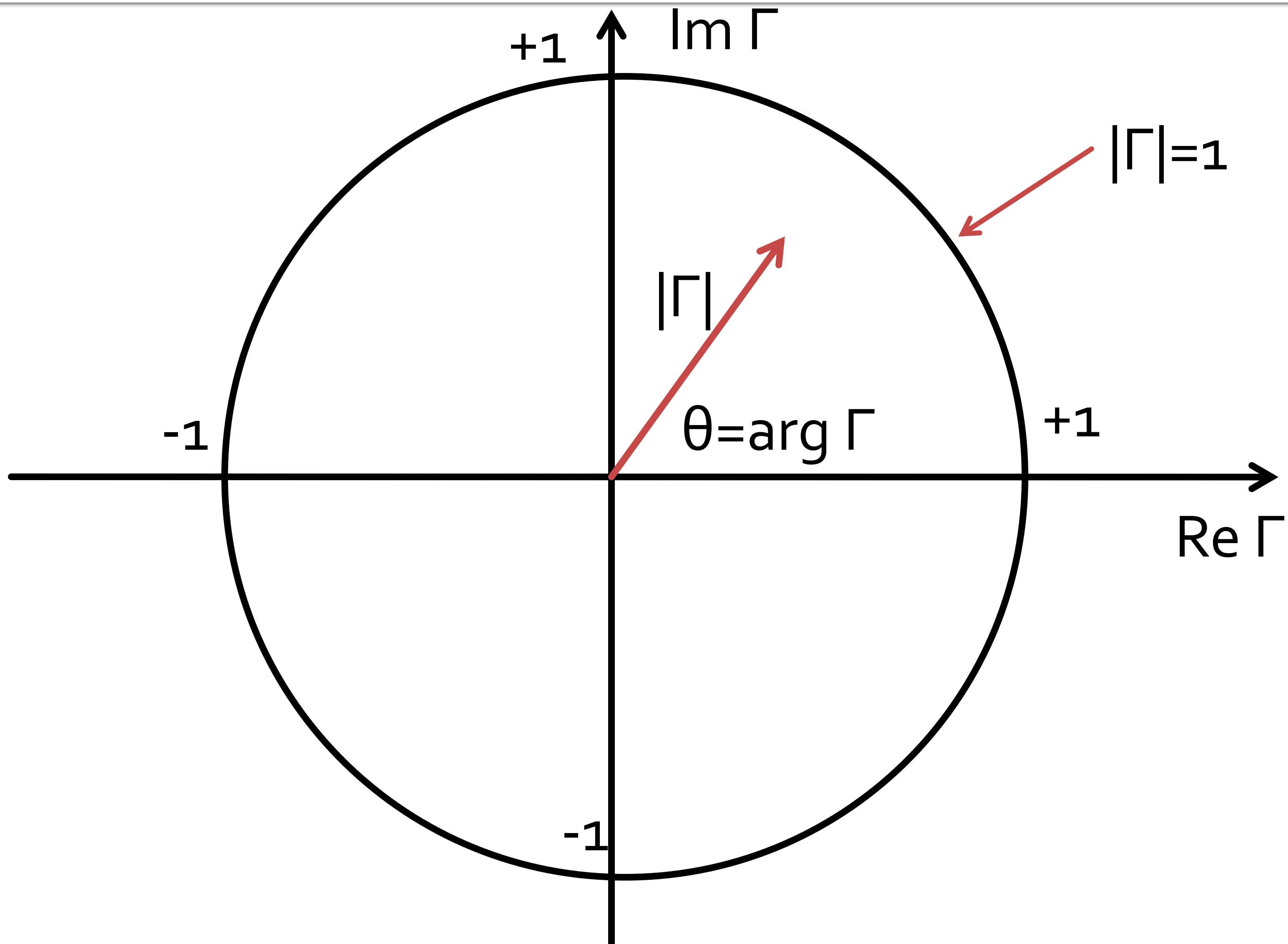






$$\Gamma = \frac{Z_L - Z_0}{Z_L + Z_0} = \frac{Y_0 - Y_L}{Y_0 + Y_L} = \frac{1 - y_L}{1 + y_L}$$

The Smith Chart

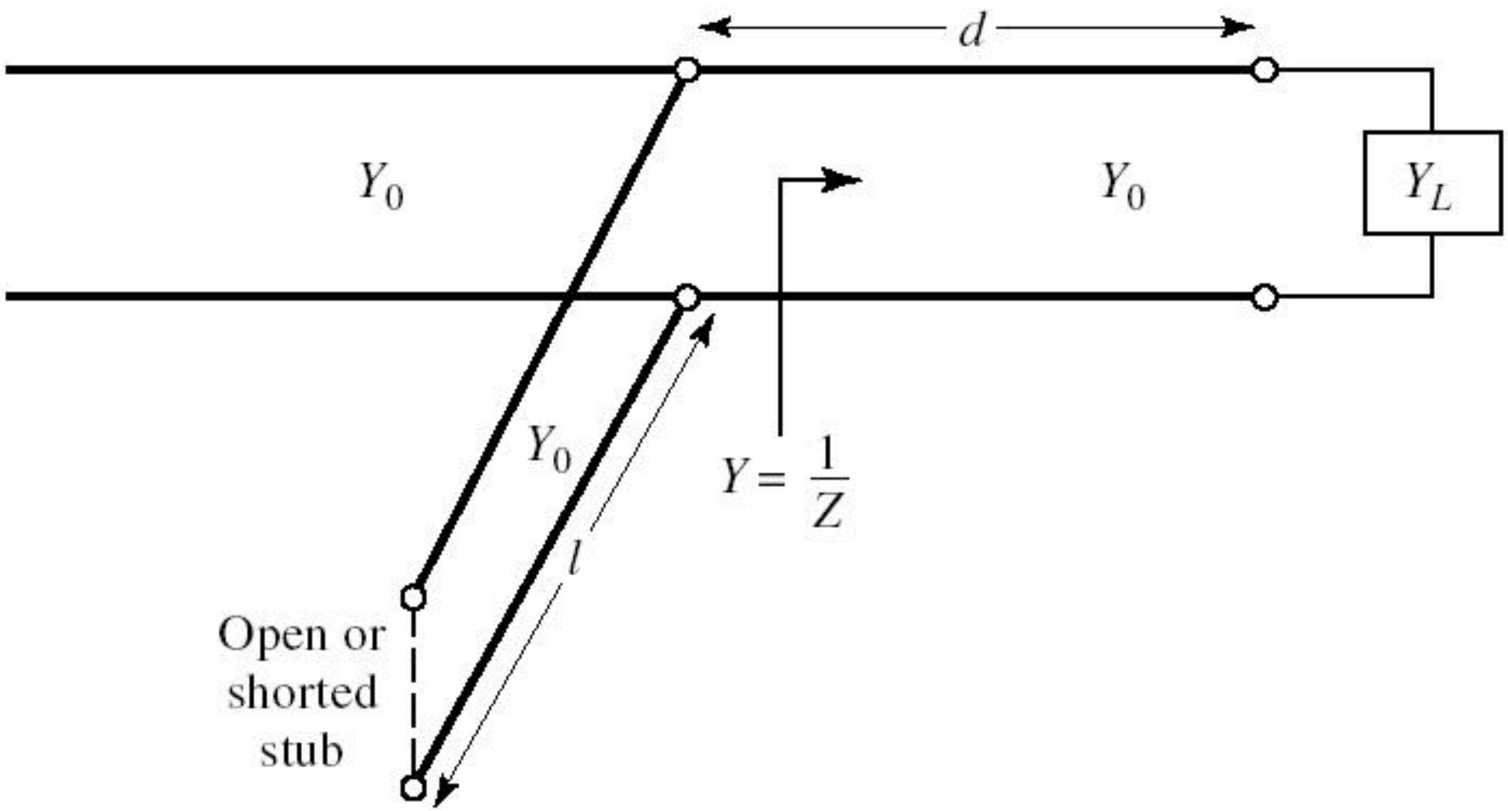


Impedance Matching with Stubs

Impedance Matching

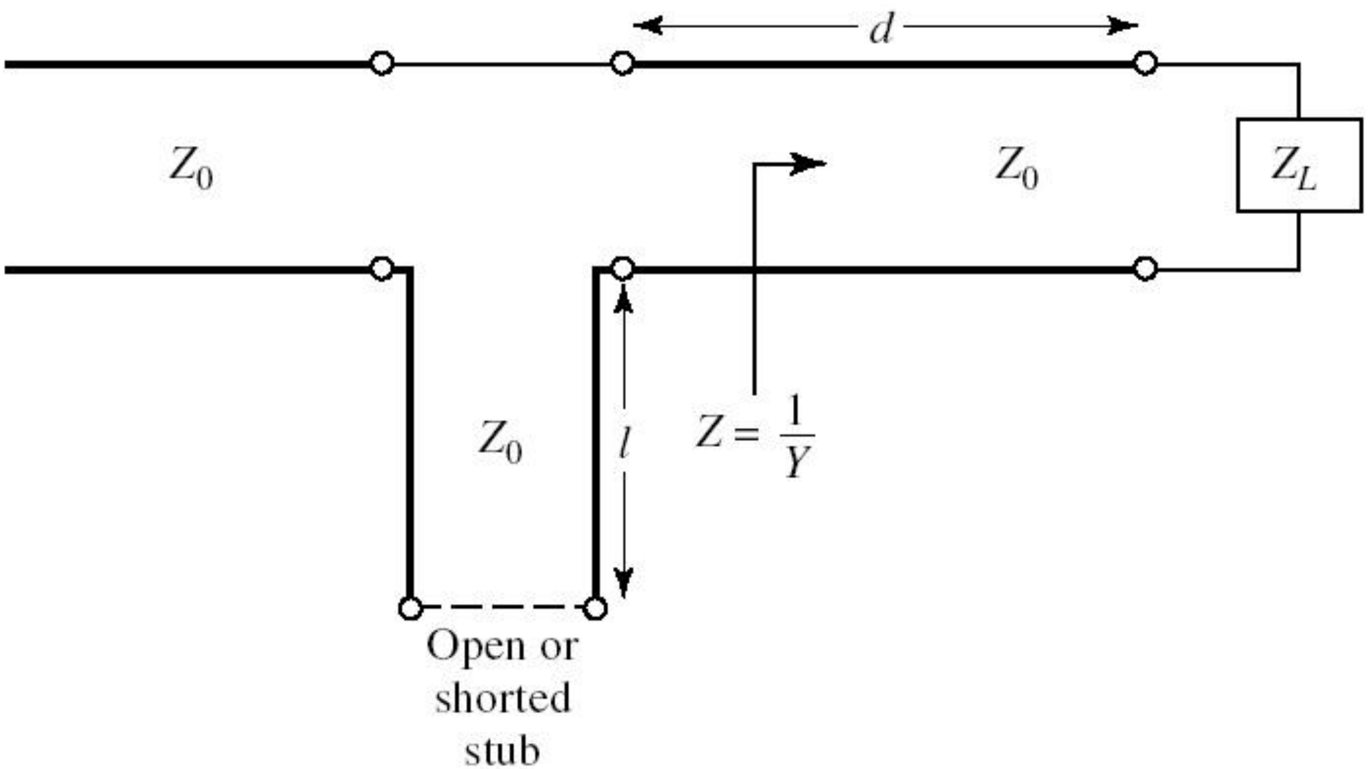
Single stub tuning

- Shunt Stub



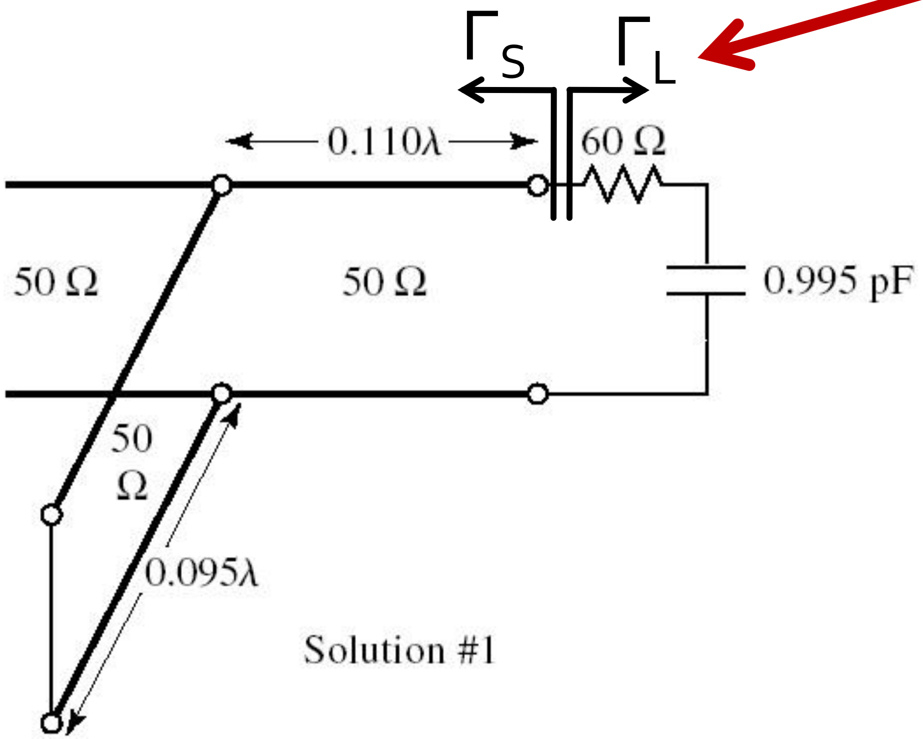
Single stub tuning

- Series Stub
- difficult to realize in single conductor line technologies (microstrip)



Analytical solution, reflection coefficient

- load: 60 Ω series with 0.995 pF at 2GHz



$$Z_L = R_L + \frac{1}{j \cdot \omega \cdot C_L} = 60\Omega - j \cdot 79.977\Omega$$

$$\Gamma_L = \frac{Z_L - Z_0}{Z_L + Z_0} = 0.405 - j \cdot 0.432$$

$$Y_L = \frac{1}{Z_L} = 0.006S + j \cdot 0.008S$$

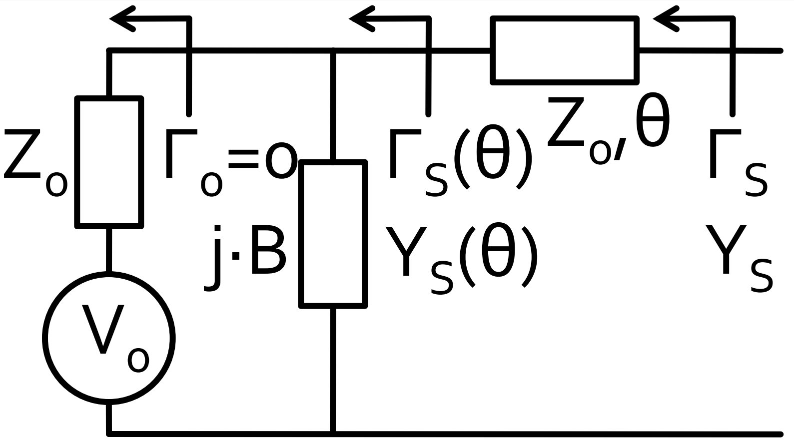
$$y_L = \frac{Y_L}{Y_0} = 0.3 + j \cdot 0.4$$

- matching requires obtaining conjugate value for Γ

$$\Gamma_S = \Gamma_L^* = 0.405 + j \cdot 0.432 \qquad \Gamma_S = 0.593\angle 46.85° \qquad |\Gamma_S| = 0.593; \quad \varphi = 46.85°$$

Analytical solution, Γ

- series line
  - electrical length E= β·l=θ
  - moves the reflection coefficient on the circle g=1
- shunt stub
  - electrical length E= $\beta \cdot l_{sp} = \theta_{sp}$
  - moves the reflection coefficient to the center of the Smith Chart ($\Gamma_0=0$)



$$y_S = \frac{Y_S}{Y_0} = Y_S \cdot Z_0 = Y_S \cdot 50\Omega$$

$$y_S = \frac{1-\Gamma_S}{1+\Gamma_S} = 0.3 - j \cdot 0.4$$

$$\Gamma_S(\theta) = [\Gamma_L(\theta)]^* = \left[\Gamma_L \cdot e^{-2j\theta}\right]^*$$

$$\Gamma_S(\theta) = \Gamma_L^* \cdot e^{2j\theta} = \Gamma_S \cdot e^{2j\theta}$$

$$y_S(\theta) = \frac{1-\Gamma_S(\theta)}{1+\Gamma_S(\theta)} = \frac{1-\Gamma_S \cdot e^{2j\theta}}{1+\Gamma_S \cdot e^{2j\theta}}$$

Analytical solution, Γ, series line

- After the series line with electrical length θ:

$$\mathrm{Re}[y_S(\theta)] = 1 \qquad \mathrm{Im}[y_S(\theta)] = B$$

$$\mathrm{Re}[y_S(\theta)] = \frac{1}{2}\cdot\left[y_S(\theta) + y_S^*(\theta)\right] \qquad \mathrm{Im}[y_S(\theta)] = \frac{1}{2j}\cdot\left[y_S(\theta) - y_S^*(\theta)\right]$$

$$\mathrm{Re}[y_S(\theta)] = \frac{1}{2}\cdot\left[\frac{1-\Gamma_S\cdot e^{2j\theta}}{1+\Gamma_S\cdot e^{2j\theta}} + \frac{1-\Gamma_S^*\cdot e^{-2j\theta}}{1+\Gamma_S^*\cdot e^{-2j\theta}}\right] \qquad \Gamma_S = |\Gamma_S|\cdot e^{j\varphi}$$

$$\mathrm{Re}[y_S(\theta)] = \frac{1}{2}\cdot\left[\frac{\left(1-|\Gamma_S|\cdot e^{j\cdot(\varphi+2\theta)}\right)\cdot\left(1+|\Gamma_S|\cdot e^{-j\cdot(\varphi+2\theta)}\right) + \left(1-|\Gamma_S|\cdot e^{-j\cdot(\varphi+2\theta)}\right)\cdot\left(1+|\Gamma_S|\cdot e^{j\cdot(\varphi+2\theta)}\right)}{\left(1+|\Gamma_S|\cdot e^{-j\cdot(\varphi+2\theta)}\right)\cdot\left(1+|\Gamma_S|\cdot e^{j\cdot(\varphi+2\theta)}\right)}\right]$$

$$\mathrm{Re}[y_S(\theta)] = \frac{1}{2}\cdot\left[\frac{2-2\cdot|\Gamma_S|^2}{1+|\Gamma_S|^2+2\cdot|\Gamma_S|\cdot\cos(\varphi+2\theta)}\right] = 1 \quad \Rightarrow \quad \boxed{\cos(\varphi+2\theta) = -|\Gamma_S|}$$

Analytical solution, Γ, series line

- Equations for computing the series line θ:

$$\mathrm{Re}[y_S(\theta)] = 1 \Rightarrow \qquad \cos(\varphi + 2\theta) = -|\Gamma_S|$$

$$\Gamma_S = |\Gamma_S| \cdot e^{j\varphi} \qquad \Gamma_S = 0.593\angle 46.85^\circ \qquad |\Gamma_S| = 0.593; \quad \varphi = 46.85^\circ$$

- two solutions possible, in the 0÷180° range (add λ/2 ⇔ 180° as needed)

$$\theta = \frac{1}{2} \cdot \left[\pm \cos^{-1}(-|\Gamma_S|) - \varphi + k \cdot 360^\circ\right] = \frac{1}{2} \cdot \left[\pm \cos^{-1}(-|\Gamma_S|) - \varphi\right] + k \cdot 180^\circ$$

$$\forall k \in N$$

$$\cos(\varphi + 2\theta) = -0.593 \Rightarrow \qquad (\varphi + 2\theta) = \pm 126.35^\circ$$

$$(46.85^\circ + 2\theta) = \begin{cases} +126.35^\circ \\ -126.35^\circ \end{cases} \qquad \theta = \begin{cases} +39.7^\circ \\ -86.6^\circ + 180^\circ = +93.4^\circ \end{cases}$$

Analytical solution, Γ, shunt stub

- Equations for computing the shunt stub θ_{sp}:

$$\mathrm{Re}[y_S(\theta)] = 1 \qquad \cos(\varphi + 2\theta) = -|\Gamma_S|$$

$$\mathrm{Im}[y_S(\theta)] = \frac{1}{2j} \cdot \left[\frac{1-\Gamma_S \cdot e^{2j\theta}}{1+\Gamma_S \cdot e^{2j\theta}} - \frac{1-\Gamma_S^* \cdot e^{-2j\theta}}{1+\Gamma_S^* \cdot e^{-2j\theta}} \right] \qquad \Gamma_S = |\Gamma_S| \cdot e^{j\varphi}$$

$$\mathrm{Im}[y_S(\theta)] = \frac{1}{2j} \cdot \left[\frac{\left(1-|\Gamma_S| \cdot e^{j\cdot(\varphi+2\theta)}\right) \cdot \left(1+|\Gamma_S| \cdot e^{-j\cdot(\varphi+2\theta)}\right) - \left(1-|\Gamma_S| \cdot e^{-j\cdot(\varphi+2\theta)}\right) \cdot \left(1+|\Gamma_S| \cdot e^{j\cdot(\varphi+2\theta)}\right)}{\left(1+|\Gamma_S| \cdot e^{-j\cdot(\varphi+2\theta)}\right) \cdot \left(1+|\Gamma_S| \cdot e^{j\cdot(\varphi+2\theta)}\right)} \right]$$

$$\mathrm{Im}[y_S(\theta)] = \frac{1}{2j} \cdot \left[\frac{2 \cdot |\Gamma_S| \cdot e^{-j\cdot(\varphi+2\theta)} - 2 \cdot |\Gamma_S| \cdot e^{+j\cdot(\varphi+2\theta)}}{1+|\Gamma_S|^2 + 2 \cdot |\Gamma_S| \cdot \cos(\varphi+2\theta)} \right] = \frac{-2 \cdot |\Gamma_S| \cdot \sin(\varphi+2\theta)}{1+|\Gamma_S|^2 + 2 \cdot |\Gamma_S| \cdot \cos(\varphi+2\theta)}$$

$$\cos(\varphi + 2\theta) = -|\Gamma_S| \Rightarrow \qquad \mathrm{Im}[y_S(\theta)] = \frac{-2 \cdot |\Gamma_S| \cdot \sin(\varphi+2\theta)}{1-|\Gamma_S|^2}$$

Analytical solution, Γ, shunt stub

- Equations for computing the shunt stub

$$\cos(\varphi + 2\theta) = -|\Gamma_S| \Rightarrow \qquad \sin(\varphi + 2\theta) = \pm\sqrt{1 - |\Gamma_S|^2}$$

$$\mathrm{Im}[y_S(\theta)] = \frac{-2 \cdot |\Gamma_S| \cdot \sin(\varphi + 2\theta)}{1 - |\Gamma_S|^2} \Rightarrow \qquad \mathrm{Im}[y_S(\theta)] = \frac{\mp 2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}}$$

- two cases

$$\varphi + 2\theta \in [0°, 180°] \Rightarrow \sin(\varphi + 2\theta) \geq 0 \quad \begin{cases} \sin(\varphi + 2\theta) = \sqrt{1 - |\Gamma_S|^2} \\ \mathrm{Im}[y_S(\theta)] = \dfrac{-2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} \end{cases}$$

$$\varphi + 2\theta \in (-180°, 0°) \Rightarrow \sin(\varphi + 2\theta) < 0 \quad \begin{cases} \sin(\varphi + 2\theta) = -\sqrt{1 - |\Gamma_S|^2} \\ \mathrm{Im}[y_S(\theta)] = \dfrac{2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} \end{cases}$$

- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **shunt stub** equation

Analytical solution, Γ, shunt stub

- We prefer (for microstrip) open circuited stub

$$Z_{in,oc} = -j \cdot Z_0 \cdot \cot \beta \cdot l$$

- The normalized susceptance to be introduced to achieve the match
  - Y(θ) is the admittance seen **towards** the source, Zo parallel with j·B

$$b = \mathrm{Im}\left[\frac{Y_{in,oc}}{Y_0}\right] = \mathrm{Im}\left[\frac{Z_0}{Z_{in,oc}}\right] = \tan \beta \cdot l = \mathrm{Im}\left[y_S(\theta)\right]$$

$$\boxed{\theta_{sp} = \beta \cdot l = \tan^{-1} \frac{\mp 2 \cdot |\Gamma_S|}{\sqrt{1-|\Gamma_S|^2}}}$$

Analytical solution, Γ

$$\cos(\varphi + 2\theta) = -|\Gamma_S|$$

$$\theta_{sp} = \beta \cdot l = \tan^{-1} \frac{\mp 2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}}$$

$$\Gamma_S = 0.593\angle 46.85°$$

$$|\Gamma_S| = 0.593; \quad \varphi = 46.85° \qquad \cos(\varphi + 2\theta) = -0.593 \Rightarrow (\varphi + 2\theta) = \pm 126.35°$$

- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **shunt stub** equation
  - **"+" solution**

    $$(46.85° + 2\theta) = +126.35° \qquad \theta = +39.7° \qquad \operatorname{Im} y_S = \frac{-2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} = -1.472$$

    $$\theta_{sp} = \tan^{-1}(\operatorname{Im} y_S) = -55.8°(+180°) \to \theta_{sp} = 124.2°$$

  - **"-" solution**

    $$(46.85° + 2\theta) = -126.35° \qquad \theta = -86.6°(+180°) \to \theta = 93.4°$$

    $$\operatorname{Im} y_S = \frac{+2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} = +1.472 \qquad \theta_{sp} = \tan^{-1}(\operatorname{Im} y_S) = 55.8°$$

Analytical solution, Γ

$$(\varphi+2\theta)=\begin{cases}+126.35^\circ\\-126.35^\circ\end{cases}\quad \theta=\begin{cases}39.7^\circ\\93.4^\circ\end{cases}\quad \mathrm{Im}\left[y_S(\theta)\right]=\begin{cases}-1.472\\+1.472\end{cases}\quad \theta_{sp}=\begin{cases}-55.8^\circ+180^\circ=124.2^\circ\\+55.8^\circ\end{cases}$$

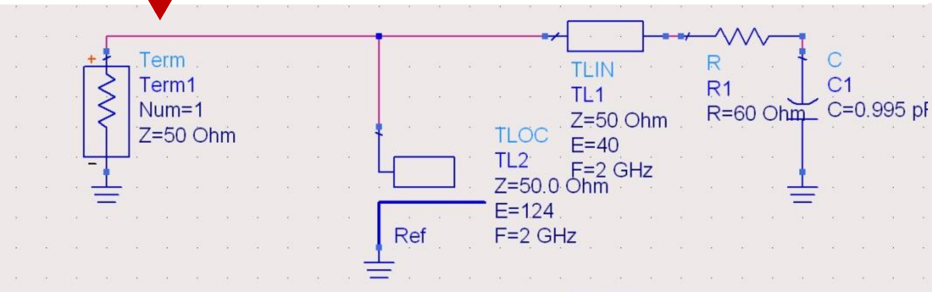
- We choose **one** of the two possible solutions
- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **shunt stub** equation

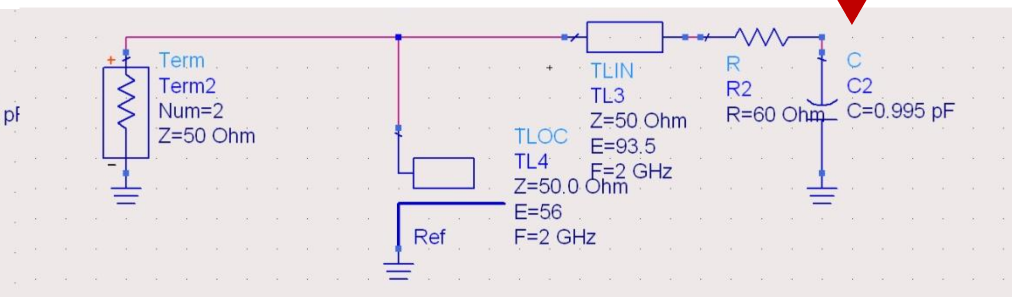
$$l_1=\frac{39.7^\circ}{360^\circ}\cdot\lambda=0.110\cdot\lambda$$

$$l_2=\frac{124.2^\circ}{360^\circ}\cdot\lambda=0.345\cdot\lambda$$

$$l_1=\frac{93.4^\circ}{360^\circ}\cdot\lambda=0.259\cdot\lambda$$

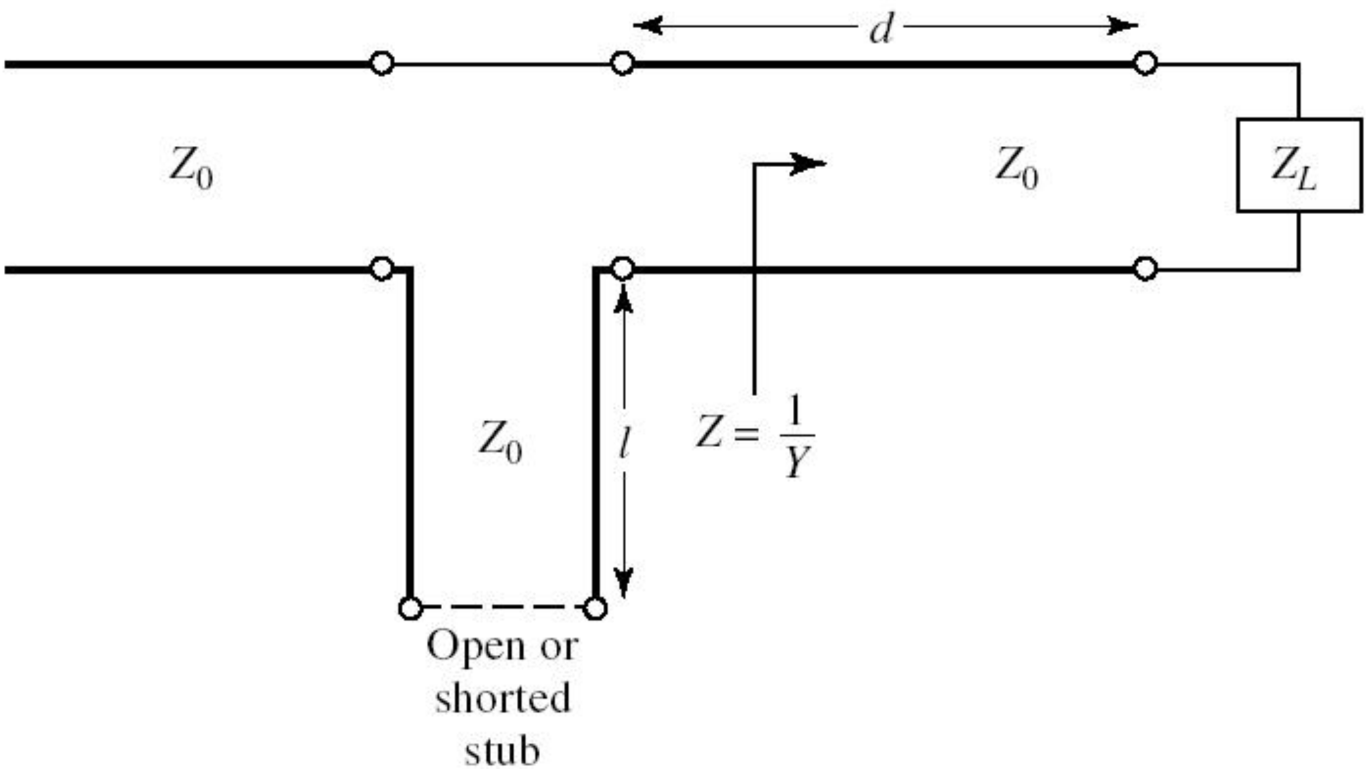
$$l_2=\frac{55.8^\circ}{360^\circ}\cdot\lambda=0.155\cdot\lambda$$





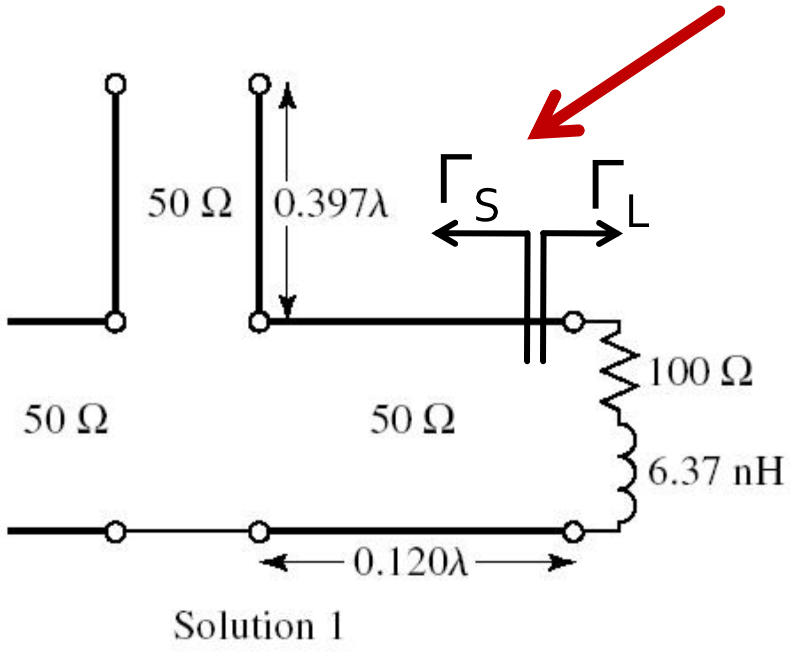
Case 2, Series Stub

- Series Stub
- difficult to realize in single conductor line technologies (microstrip)



Analytical solution, reflection coefficient

- load: 100 Ω series with 6.37 nH at 2 GHz



$$Z_L = R_L + \frac{1}{j \cdot \omega \cdot C_L} = 100\Omega + j \cdot 80.05\Omega$$

$$\Gamma_L = \frac{Z_L - Z_0}{Z_L + Z_0} = 0.481 + j \cdot 0.277$$

$$z_L = \frac{Z_L}{Z_0} = 2 + j \cdot 1.6$$

- matching requires obtaining conjugate value for Γ

$$\Gamma_S = \Gamma_L^* = 0.481 - j \cdot 0.277$$

$$\Gamma_S = 0.555\angle -29.92^\circ \qquad |\Gamma_S| = 0.555; \quad \varphi = -29.92^\circ$$

Analytical solution, Γ

$$\cos(\varphi + 2\theta) = |\Gamma_S|$$

$$\theta_{ss} = \beta \cdot l = \cot^{-1} \frac{\mp 2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}}$$

$$\Gamma_S = 0.555\angle -29.92°$$

$$|\Gamma_S| = 0.555; \quad \varphi = -29.92° \qquad \cos(\varphi + 2\theta) = 0.555 \Rightarrow (\varphi + 2\theta) = \pm 56.28°$$

- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **series stub** equation
  - **"+" solution**

$$(-29.92° + 2\theta) = +56.28° \qquad \theta = 43.1° \qquad \operatorname{Im} z_S = \frac{+2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} = +1.335$$

$$\theta_{ss} = -\cot^{-1}(\operatorname{Im} z_S) = -36.8° (+180°) \rightarrow \theta_{ss} = 143.2°$$

  - **"-" solution**

$$(-29.92° + 2\theta) = -56.28° \qquad \theta = -13.2° (+180°) \rightarrow \theta = 166.8°$$

$$\operatorname{Im} z_S = \frac{-2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} = -1.335 \qquad \theta_{ss} = -\cot^{-1}(\operatorname{Im} z_S) = 36.8°$$

Analytical solution, Γ

$$(\varphi+2\theta)=\begin{cases}+56.28^\circ\\-56.28^\circ\end{cases}\quad \theta=\begin{cases}43.1^\circ\\166.8^\circ\end{cases}\quad \mathrm{Im}[z_S(\theta)]=\begin{cases}+1.335\\-1.335\end{cases}\quad \theta_{ss}=\begin{cases}-36.8^\circ+180^\circ=143.2^\circ\\+36.8^\circ\end{cases}$$

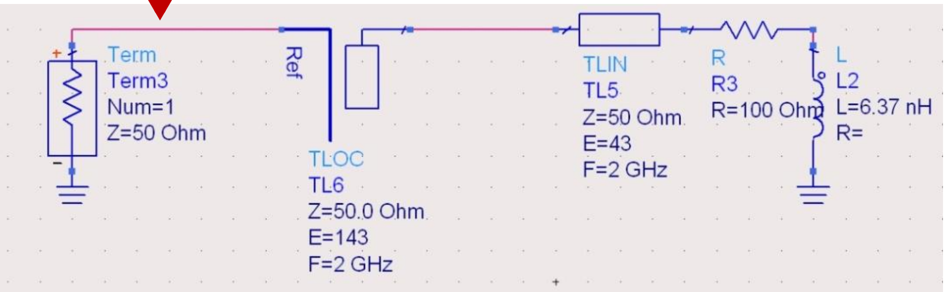
- We choose **one** of the two possible solutions
- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **series stub** equation

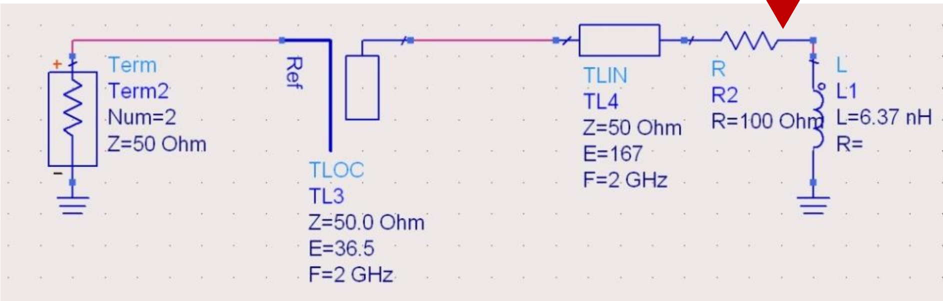
$$l_1=\frac{43.1^\circ}{360^\circ}\cdot\lambda=0.120\cdot\lambda$$

$$l_2=\frac{143.2^\circ}{360^\circ}\cdot\lambda=0.398\cdot\lambda$$

$$l_1=\frac{166.8^\circ}{360^\circ}\cdot\lambda=0.463\cdot\lambda$$

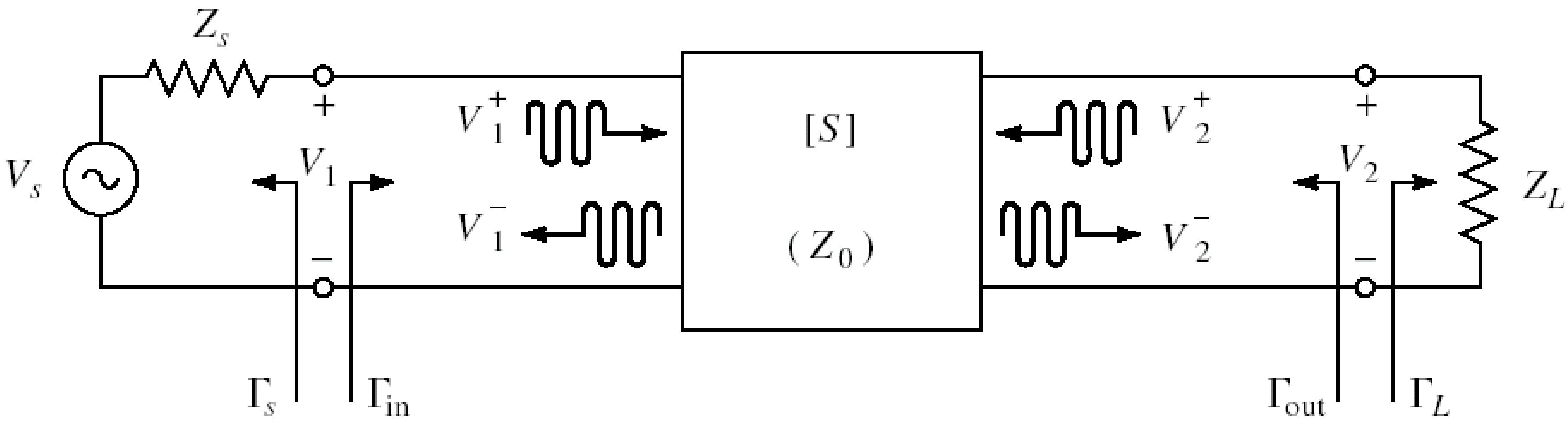
$$l_2=\frac{36.8^\circ}{360^\circ}\cdot\lambda=0.102\cdot\lambda$$





Microwave Amplifiers

Amplifier as two-port



- Charaterized with S parameters
- normalized at Zo (implicit 50Ω)
- Datasheets: S parameters for specific bias conditions

Datasheets

NE46100

V_{CE} = 5 V, I_C = 50 mA

FREQUENCY (MHz)	S11 MAG	S11 ANG	S21 MAG	S21 ANG	S12 MAG	S12 ANG	S22 MAG	S22 ANG	K	MAG[2] (dB)
100	0.778	-137	26.776	114	0.028	30	0.555	-102	0.16	29.8
200	0.815	-159	14.407	100	0.035	29	0.434	-135	0.36	26.2
500	0.826	-177	5.855	84	0.040	38	0.400	-162	0.75	21.7
800	0.827	176	3.682	76	0.052	43	0.402	-169	0.91	18.5
1000	0.826	173	2.963	71	0.058	47	0.405	-172	1.02	16.3
1200	0.825	170	2.441	66	0.064	47	0.412	-174	1.08	14.0
1400	0.820	167	2.111	61	0.069	47	0.413	-176	1.17	12.4
1600	0.828	165	1.863	57	0.078	54	0.426	-177	1.15	11.4
1800	0.827	162	1.671	53	0.087	50	0.432	-178	1.14	10.6
2000	0.828	159	1.484	49	0.093	50	0.431	-180	1.17	9.5
2500	0.822	153	1.218	39	0.11	48	0.462	177	1.18	7.8
3000	0.818	148	1.010	30	0.135	46	0.490	174	1.16	6.3
3500	0.824	142	0.876	21	0.147	44	0.507	170	1.16	5.3
4000	0.812	137	0.762	13	0.168	38	0.535	167	1.14	4.3

V_{CE} = 5 V, I_C = 100 mA

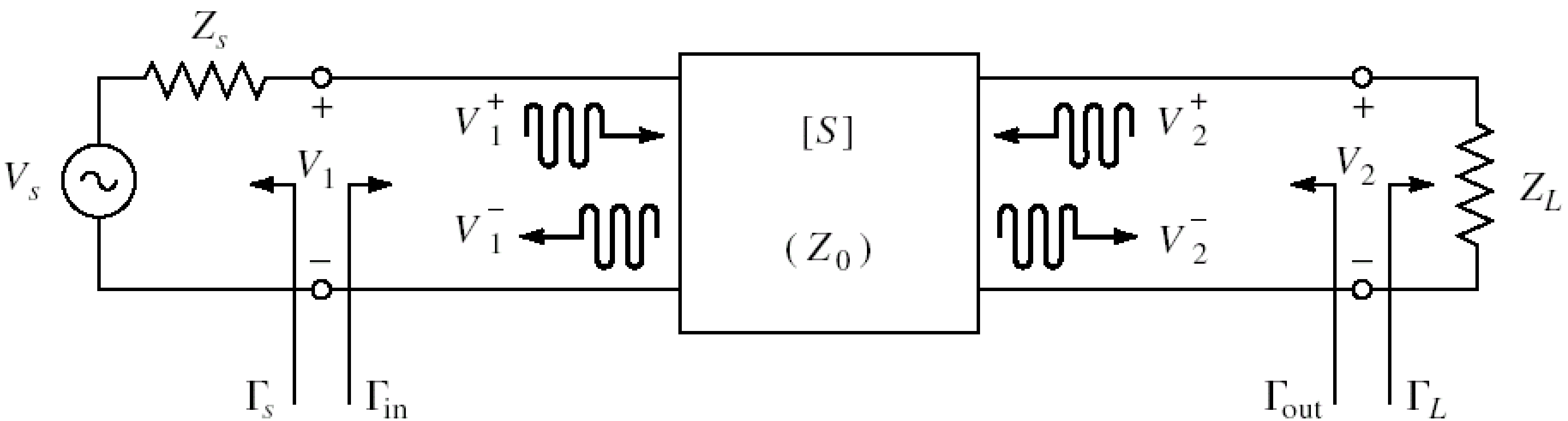
FREQUENCY (MHz)	S11 MAG	S11 ANG	S21 MAG	S21 ANG	S12 MAG	S12 ANG	S22 MAG	S22 ANG	K	MAG[2] (dB)
100	0.778	-144	27.669	111	0.027	35	0.523	-114	0.27	30.2
200	0.820	-164	14.559	97	0.029	29	0.445	-144	0.42	27.0
500	0.832	-179	5.885	84	0.035	38	0.435	-166	0.81	22.2
800	0.833	175	3.691	76	0.048	45	0.435	-173	0.95	18.8
1000	0.831	172	2.980	71	0.056	51	0.437	-176	1.05	16.0
1200	0.836	169	2.464	67	0.061	52	0.432	-178	1.11	14.0
1400	0.829	166	2.121	61	0.072	53	0.447	-180	1.12	12.6
1600	0.831	164	1.867	58	0.080	54	0.445	179	1.14	11.4

S2P - Touchstone

- Touchstone file format (*.s2p)

```
! SIEMENS Small Signal Semiconductors
! VDS = 3.5 V     ID = 15 mA
# GHz  S  MA  R  50
!  f        S11          S21          S12          S22
! GHz     MAG   ANG     MAG   ANG     MAG   ANG     MAG   ANG
 1.000 0.9800  -18.0   2.230  157.0  0.0240   74.0  0.6900  -15.0
 2.000 0.9500  -39.0   2.220  136.0  0.0450   57.0  0.6600  -30.0
 3.000 0.8900  -64.0   2.210  110.0  0.0680   40.0  0.6100  -45.0
 4.000 0.8200  -89.0   2.230   86.0  0.0850   23.0  0.5600  -62.0
 5.000 0.7400 -115.0   2.190   61.0  0.0990    7.0  0.4900  -80.0
 6.000 0.6500 -142.0   2.110   36.0  0.1070  -10.0  0.4100  -98.0
!
!  f       Fmin   Gammaopt  rn/50
! GHz       dB    MAG  ANG    -
 2.000     1.00  0.72   27   0.84
 4.000     1.40  0.64   61   0.58
```

Amplifier as two-port



$$\Gamma_{in} = S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L}$$

$$\Gamma_{out} = S_{22} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_S}{1 - S_{11} \cdot \Gamma_S}$$

Two-Port Power Gains

- Power Gain

$$G=\frac{P_L}{P_{in}}=\frac{|S_{21}|^2\cdot\left(1-|\Gamma_L|^2\right)}{\left(1-|\Gamma_{in}|^2\right)\cdot|1-S_{22}\cdot\Gamma_L|^2}$$

$$P_{in}=P_{in}(\Gamma_S,\Gamma_{in}(\Gamma_L),S)$$

$$P_L=P_L(\Gamma_S,\Gamma_{in}(\Gamma_L),S)$$

- The **actual** power gain **introduced** by the amplifier is less important because a higher gain may be accompanied by a **decrease** in input power (power actually drained from the source)
- We prefer to characterize the amplifier effect looking to the **power actually delivered to the load** in relation to the power **available from the source** (which is a constant)

Two-Port Power Gains

- **Available** power gain

$$G_A = \frac{P_{av\,L}}{P_{av\,S}} = \frac{|S_{21}|^2 \cdot \left(1-|\Gamma_S|^2\right)}{|1-S_{22}\cdot\Gamma_L|^2 \cdot \left(1-|\Gamma_{out}|^2\right)}$$

- **Transducer** power gain

$$G_T = \frac{P_L}{P_{av\,S}} = \frac{|S_{21}|^2 \cdot \left(1-|\Gamma_S|^2\right)\cdot\left(1-|\Gamma_L|^2\right)}{|1-\Gamma_S\cdot\Gamma_{in}|^2 \cdot |1-S_{22}\cdot\Gamma_L|^2}$$

$$\Gamma_{in} = \Gamma_{in}(\Gamma_L)$$

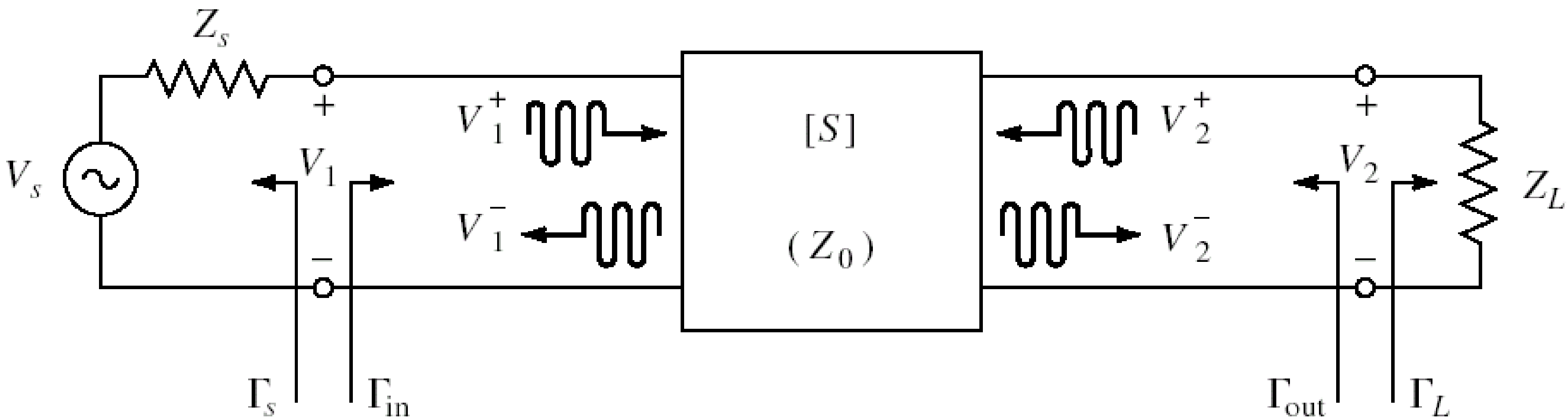
- **Unilateral transducer** power gain

$$G_{TU} = |S_{21}|^2 \cdot \frac{1-|\Gamma_S|^2}{|1-S_{11}\cdot\Gamma_S|^2} \cdot \frac{1-|\Gamma_L|^2}{|1-S_{22}\cdot\Gamma_L|^2}$$

$$S_{12} \cong 0 \qquad \Gamma_{in} = S_{11}$$

Input and output can be treated independently

Amplifier as two-port



- For an amplifier two-port we are interested in:
  - stability
  - power gain
  - noise (sometimes – small signals)
  - linearity (sometimes – large signals)

Stability

Microwave Amplifiers

Stability

- C6 $\Gamma = \Gamma_r + j \cdot \Gamma_i$ $r_L = \frac{1 - \Gamma_r^2 - \Gamma_i^2}{(1 - \Gamma_r)^2 + \Gamma_i^2}$

  Z_{in} $\Gamma_{in} = \Gamma_r + j \cdot \Gamma_i$
- instability

  $\mathrm{Re}\{Z_{in}\} < 0 \iff 1 - \Gamma_r^2 - \Gamma_i^2 < 0$ $|\Gamma_{in}| > 1$
- stability, Z_{in}
  - conditions to be met by Γ_L to achieve (input) stability

    $|\Gamma_{in}| < 1$ $\left| S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L} \right| < 1$
- similarly Z_{out}
  - conditions to be met by Γ_S to achieve (output) stability

Stability

$$|\Gamma_{in}| < 1 \qquad \left| S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L} \right| < 1$$

- We can calculate conditions to be met by Γ_L to achieve stability

$$|\Gamma_{out}| < 1 \qquad \left| S_{22} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_S}{1 - S_{11} \cdot \Gamma_S} \right| < 1$$

- We can calculate conditions to be met by Γ_S to achieve stability

Stability

$$|\Gamma_{in}| < 1 \qquad \left| S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L} \right| < 1$$

- The limit between stability/instability

$$|\Gamma_{in}| = 1 \qquad \left| S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L} \right| = 1$$

$$|S_{11} \cdot (1 - S_{22} \cdot \Gamma_L) + S_{12} \cdot S_{21} \cdot \Gamma_L| = |1 - S_{22} \cdot \Gamma_L|$$

- determinant of the S matrix $\Delta = S_{11} \cdot S_{22} - S_{12} \cdot S_{21}$

$$|S_{11} - \Delta \cdot \Gamma_L| = |1 - S_{22} \cdot \Gamma_L|$$

$$|S_{11} - \Delta \cdot \Gamma_L|^2 = |1 - S_{22} \cdot \Gamma_L|^2$$

Stability

$$\left|S_{11}-\Delta\cdot\Gamma_L\right|^2=\left|1-S_{22}\cdot\Gamma_L\right|^2$$

$$a\cdot a^*=|a|\cdot e^{j\theta}\cdot|a|\cdot e^{-j\theta}=|a|^2$$

$$|a+b|^2=(a+b)\cdot(a+b)^*=(a+b)\cdot\left(a^*+b^*\right)=|a|^2+|b|^2+a^*\cdot b+a\cdot b^*$$

$$|S_{11}|^2+|\Delta|^2\cdot|\Gamma_L|^2-\left(\Delta\cdot\Gamma_L\cdot S_{11}^*+\Delta^*\cdot\Gamma_L^*\cdot S_{11}\right)=1+|S_{22}|^2\cdot|\Gamma_L|^2-\left(S_{22}^*\cdot\Gamma_L^*+S_{22}\cdot\Gamma_L\right)$$

$$\left(|S_{22}|^2-|\Delta|^2\right)\cdot\Gamma_L\cdot\Gamma_L^*-\left(S_{22}-\Delta\cdot S_{11}^*\right)\cdot\Gamma_L-\left(S_{22}^*-\Delta^*\cdot S_{11}\right)\cdot\Gamma_L^*=|S_{11}|^2-1$$

$$\Gamma_L\cdot\Gamma_L^*-\frac{\left(S_{22}-\Delta\cdot S_{11}^*\right)\cdot\Gamma_L+\left(S_{22}^*-\Delta^*\cdot S_{11}\right)\cdot\Gamma_L^*}{|S_{22}|^2-|\Delta|^2}=\frac{|S_{11}|^2-1}{|S_{22}|^2-|\Delta|^2}+\frac{\left|S_{22}-\Delta\cdot S_{11}^*\right|^2}{\left(|S_{22}|^2-|\Delta|^2\right)^2}$$

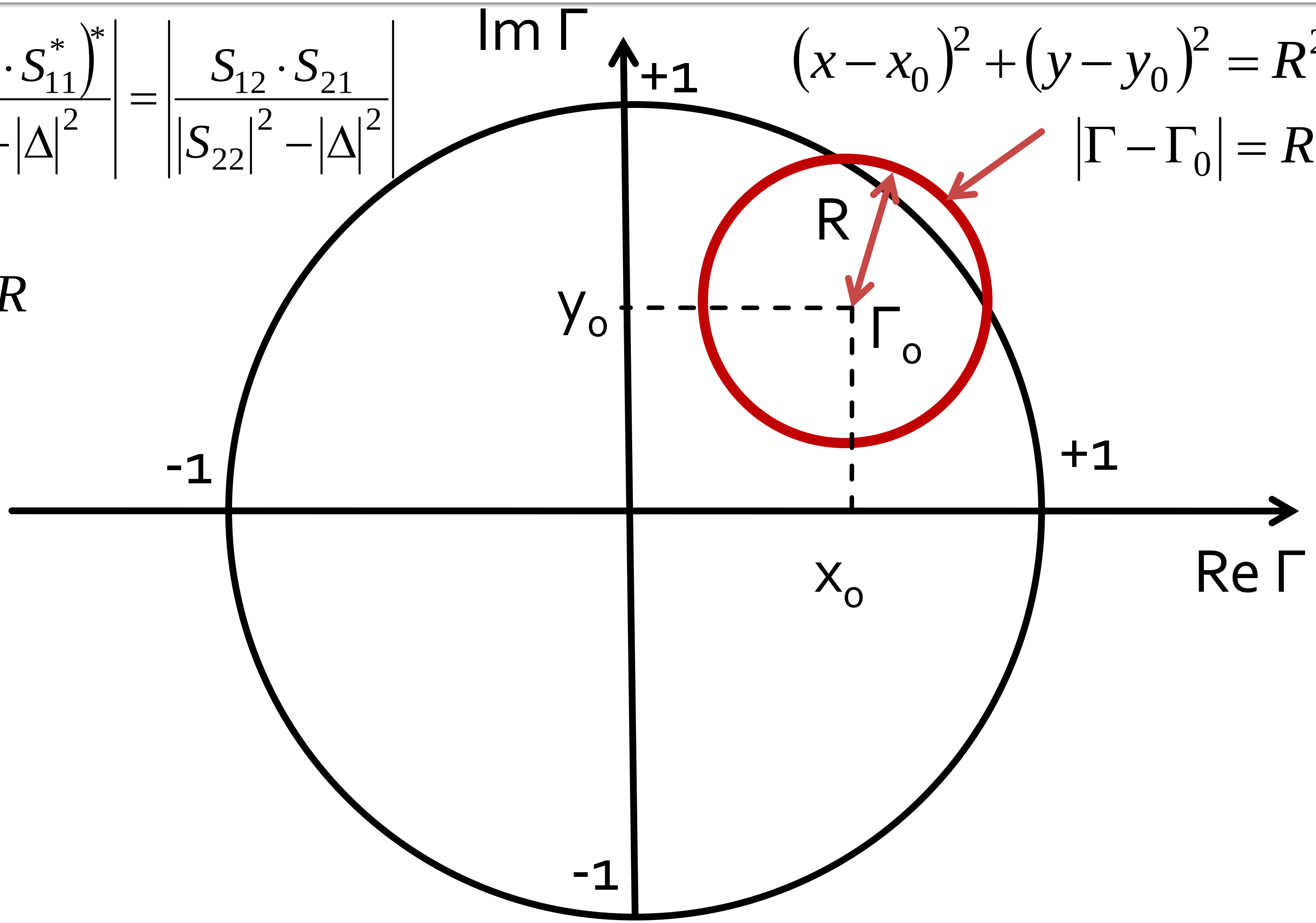
$$\left|\Gamma_L-\frac{\left(S_{22}-\Delta\cdot S_{11}^*\right)^*}{|S_{22}|^2-|\Delta|^2}\right|^2=\frac{|S_{11}|^2-1}{|S_{22}|^2-|\Delta|^2}+\frac{\left|S_{22}-\Delta\cdot S_{11}^*\right|^2}{\left(|S_{22}|^2-|\Delta|^2\right)^2}$$

Stability

$$\left| \Gamma_L - \frac{\left(S_{22} - \Delta \cdot S_{11}^*\right)^*}{|S_{22}|^2 - |\Delta|^2} \right| = \left| \frac{S_{12} \cdot S_{21}}{|S_{22}|^2 - |\Delta|^2} \right|$$

$$|\Gamma - \Gamma_0| = R$$

$$(x - x_0)^2 + (y - y_0)^2 = R^2$$



Output stability circle (CSOUT)

$$\left|\Gamma_L - \frac{\left(S_{22} - \Delta \cdot S_{11}^*\right)^*}{|S_{22}|^2 - |\Delta|^2}\right| = \left|\frac{S_{12} \cdot S_{21}}{|S_{22}|^2 - |\Delta|^2}\right| \qquad |\Gamma_L - C_L| = R_L$$

- We obtain the equation of a circle in the complex plane, which represents the locus of Γ_L for the **limit between stability and instability** ($|\Gamma_{in}| = 1$)
- This circle is the **output stability circle** (Γ_L)

$$C_L = \frac{\left(S_{22} - \Delta \cdot S_{11}^*\right)^*}{|S_{22}|^2 - |\Delta|^2} \qquad R_L = \frac{|S_{12} \cdot S_{21}|}{\left||S_{22}|^2 - |\Delta|^2\right|}$$

Input stability circle (CSOUT)

- Similarly

$$|\Gamma_{out}| = 1 \qquad \left| S_{22} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_S}{1 - S_{11} \cdot \Gamma_S} \right| = 1$$

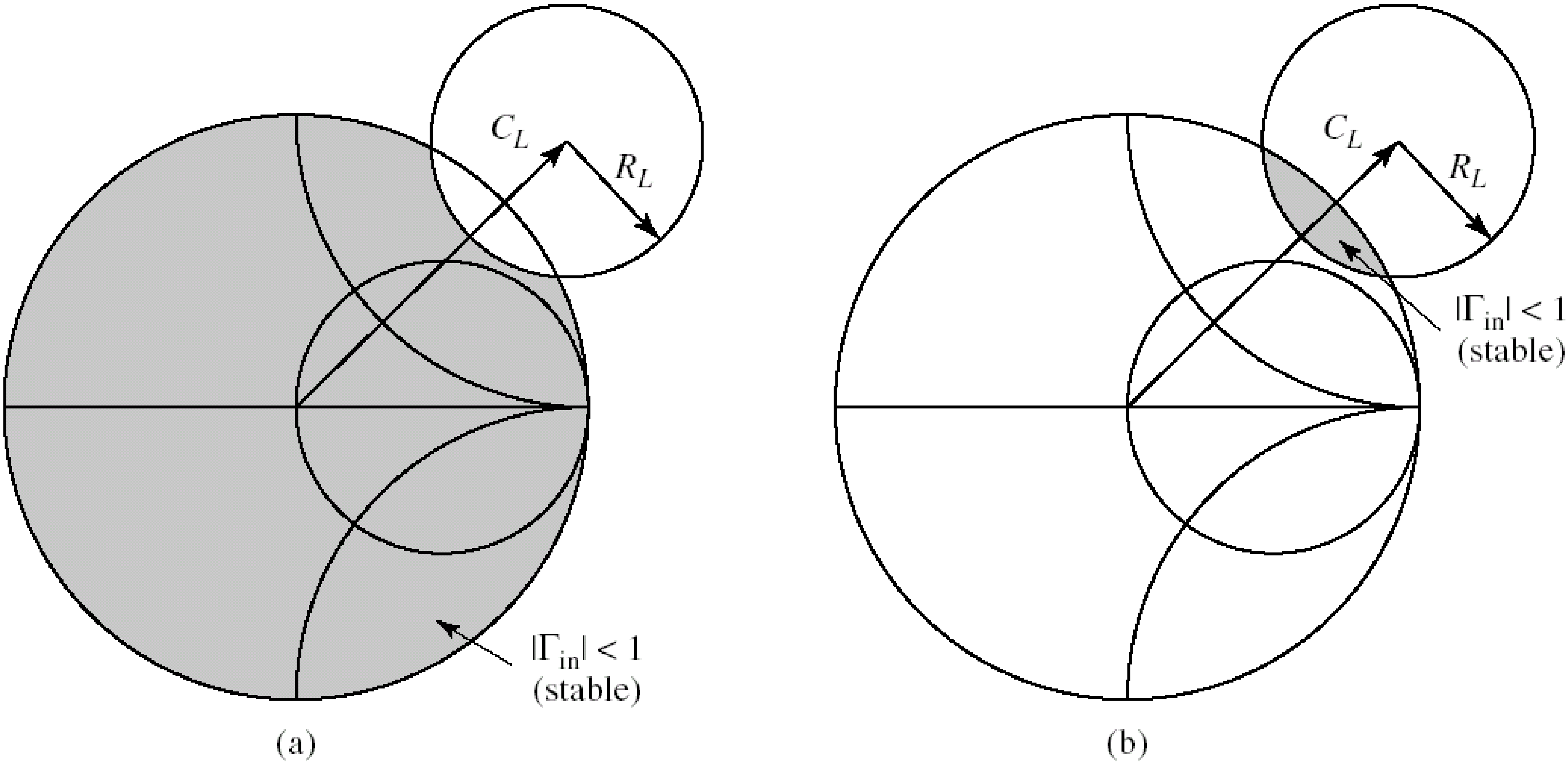
- We obtain the equation of a circle in the complex plane, which represents the locus of Γ_S for the **limit between stability and instability** ($|\Gamma_{out}| = 1$)
- This circle is the **input stability circle** (Γ_S)

$$C_S = \frac{\left(S_{11} - \Delta \cdot S_{22}^*\right)^*}{|S_{11}|^2 - |\Delta|^2} \qquad R_S = \frac{|S_{12} \cdot S_{21}|}{\left| |S_{11}|^2 - |\Delta|^2 \right|}$$

Output stability circle (CSOUT)

- The **output stability circle** represents the locus of Γ_L for the **limit between stability and instability** ($|\Gamma_{in}| = 1$)
- The circle divides the complex planes in two areas, the **inside** and the **outside** of the circle
- The two areas will represent the locus of Γ_L for stability ($|\Gamma_{in}|<1$) / instability ($|\Gamma_{in}|>1$)

Output stability circle (CSOUT)



- Two cases possible: (a) stable outside/ (b) stable inside

Output stability circle (CSOUT)

- Identification of the stability / instability regions
  - Center of the Smith Chart in Γ_L complex plane correspond to $\Gamma_L = 0$
  - Input reflection coefficient

$$\Gamma_{in} = S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L} \qquad \Gamma_{in}\big|_{\Gamma_L = 0} = S_{11} \qquad \left|\Gamma_{in}\right|_{\Gamma_L = 0} = \left|S_{11}\right|$$

  - A decision can be made based on |S11| value the position of the center of the Smith chart (origin of the complex plane) relative to the circle

Identification of the stability / instability regions

- Output stability circle
  - **|S11| < 1** → the center of the Smith chart on which Γ_L is represented is a **stable point**, so it's placed in the stability region (most often situation)
  - |S11| > 1 → the center of the Smith chart on which Γ_L is represented is a **unstable point**, so it's placed in the instability region
- Input stability circle
  - **|S22| < 1** → the center of the Smith chart on which Γ_S is represented is a **stable point**, so it's placed in the stability region (most often situation)
  - |S22| > 1 → the center of the Smith chart on which Γ_S is represented is a **unstable point**, so it's placed in the instability region

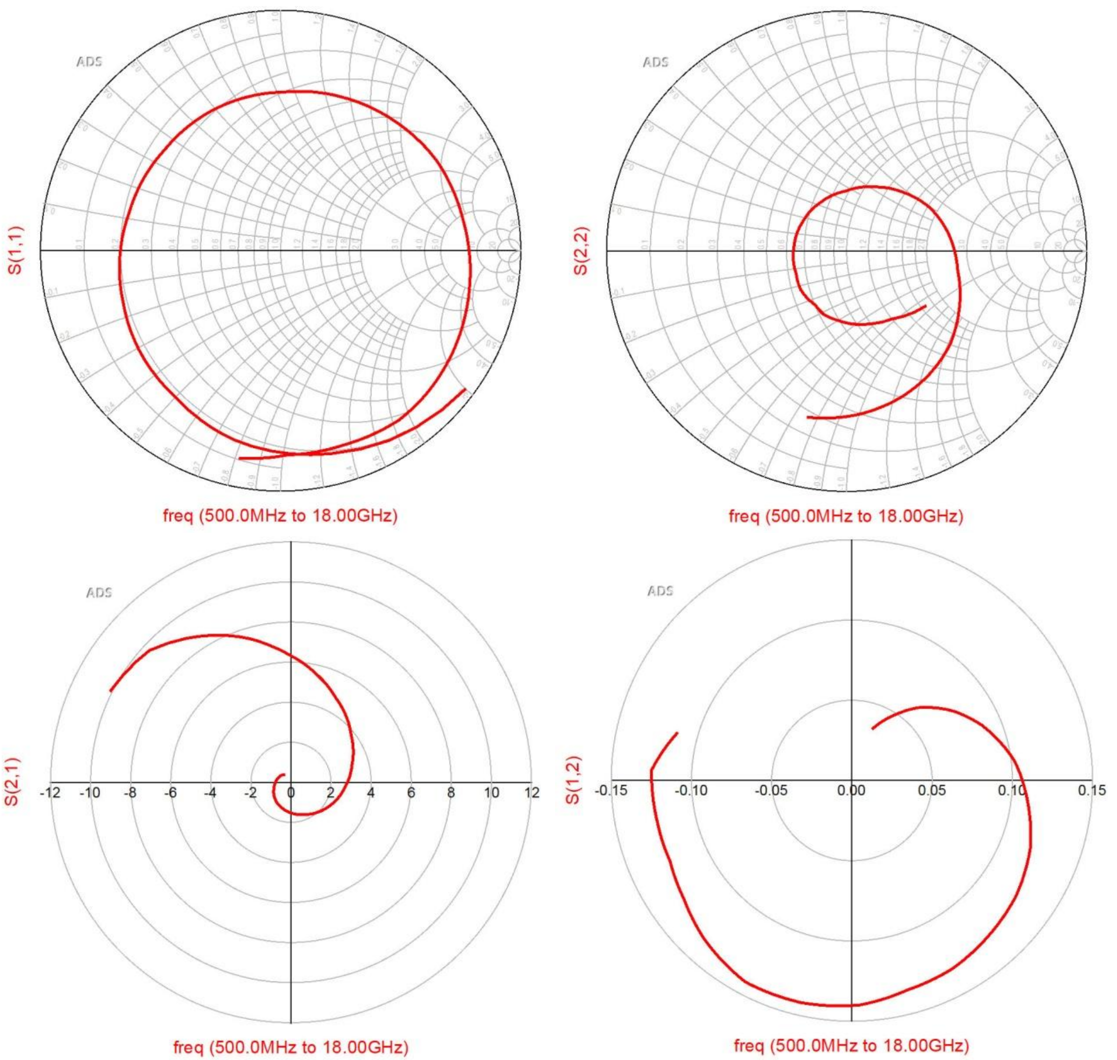
Example

- ATF-34143 **at Vds=3V Id=20mA.**
- @5GHz
  - $S_{11} = 0.64\angle 139°$
  - $S_{12} = 0.119\angle -21°$
  - $S_{21} = 3.165\angle 16°$
  - $S_{22} = 0.22\angle 146°$

```
!ATF-34143
!S-PARAMETERS at Vds=3V  Id=20mA.   LAST UPDATED 01-29-99

# ghz s ma r 50

2.0  0.75  -126  6.306  90  0.088  23  0.26  -120
2.5  0.72  -145  5.438  75  0.095  15  0.25  -140
3.0  0.69  -162  4.762  62  0.102  7  0.23  -156
4.0  0.65  166  3.806  38  0.111  -8  0.22  174
5.0  0.64  139  3.165  16  0.119  -21  0.22  146
6.0  0.65  114  2.706  -5  0.125  -35  0.23  118
7.0  0.66  89  2.326  -27  0.129  -49  0.25  91
8.0  0.69  67  2.017  -47  0.133  -62  0.29  67
9.0  0.72  48  1.758  -66  0.135  -75  0.34  46

!FREQ   Fopt    GAMMA OPT       RN/Zo
!GHZ     dB     MAG     ANG       -

2.0  0.19  0.71  66  0.09
2.5  0.23  0.65  83  0.07
3.0  0.29  0.59  102  0.06
4.0  0.42  0.51  138  0.03
5.0  0.54  0.45  174  0.03
6.0  0.67  0.42  -151  0.05
7.0  0.79  0.42  -118  0.10
8.0  0.92  0.45  -88  0.18
9.0  1.04  0.51  -63  0.30
10.0  1.16  0.61  -43  0.46
```

Example

- ATF-34143
- **at**
  - **Vds=3V**
  - **Id=20mA.**



Solution + region identification

- S parameters
  - $S_{11} = -0.483+0.42\cdot j$
  - $S_{12} = 0.111-0.043\cdot j$
  - $S_{21} = 3.042+0.872\cdot j$
  - $S_{22} = -0.182+0.123\cdot j$
- $|S_{22}| < 1$
- $|C_L| < R_L$, $0 \in CSOUT$
- The center of the Smith chart is placed inside the output stability circle ($0 \in CSOUT$) and is a stable point
  - the inside of the output stability circle – stability region
  - the outside of the output stability circle – instability region

$$C_L = \frac{\left(S_{22} - \Delta \cdot S_{11}^*\right)^*}{|S_{22}|^2 - |\Delta|^2} = 3.931 - 0.897 \cdot j$$

$$|C_L| = 4.032$$

$$R_L = \frac{|S_{12} \cdot S_{21}|}{\left||S_{22}|^2 - |\Delta|^2\right|} = 4.891$$

Solution + region identification

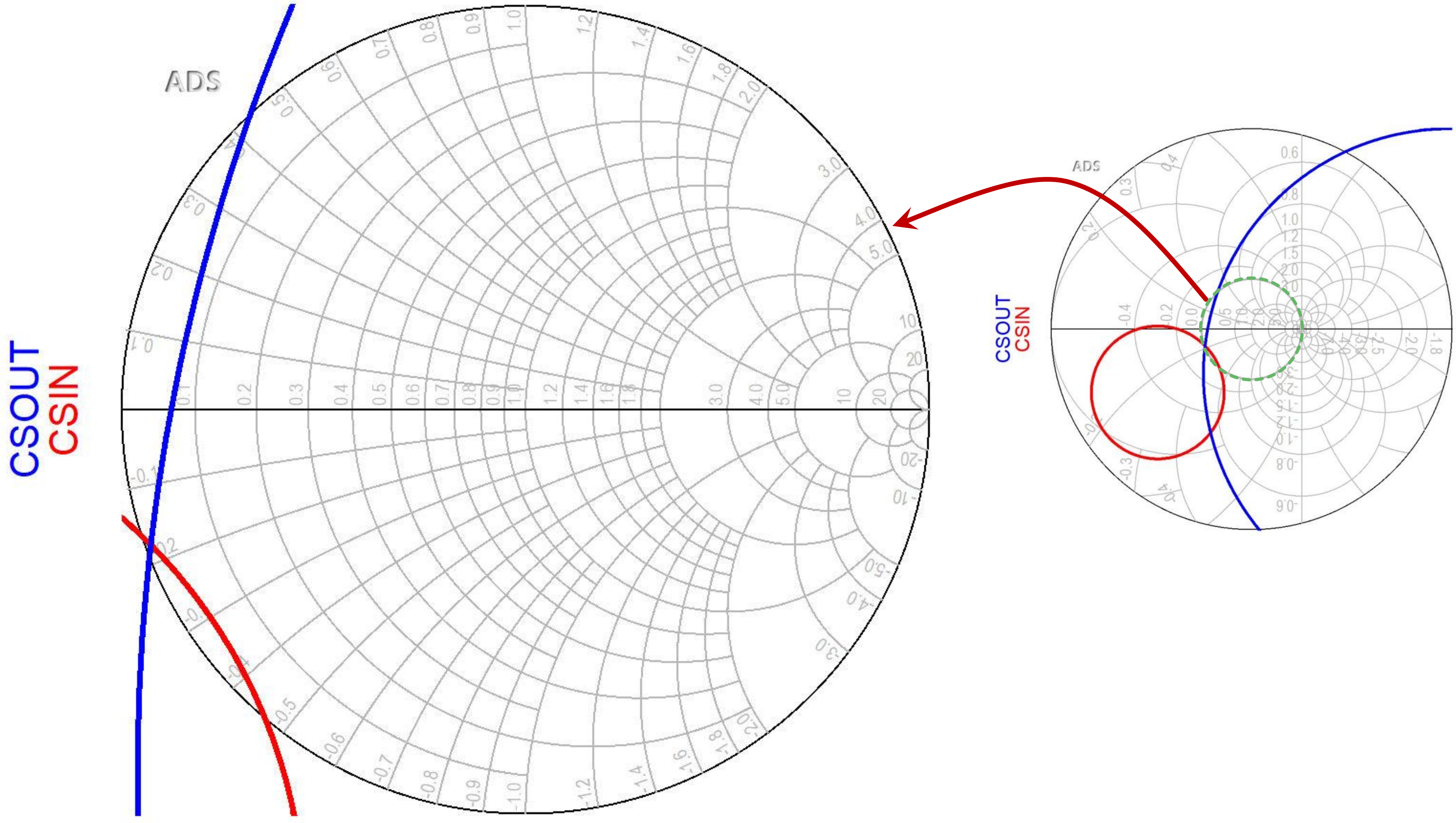
- S parameters
  - S11 = -0.483+0.42·j
  - S12 = 0.111-0.043·j
  - S21 = 3.042+0.872·j
  - S22 = -0.182+0.123·j
- $|S_{11}| < 1$
- $|C_S| > R_S$, $0 \notin CSIN$
- The center of the Smith chart is placed outside the input stability circle ($0 \notin CSIN$) and is a stable point
  - the outside of the input stability circle – stability region
  - the inside of the input stability circle – instability region

$$C_S = \frac{\left(S_{11} - \Delta \cdot S_{22}^*\right)^*}{|S_{11}|^2 - |\Delta|^2} = -1.871 - 1.265 \cdot j$$

$$|C_S| = 2.259$$

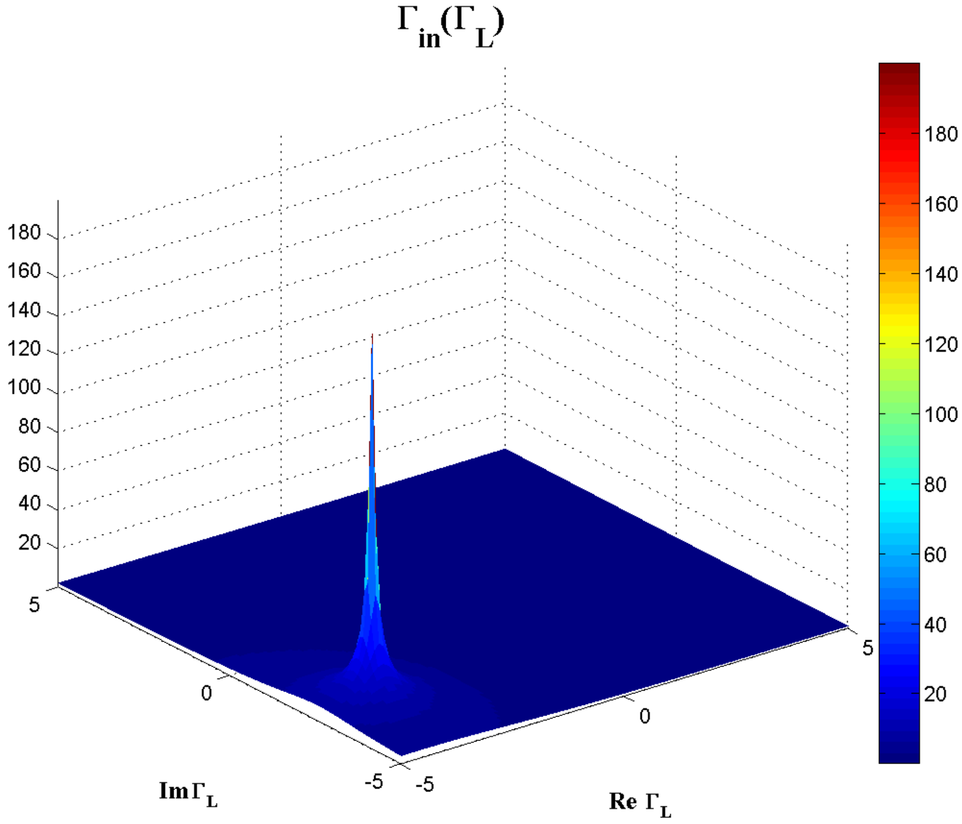
$$R_S = \frac{|S_{12} \cdot S_{21}|}{\left||S_{11}|^2 - |\Delta|^2\right|} = 1.325$$

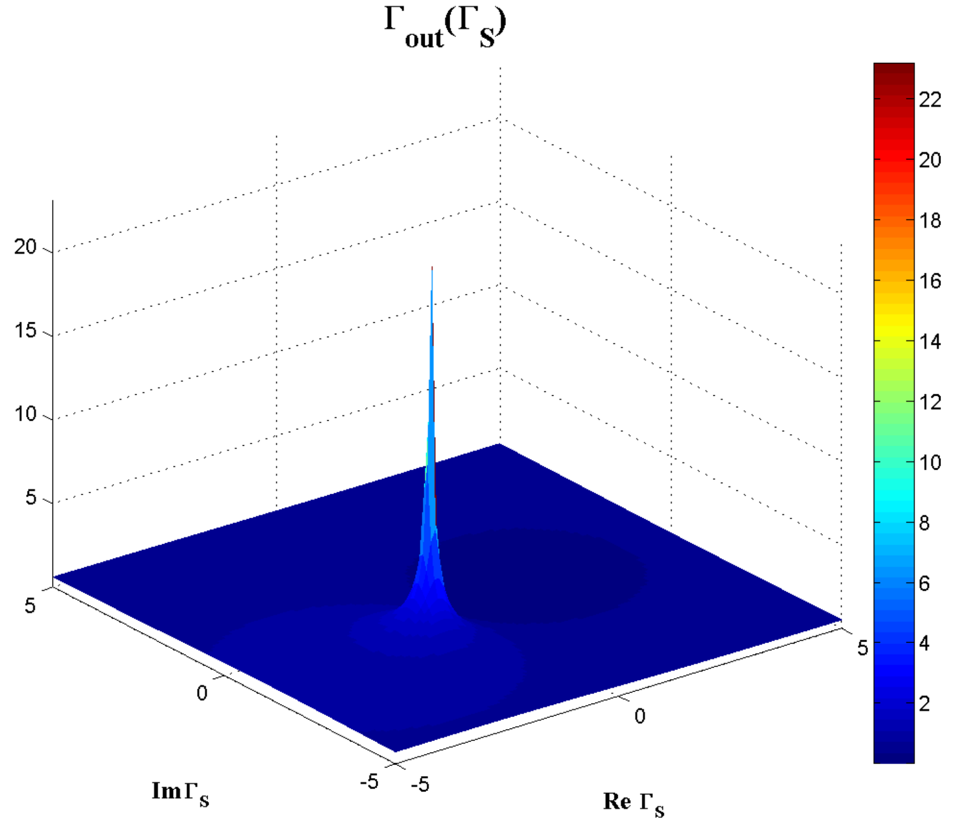
ADS



3D representation of $|\Gamma_{in}|$, $|\Gamma_{out}|$

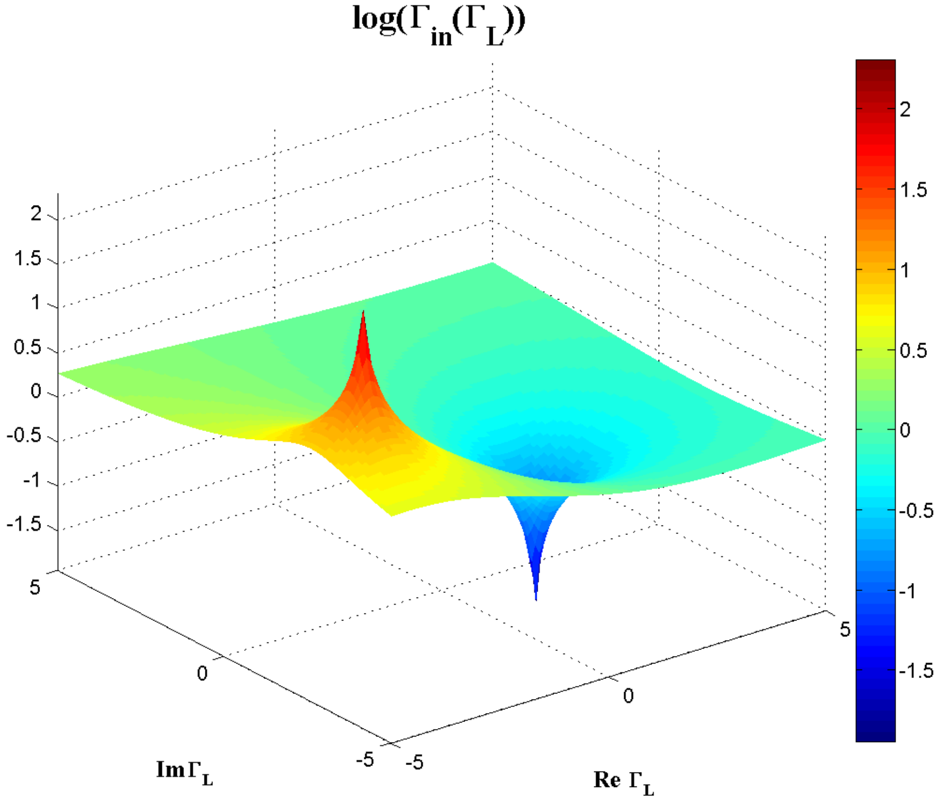
- High variations -> we change to z logarithmic scale

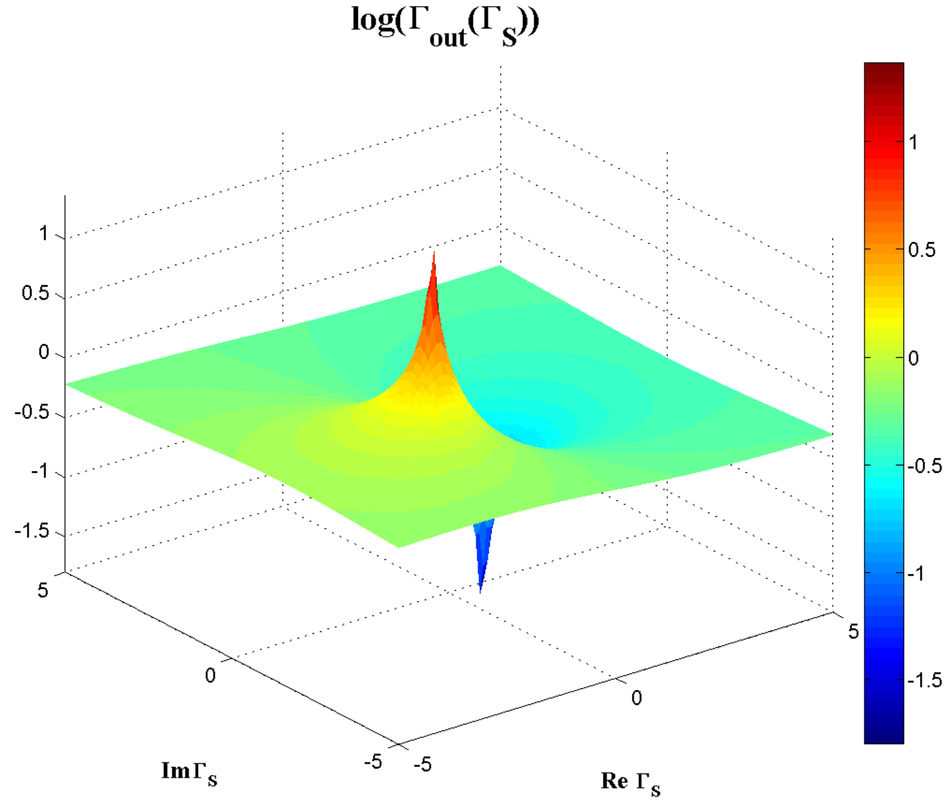




3D representation of $|\Gamma_{in}|$, $|\Gamma_{out}|$

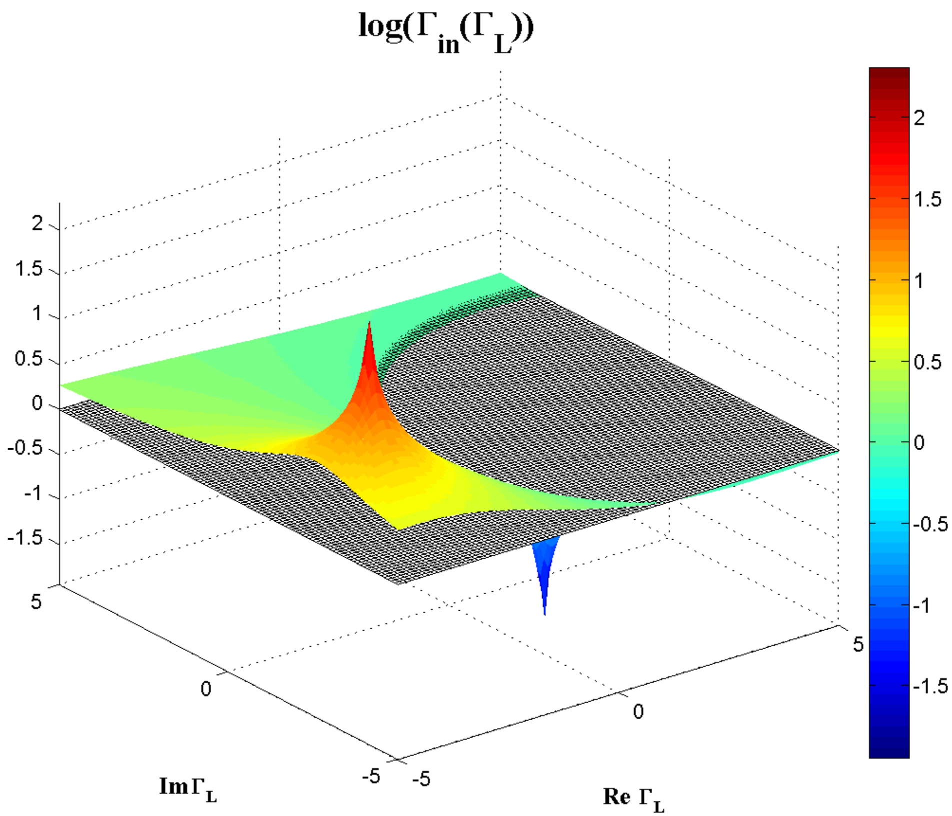
- $\log_{10}|\Gamma_{in}|$, $\log_{10}|\Gamma_{out}|$

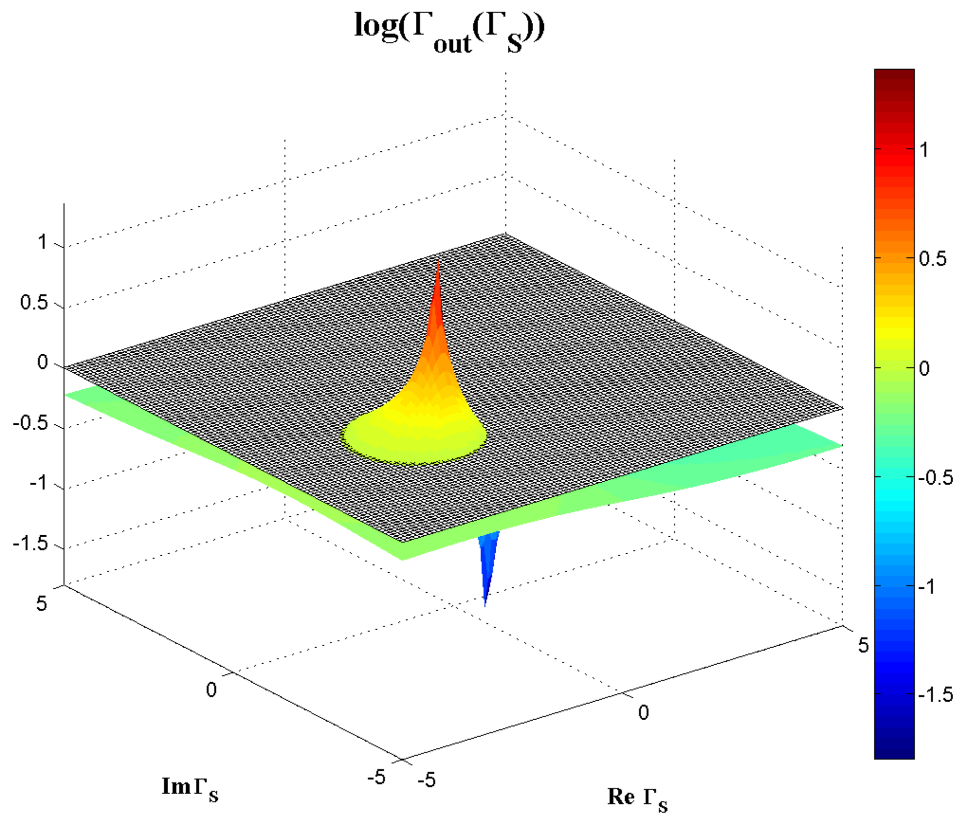




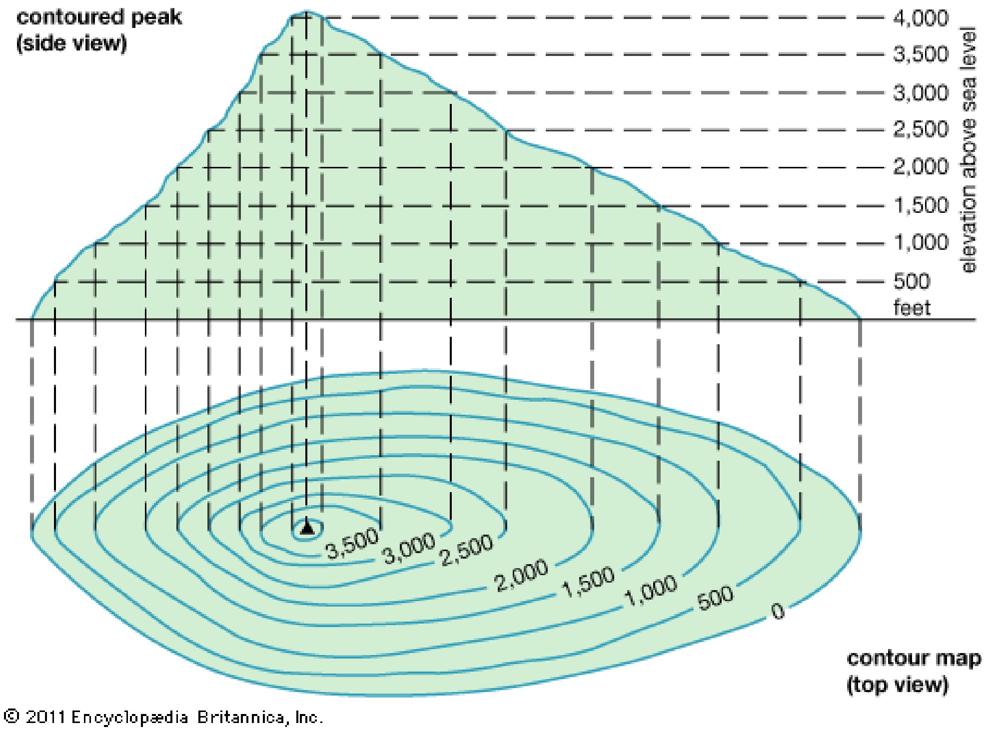
3D representation of $|\Gamma_{in}|$, $|\Gamma_{out}|$, $|\Gamma|=1$

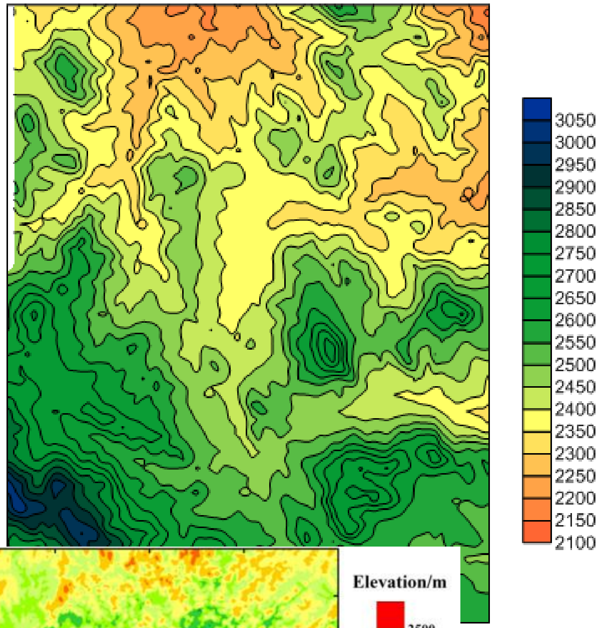
- $|\Gamma| = 1 \rightarrow \log_{10}|\Gamma| = 0$, the intersection with the plane z = 0 is a circle

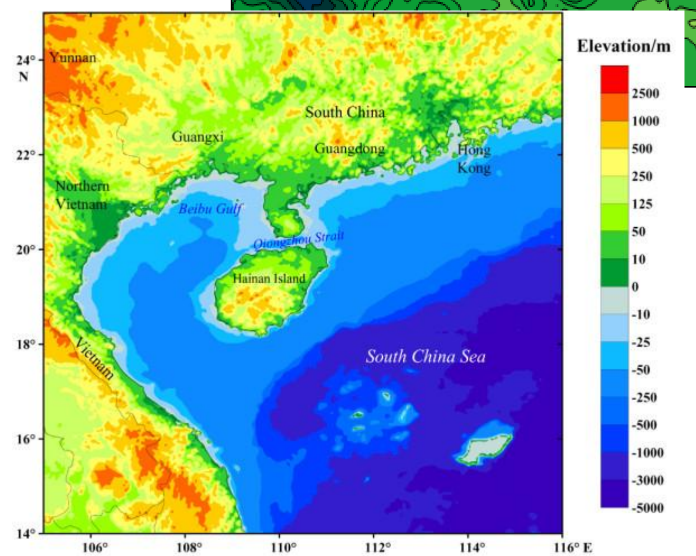




Contour map/lines

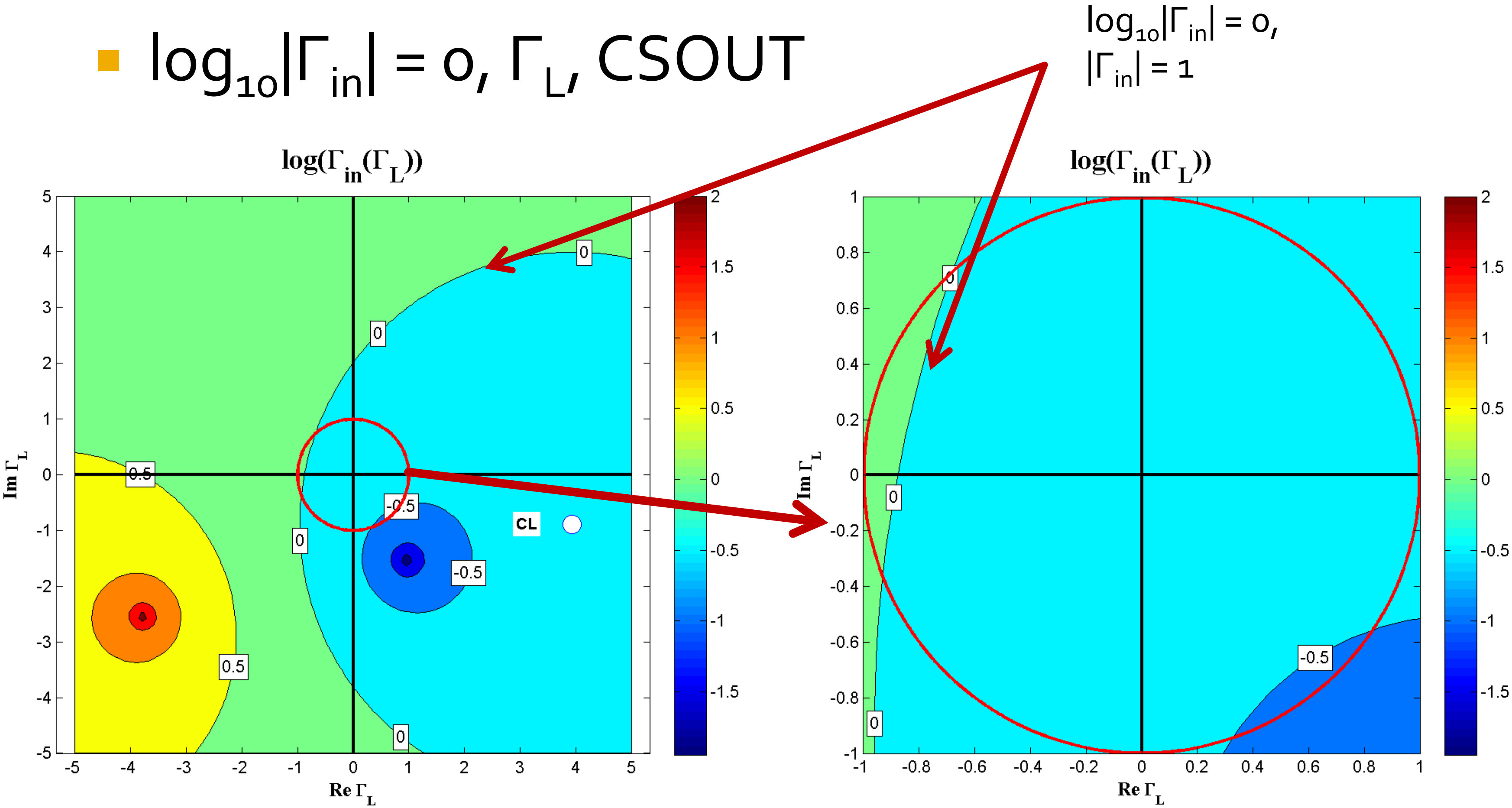






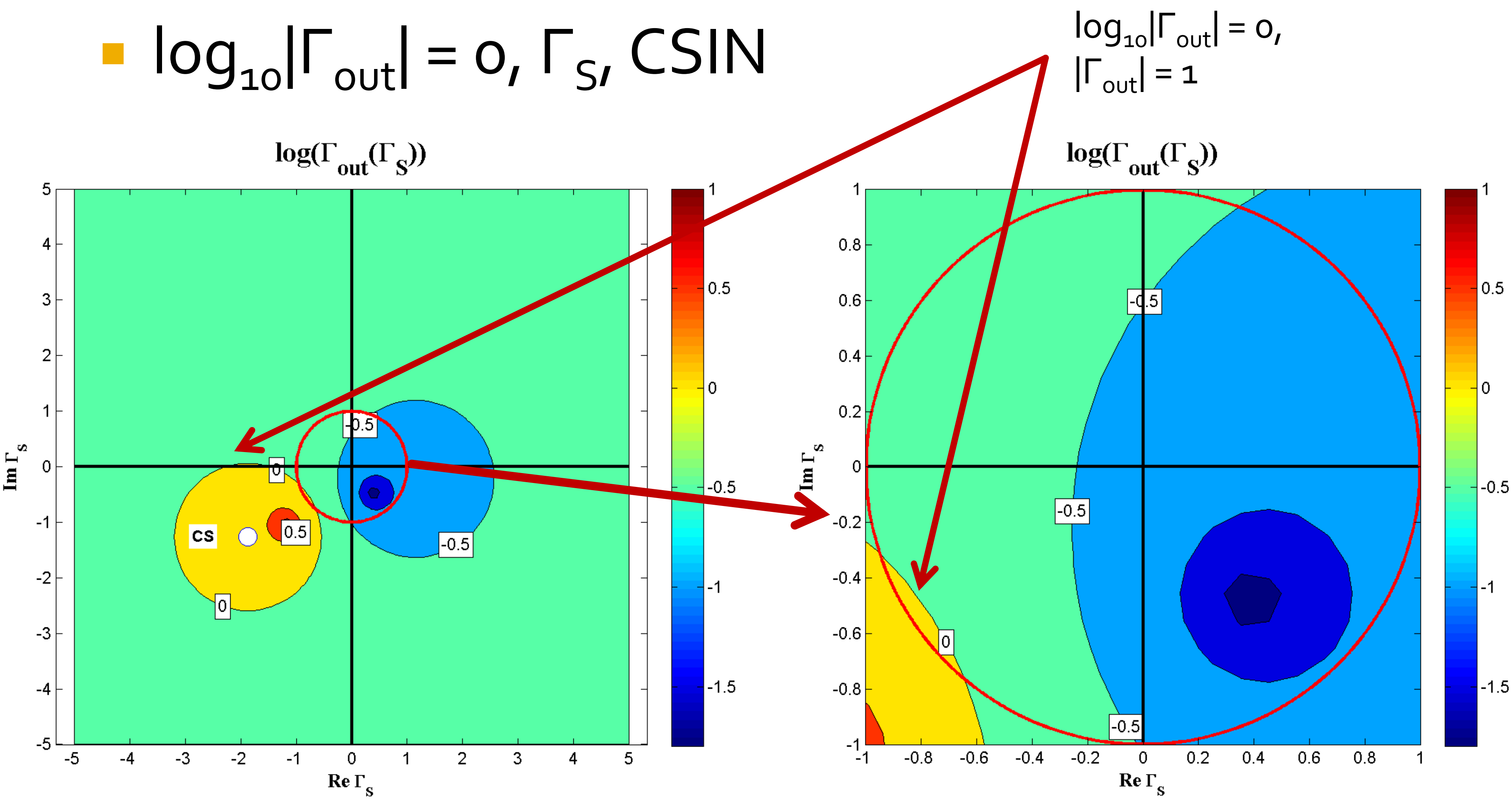
Contour lines of $\log_{10}|\Gamma_{in}|$

- $\log_{10}|\Gamma_{in}| = 0$, Γ_L, CSOUT

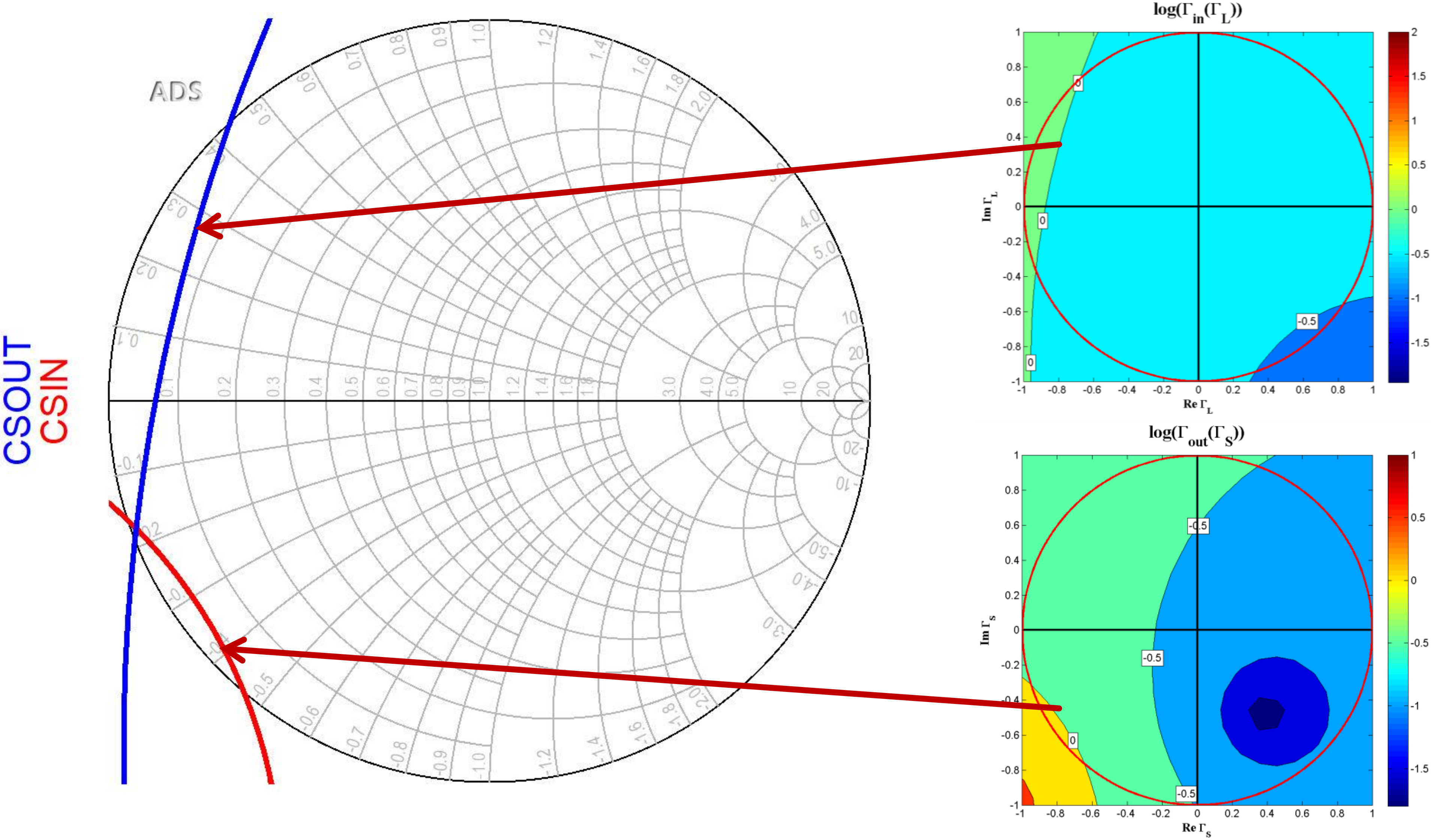


Contour lines of $\log_{10}|\Gamma_{out}|$

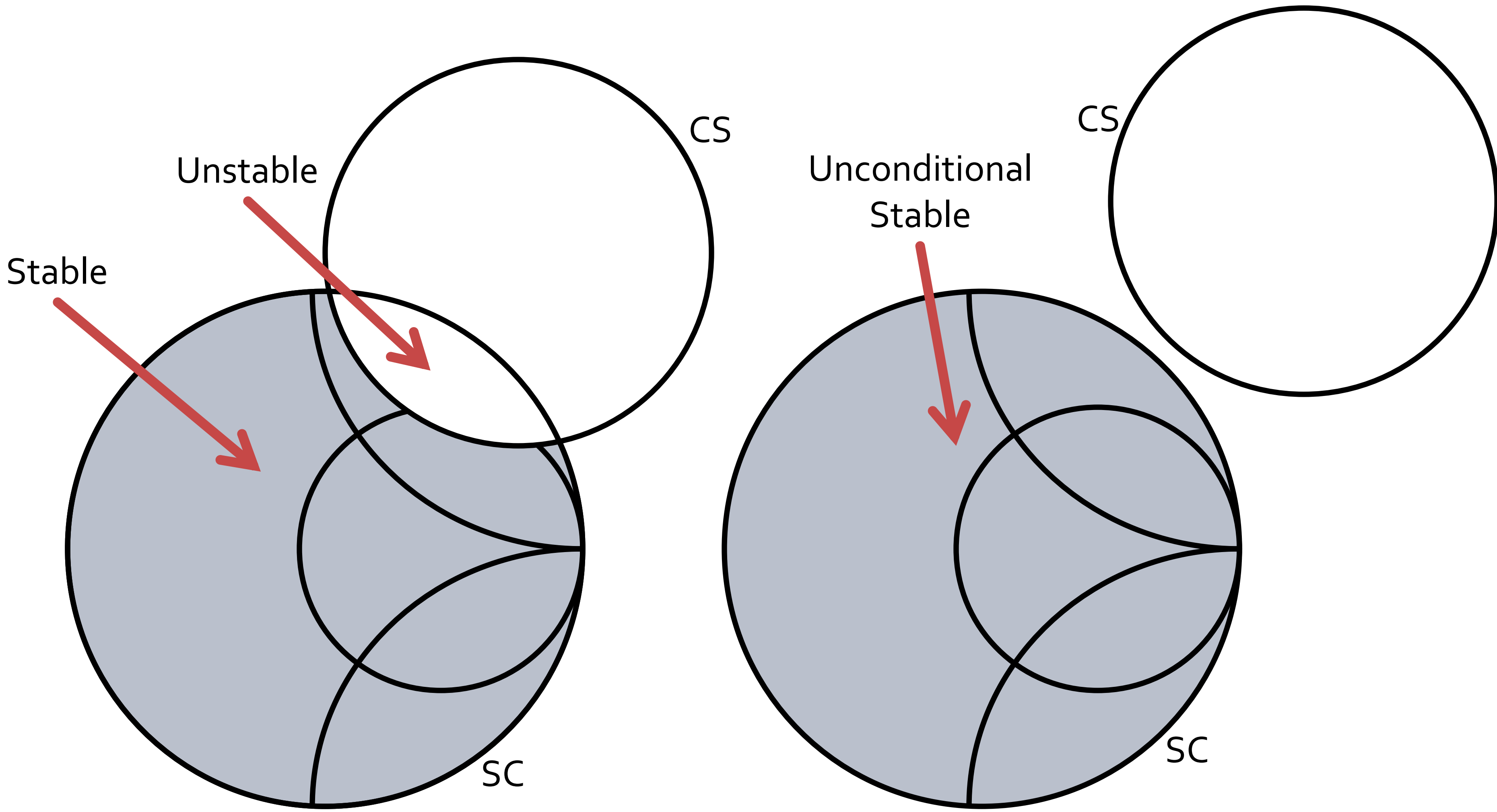
- $\log_{10}|\Gamma_{out}| = 0$, Γ_S, CSIN



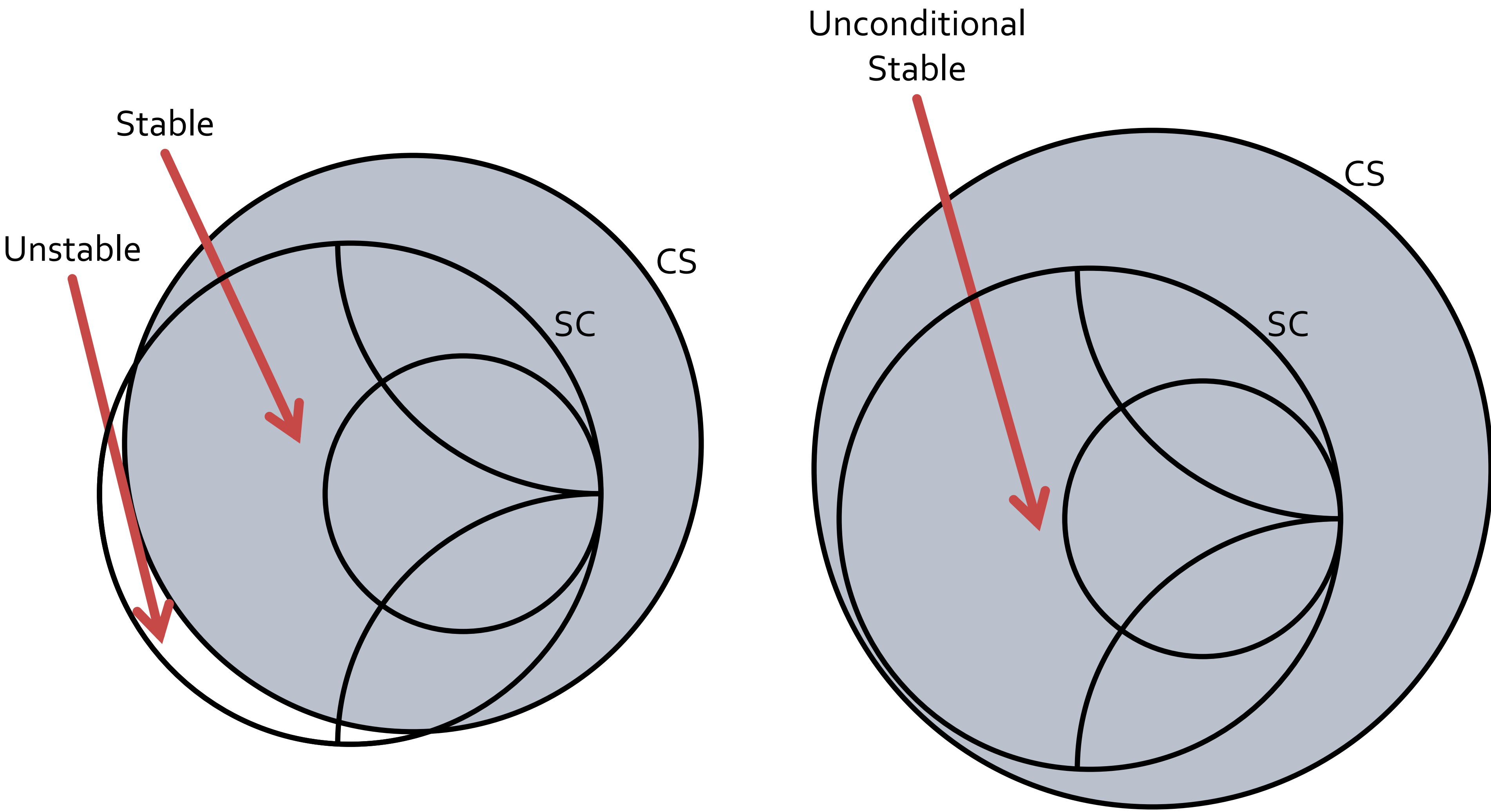
CSIN, CSOUT



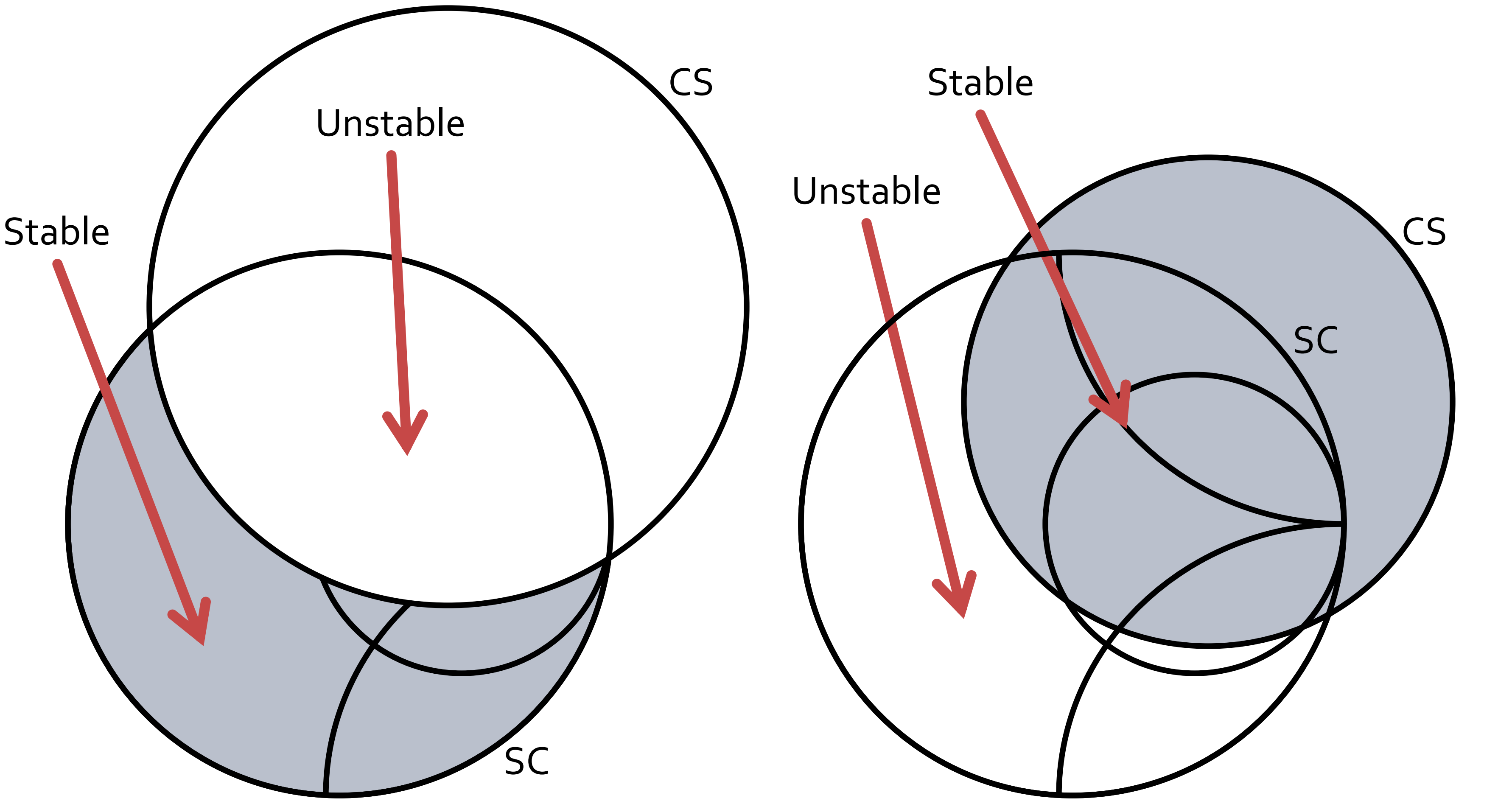
Several possible positioning



Several possible positioning



(Quite) Rare positioning



Stability

- **Unconditional stability:** the circuit is unconditionally stable if $|\Gamma_{in}|<1$ and $|\Gamma_{out}|<1$ for **any** passive impedance of the load/source
- **Conditional stability:** the circuit is conditionally stable if $|\Gamma_{in}|<1$ and $|\Gamma_{out}|<1$ only for **some** passive impedance of the load/source

Unconditional stability

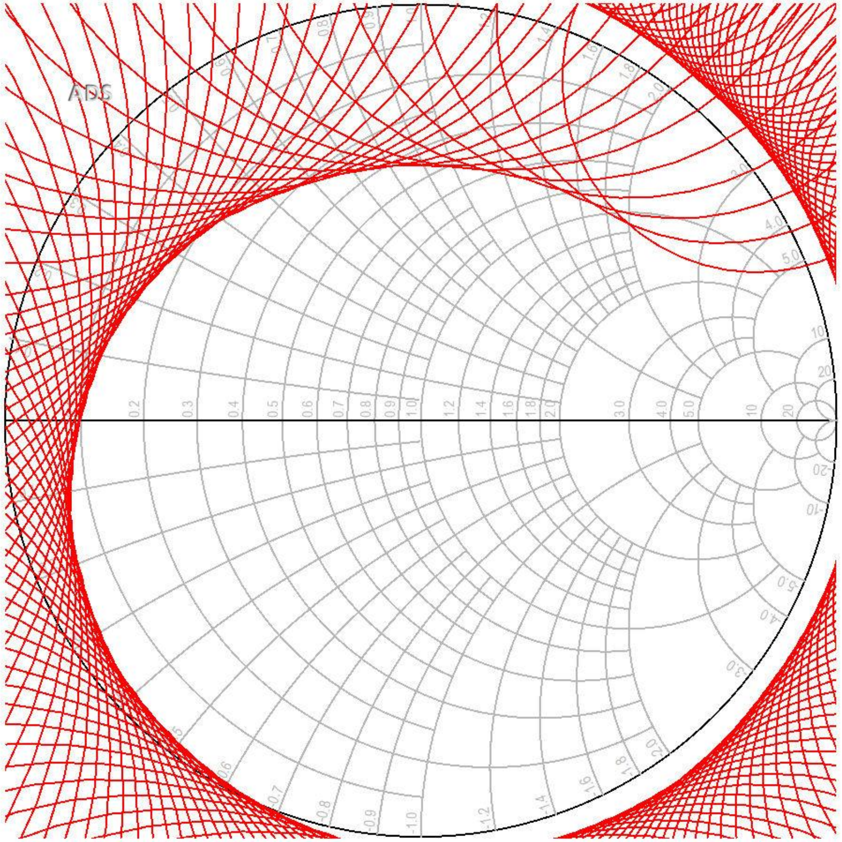
- The two-port is unconditionally stable if:
  - The stability circle is disjoint with the Smith Chart (exterior to the Chart) and the stable region is outside the circle
  - The stability circle encloses the entire Smith Chart and the stable region is inside the circle
- One mandatory condition for unconditional stability is |S11| < 1 (CSOUT) or |S22| < 1 (CSIN) – if in at least one point the two-port is not stable then it cannot be unconditionally stable
- Mathematically :

$$\begin{cases} \left| |C_L| - R_L \right| > 1 \\ |S_{11}| < 1 \end{cases} \qquad \begin{cases} \left| |C_S| - R_S \right| > 1 \\ |S_{22}| < 1 \end{cases}$$

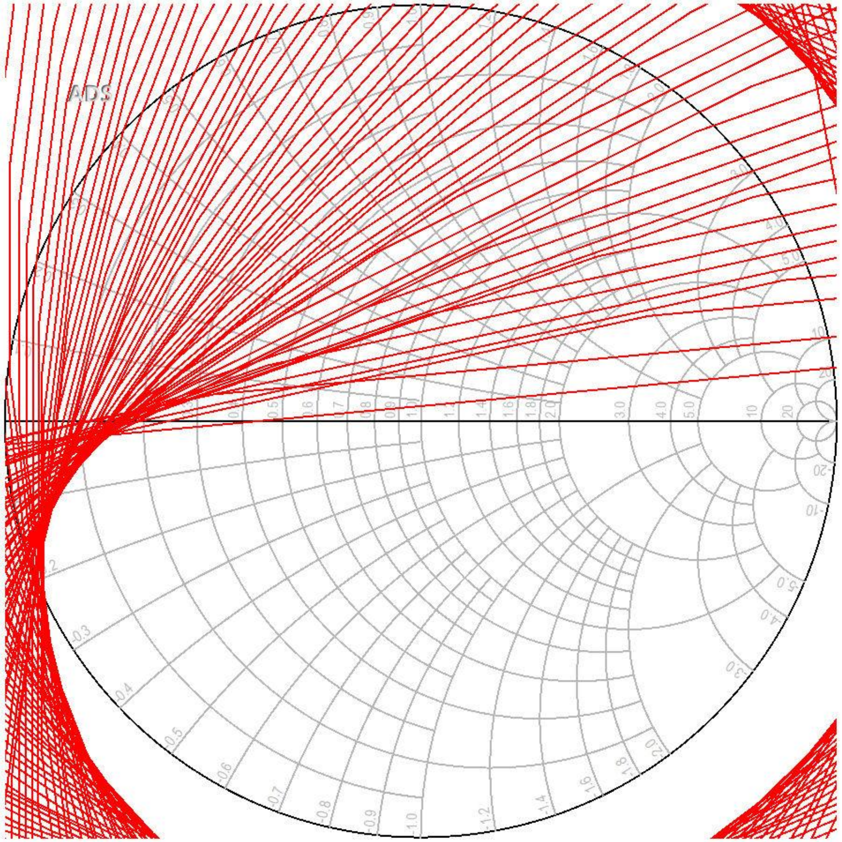
Tests for Unconditional Stability

- Useful for wide frequency range analysis
- It is not enough to check the stability only at the operating frequencies
  - we must obtain stable operation for chosen Γ_L and Γ_S at **any** frequency

Circles in wide frequency range



CSIN



CSOUT

Rollet's condition

$$K = \frac{1 - |S_{11}|^2 - |S_{22}|^2 + |\Delta|^2}{2 \cdot |S_{12} \cdot S_{21}|} \qquad \Delta = S_{11} \cdot S_{22} - S_{12} \cdot S_{21}$$

- The two-port is **unconditionally stable** if:
- two conditions are simultaneously satisfied:
  - K > 1
  - |Δ| < 1
- together with the implicit conditions:
  - |S11| < 1
  - |S22| < 1

$$K = \frac{1 - |S_{11}|^2 - |S_{22}|^2 + |\Delta|^2}{2 \cdot |S_{12} \cdot S_{21}|} > 1 \qquad |\Delta| = |S_{11} \cdot S_{22} - S_{12} \cdot S_{21}| < 1$$

μ Criterion

- Rollet's condition cannot be used to compare the relative stability of two or more devices because it involves constraints on two separate parameters, K and Δ

$$\mu = \frac{1-|S_{11}|^2}{|S_{22} - \Delta \cdot S_{11}^*| + |S_{12} \cdot S_{21}|} > 1$$

- The two-port is **unconditionally stable** if:
  - $\mu > 1$
- together with the implicit conditions:
  - $|S_{11}| < 1$
  - $|S_{22}| < 1$
- In addition, it can be said that larger values of μ imply greater stability
  - μ is the distance from the center of the Smith Chart to the closest output stability circle

μ′ Criterion

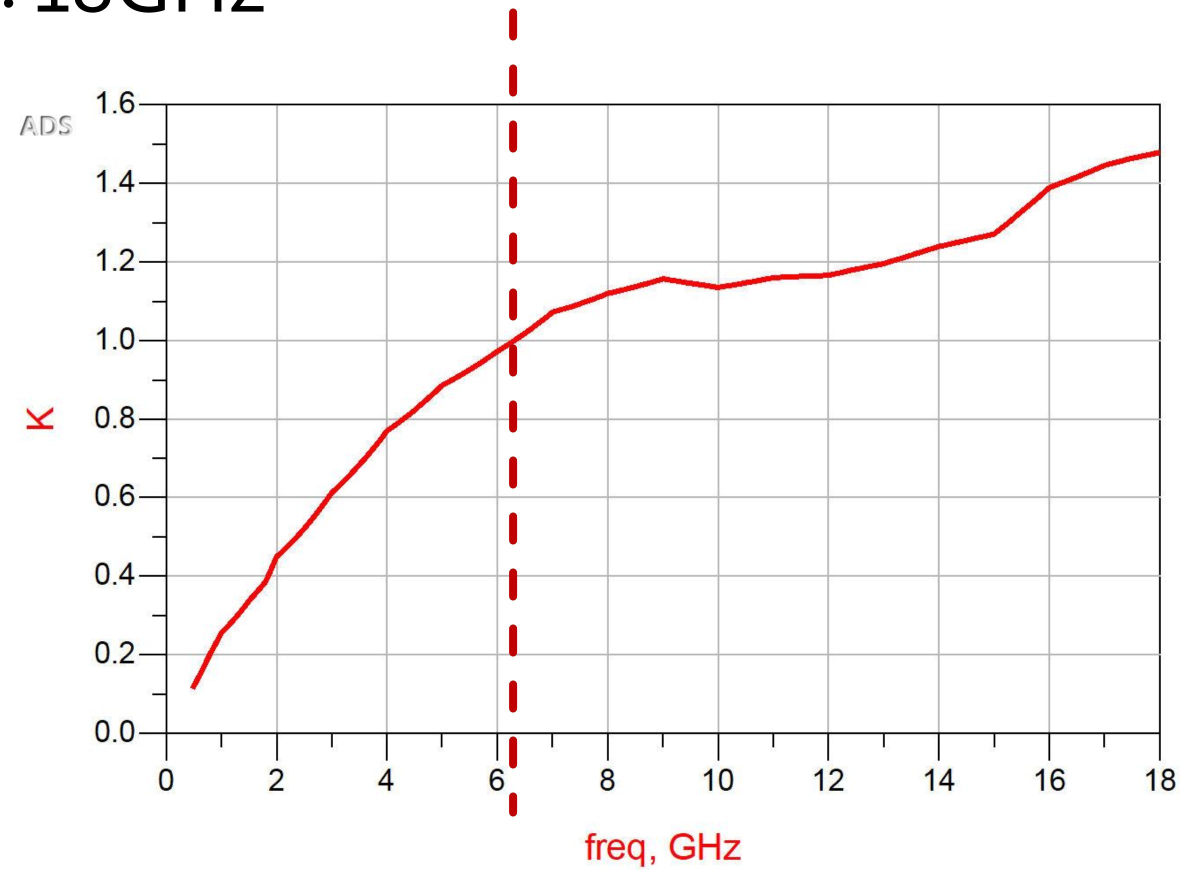
- Dual parameter to μ, determined in relation to the input stability circles

$$\mu' = \frac{1-|S_{22}|^2}{|S_{11} - \Delta \cdot S_{22}^*| + |S_{12} \cdot S_{21}|} > 1$$

- The two-port is **unconditionally stable** if:
  - $\mu' > 1$
- together with the implicit conditions:
  - $|S_{11}| < 1$
  - $|S_{22}| < 1$
- In addition, it can be said that larger values of μ′ imply greater stability
  - μ′ is the distance from the center of the Smith Chart to the closest input stability circle

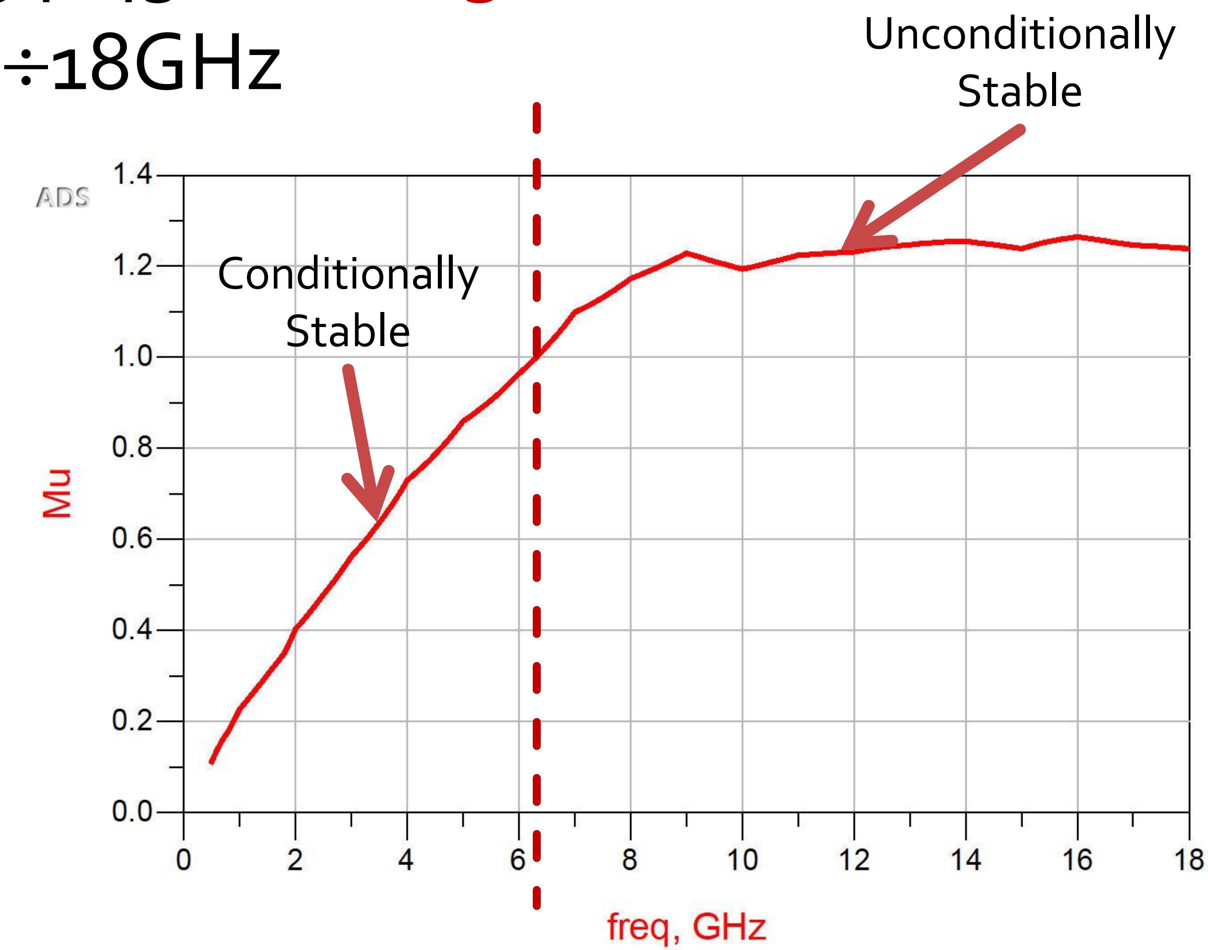
Rollet's condition

- ATF-34143 **at Vds=3V Id=20mA**.
- @0.5÷18GHz



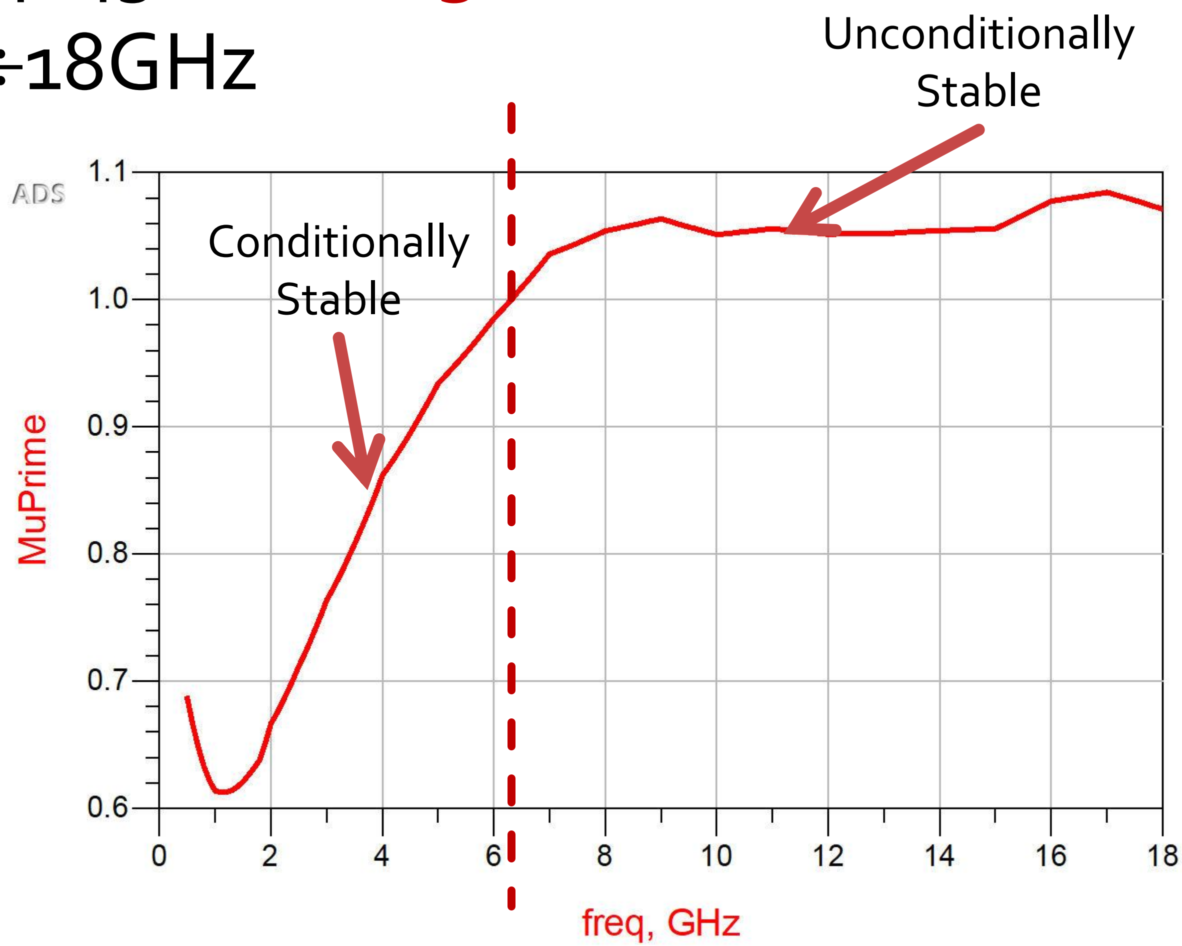
µ Criterion

- ATF-34143 **at Vds=3V Id=20mA**.
- @0.5÷18GHz



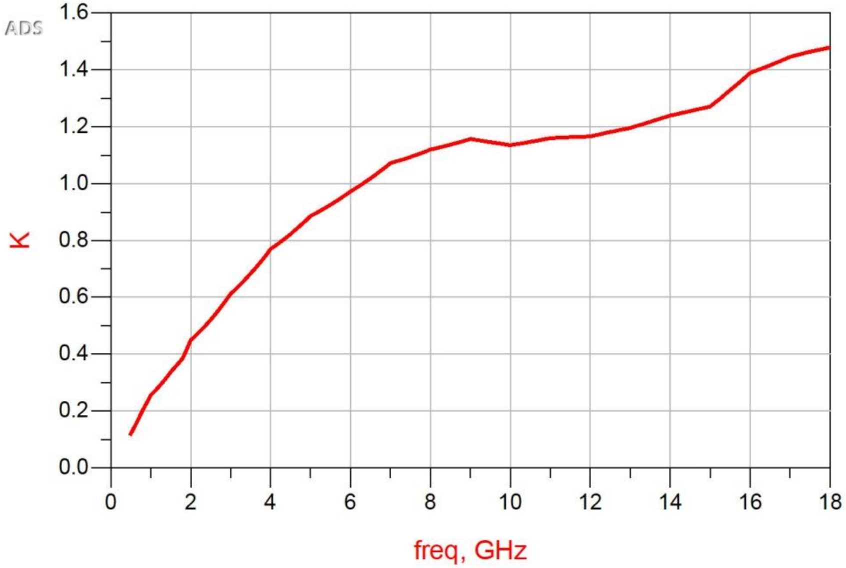
μ' Criterion

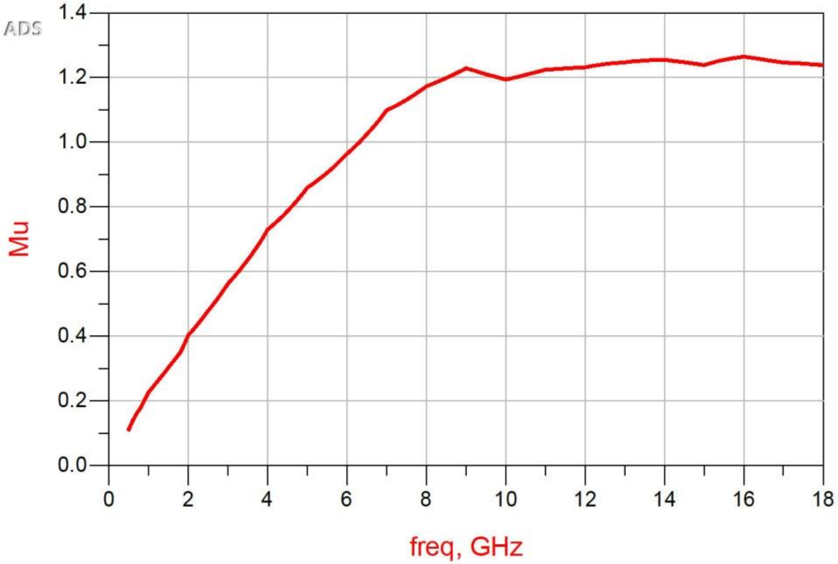
- ATF-34143 **at Vds=3V Id=20mA**.
- @0.5÷18GHz



Stability

- ATF-34143 **at Vds=3V Id=20mA**.
- @0.5÷18GHz
- unconditionally stable for f > 6.31GHz

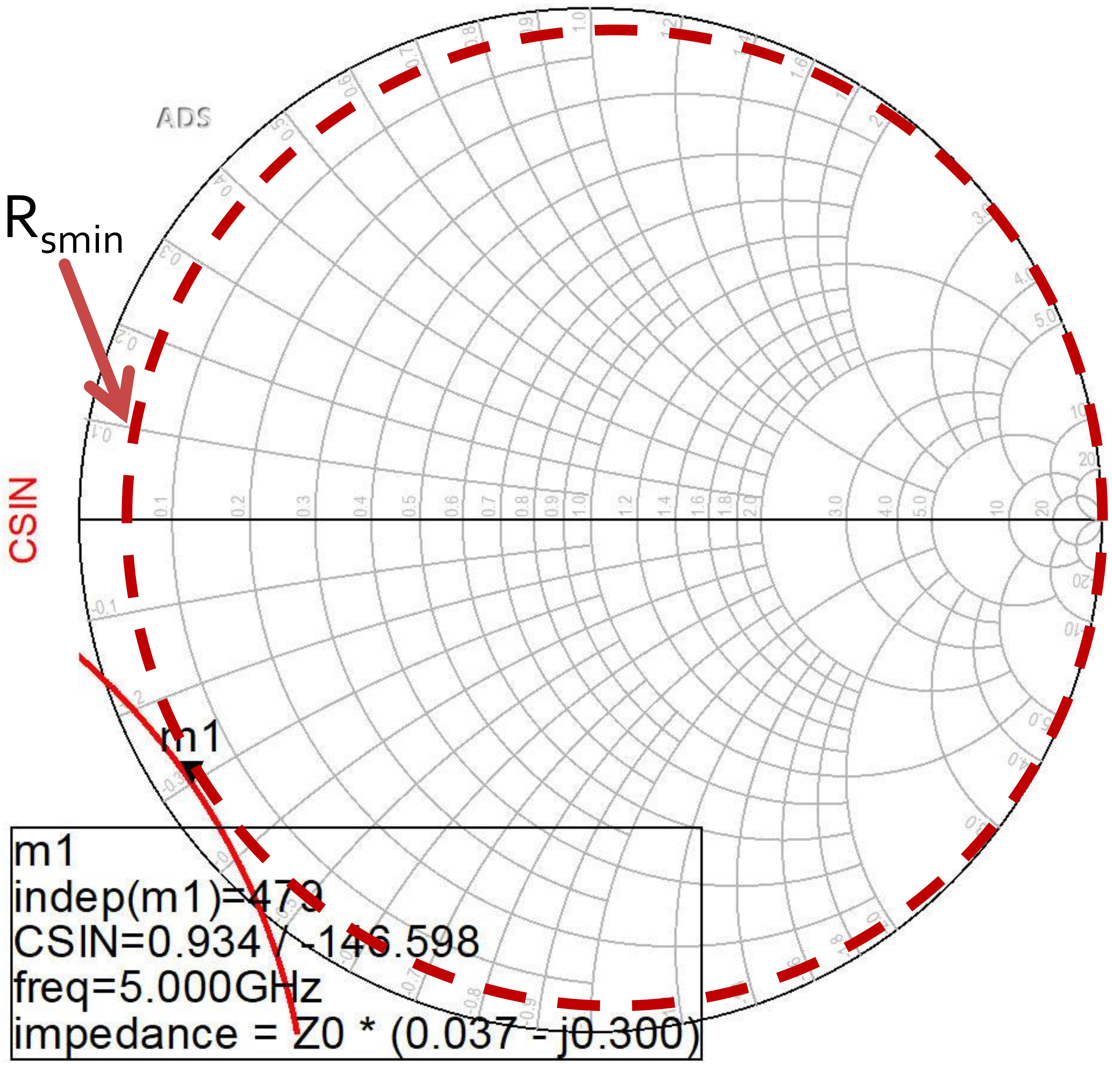


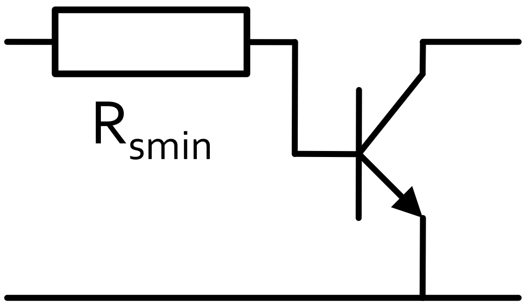


Stabilization of two-port

- Unconditional stability in a wide frequency range has some important advantages
  - Ex: We can use ATF 34143 to design a (conditionally) stable amplifier at 5GHz, but this design is useless if the amplifier oscillates at 500MHz ($\mu \approx 0.1$)
- **The minimal requirement** when working with conditionally stable devices is to **check stability** at several frequencies over the operating bandwidth and outside the bandwidth
- Unconditional stability can be forced by inserting series/shunt resistors at two-port's input/output (with loss of gain!)

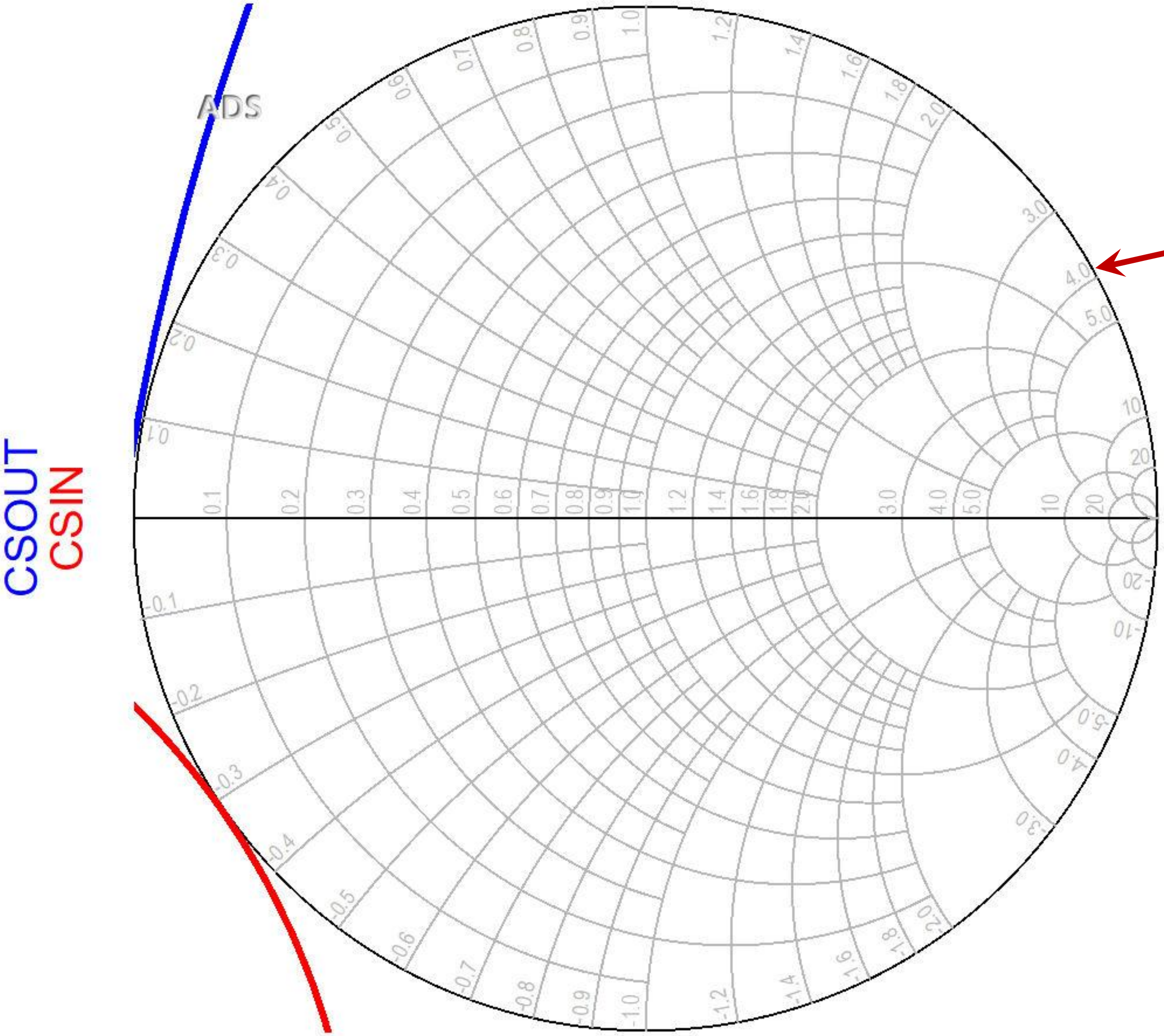
Input series resistor

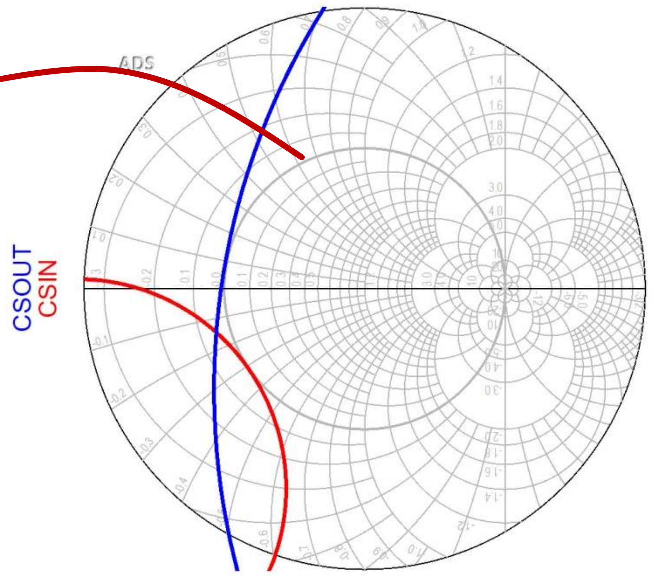




$$R_{s\,\min} = 0.037 \cdot 50\Omega = 1.85\Omega$$

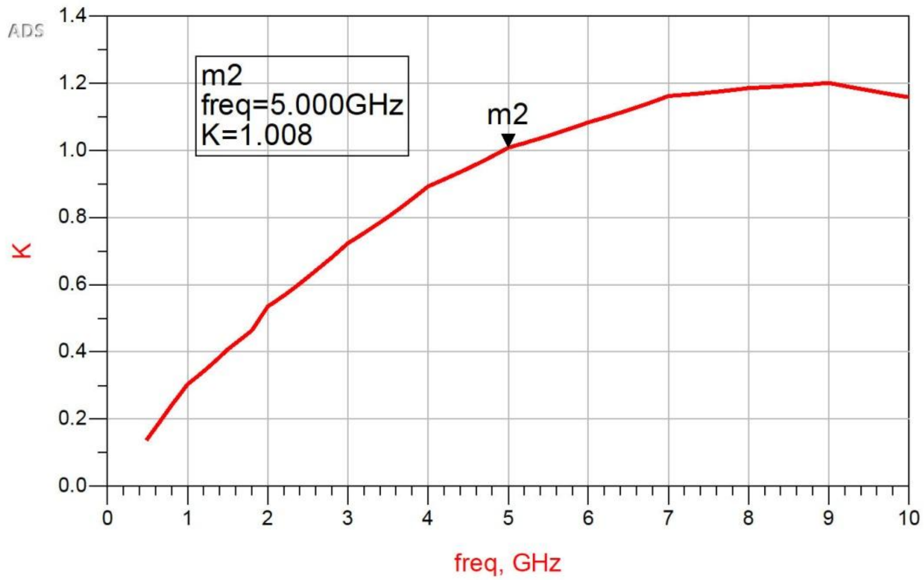
ADS, Rs = 2Ω

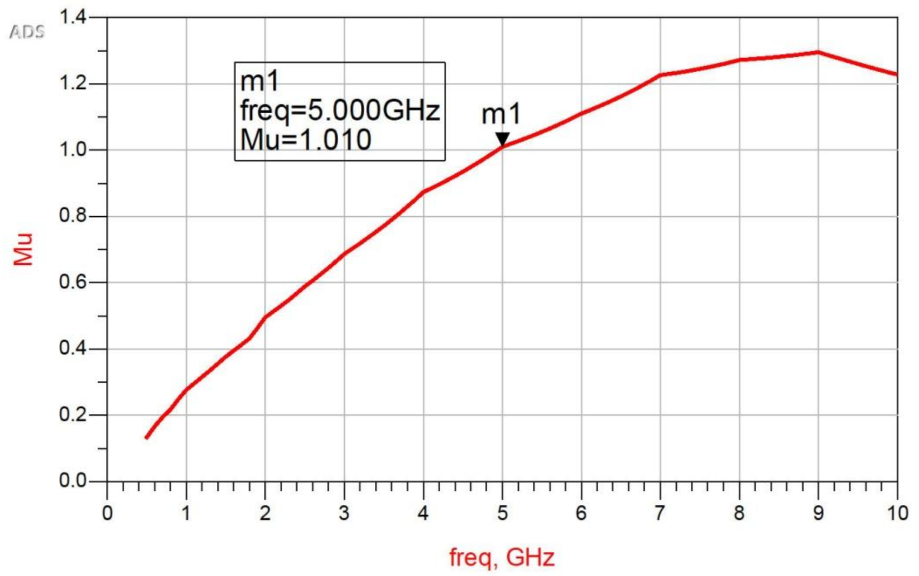




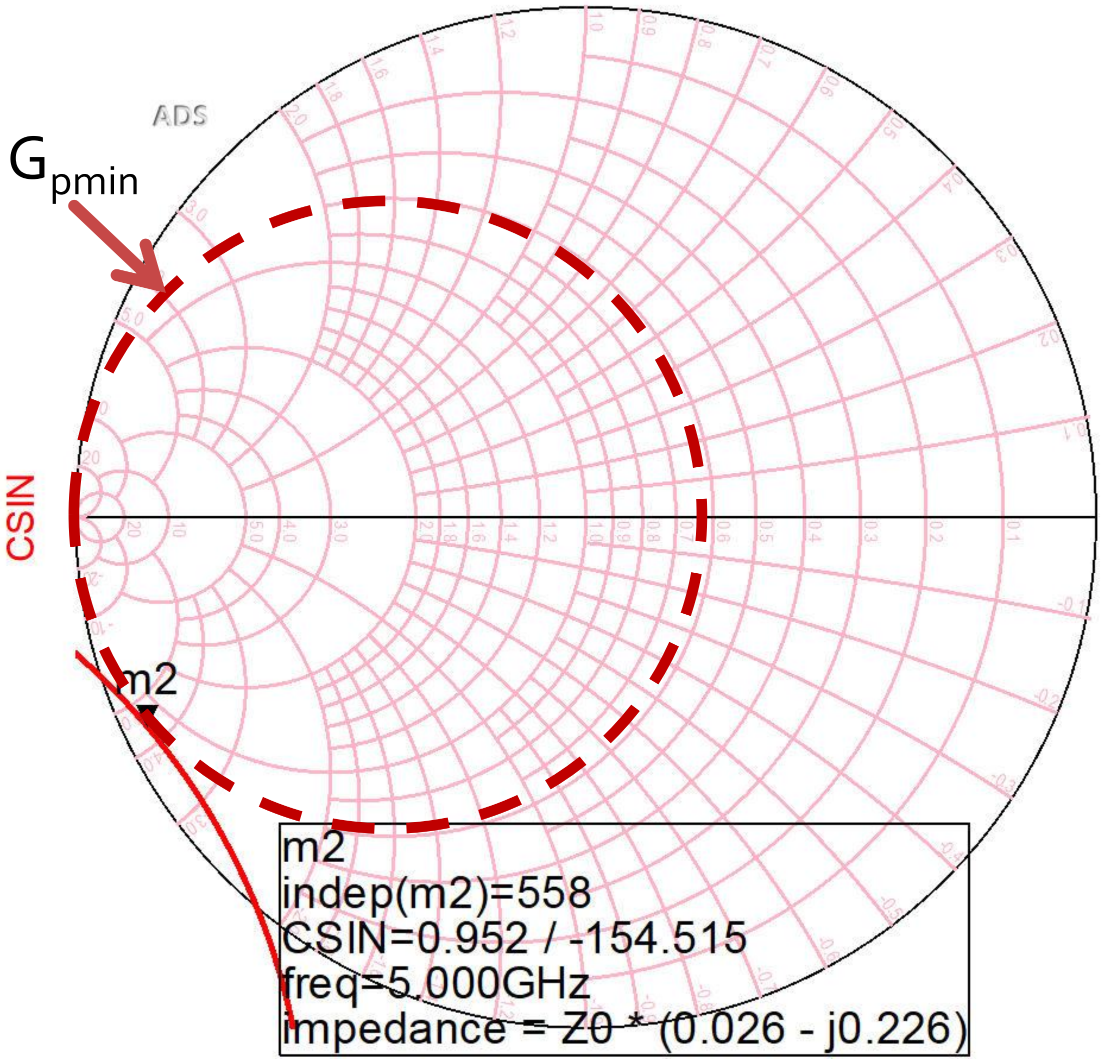
Input series resistor

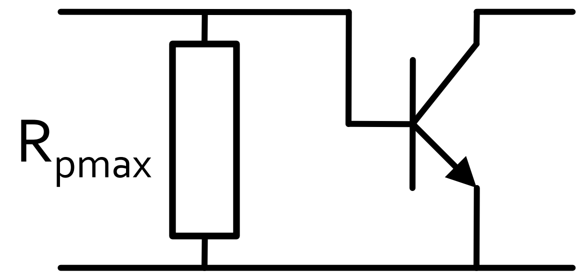
- Rs = 2Ω
- K = 1.008, MAG = 13.694dB @ 5GHz
  - no stabilization, K = 0.886, MAG = 14.248dB @ 5GHz





Input shunt resistor



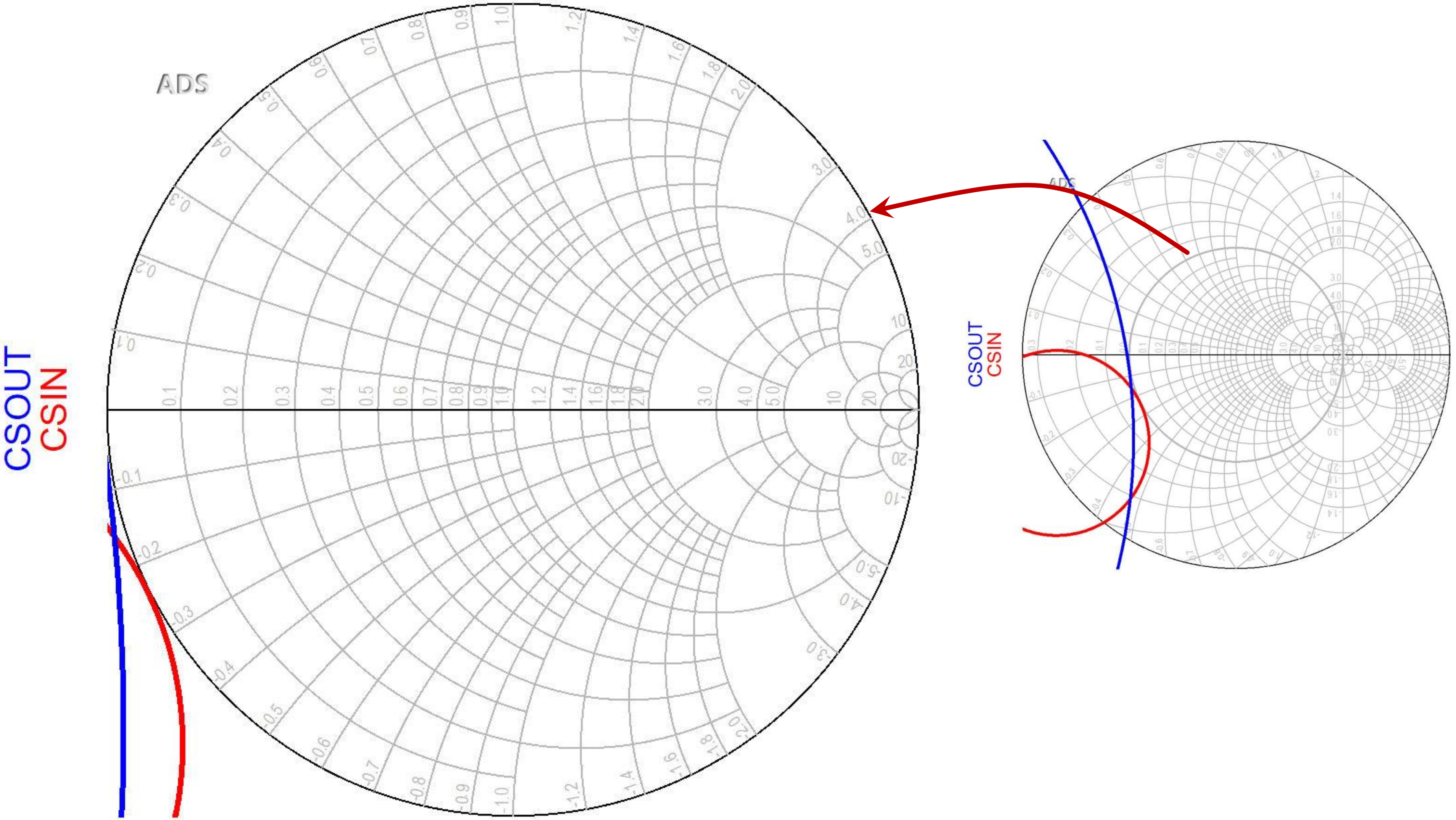


$$R_{p\max} = \frac{1}{G_{p\min}}$$

$$\frac{1}{0.026 - j \cdot 0.226} = 0.502 + j \cdot 4.367$$

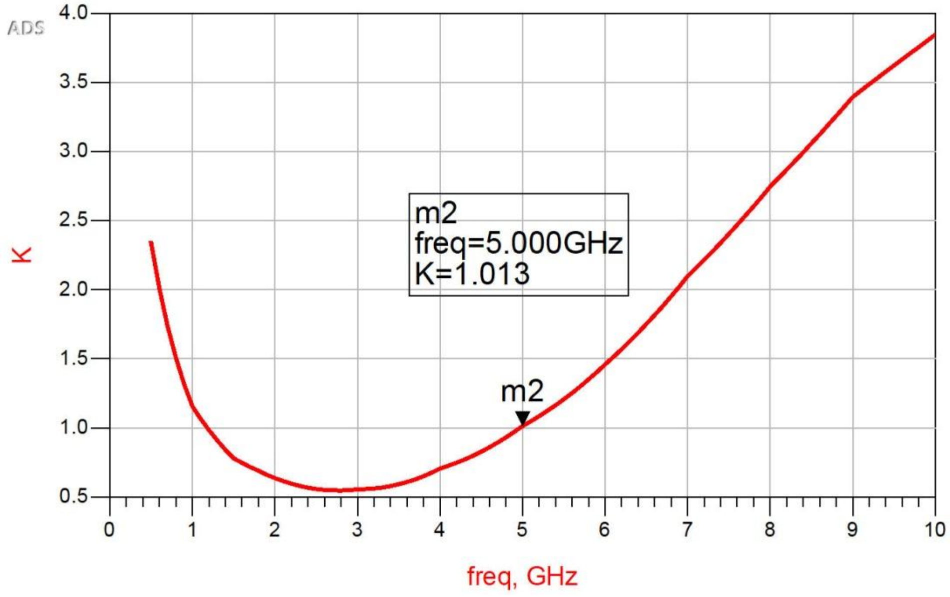
$$R_{p\max} = \frac{50\Omega}{0.502} = 99.6\Omega$$

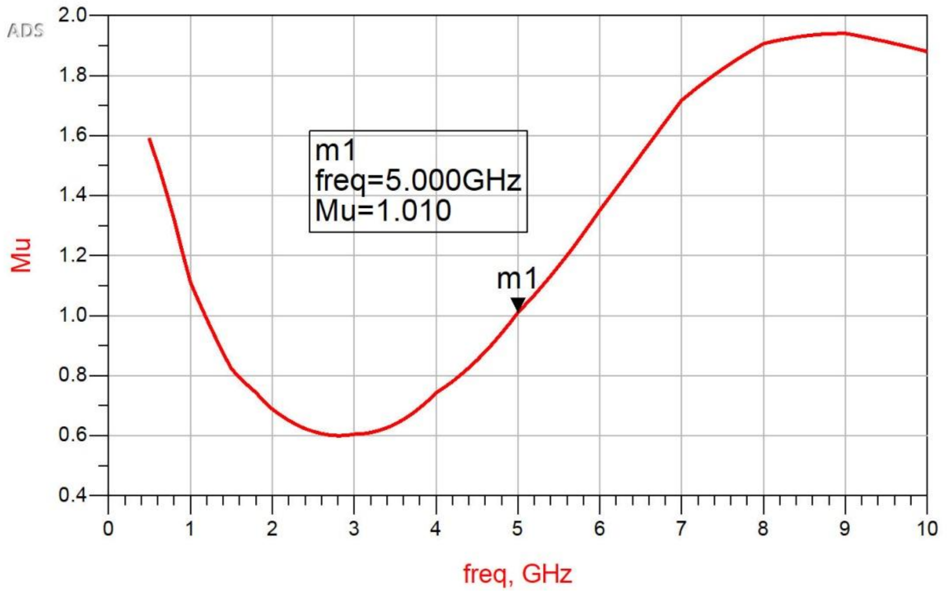
ADS, Rp = 90Ω



Input shunt resistor

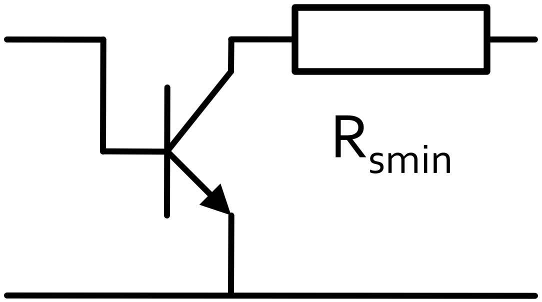
- Rp = 90Ω
- K = 1.013, MAG = 13.561dB @ 5GHz
  - no stabilization, K = 0.886, MAG = 14.248dB @ 5GHz

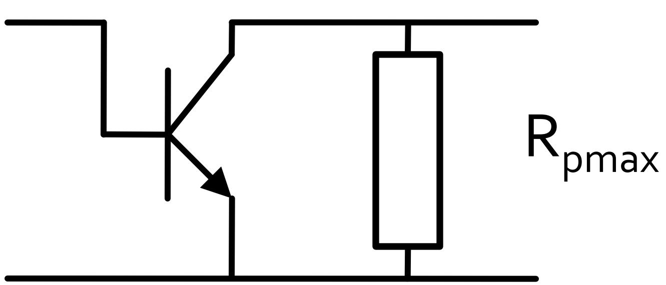




Output series/shunt resistor

- The procedure can be applied similarly at the output (finding g/r circles tangent to CSOUT)
- From previous examples, resistive loading at the input has a positive effect over output stability and vice versa (resistive loading at the output, effect over input stability)

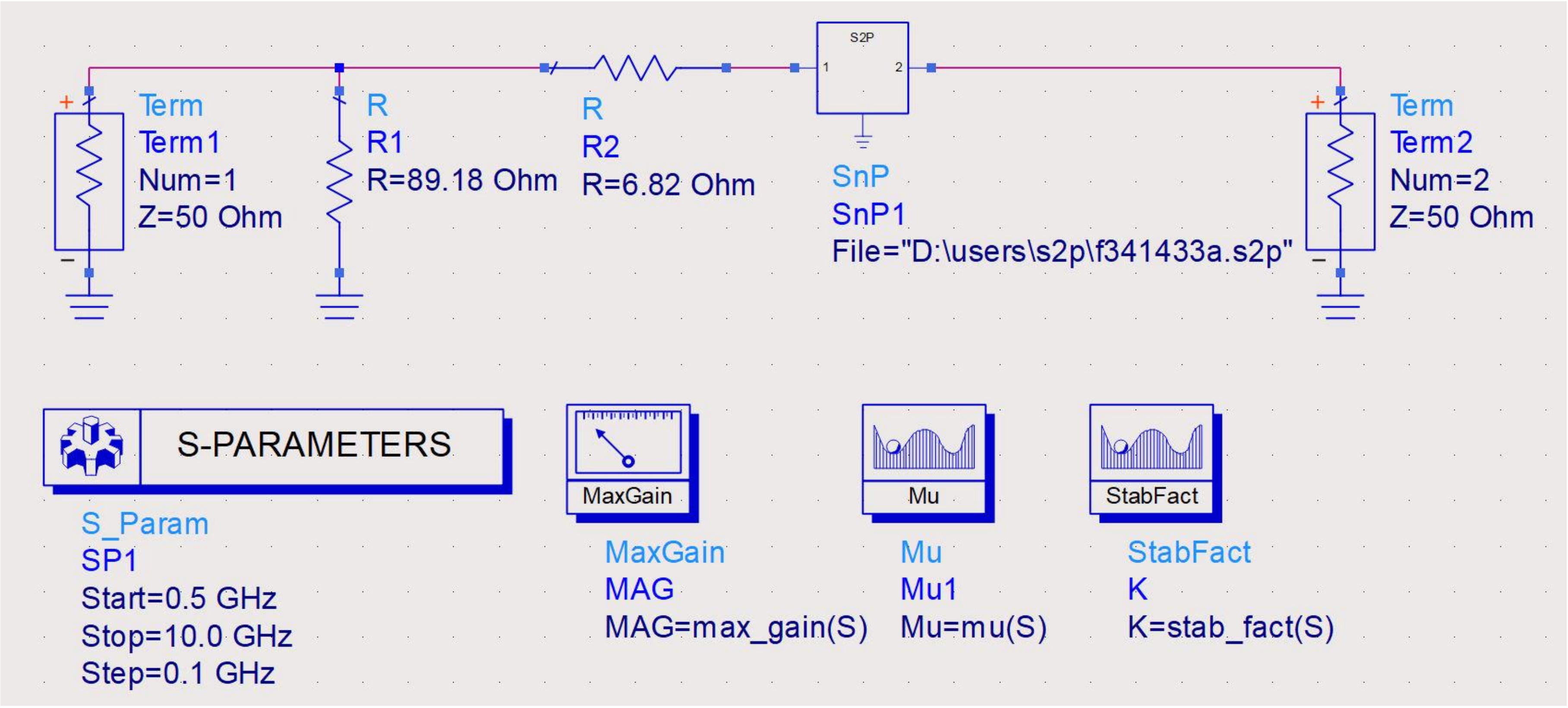




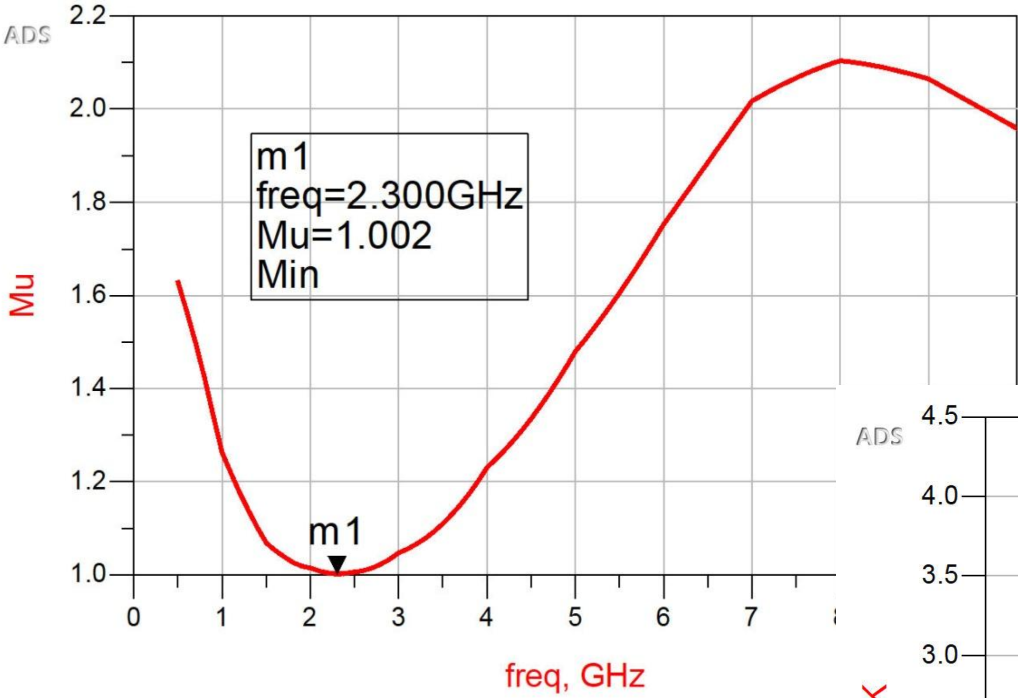
Stabilization of two-port

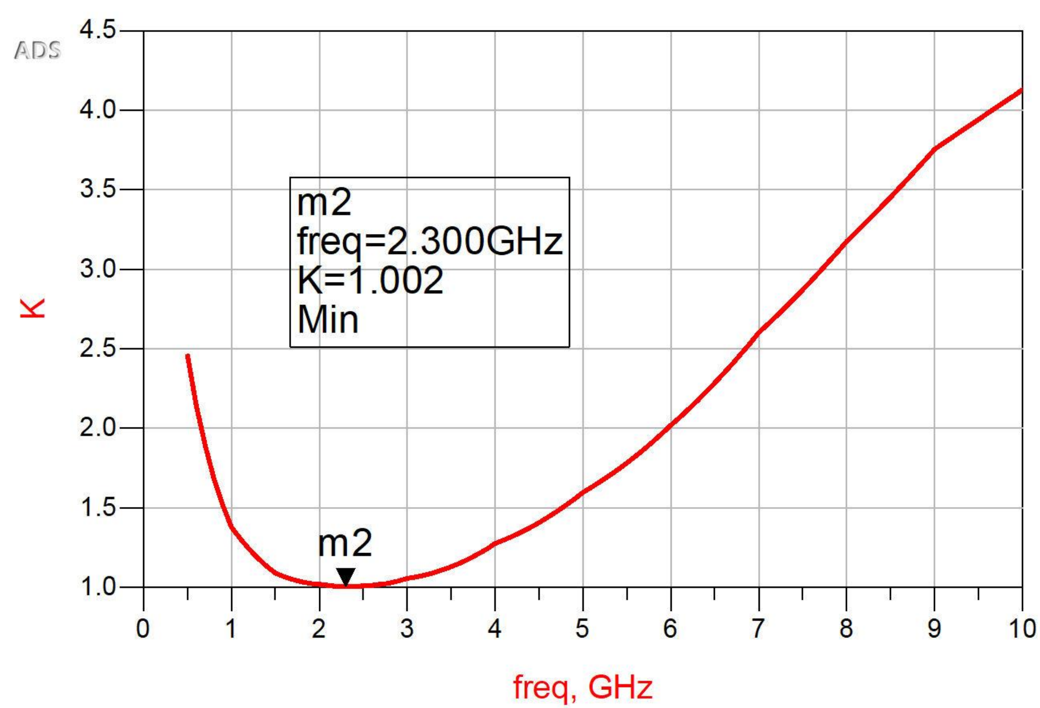
- Negative effect over the power gain
  - we must check MAG/MSG while designing resistive loading
- Negative effect over the noise (next lectures)
- We can choose one of the 4 possibilities or a combination which offers better results (depending on transistor, application etc.)
- We can use frequency selective loading
  - Ex: RL, RC circuits which sacrifice performance only when needed to improve stability and have no effect at frequencies where the device is already stable
- It might be possible (and should be checked) that stability is improved as an effect of parasitic elements of biasing circuits (bypass capacitors and RF chokes)

Stabilization of two-port

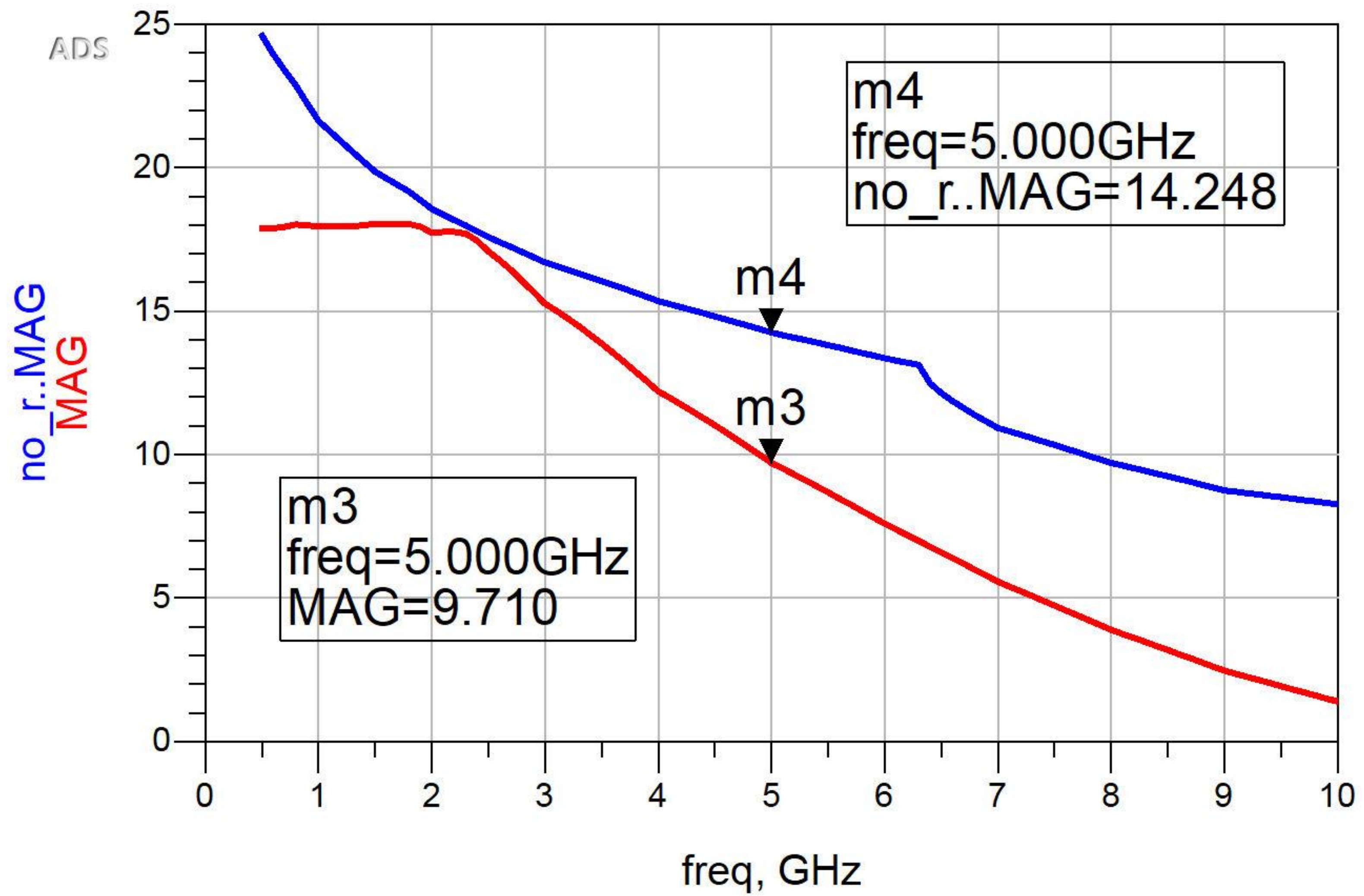


Stabilization of two-port

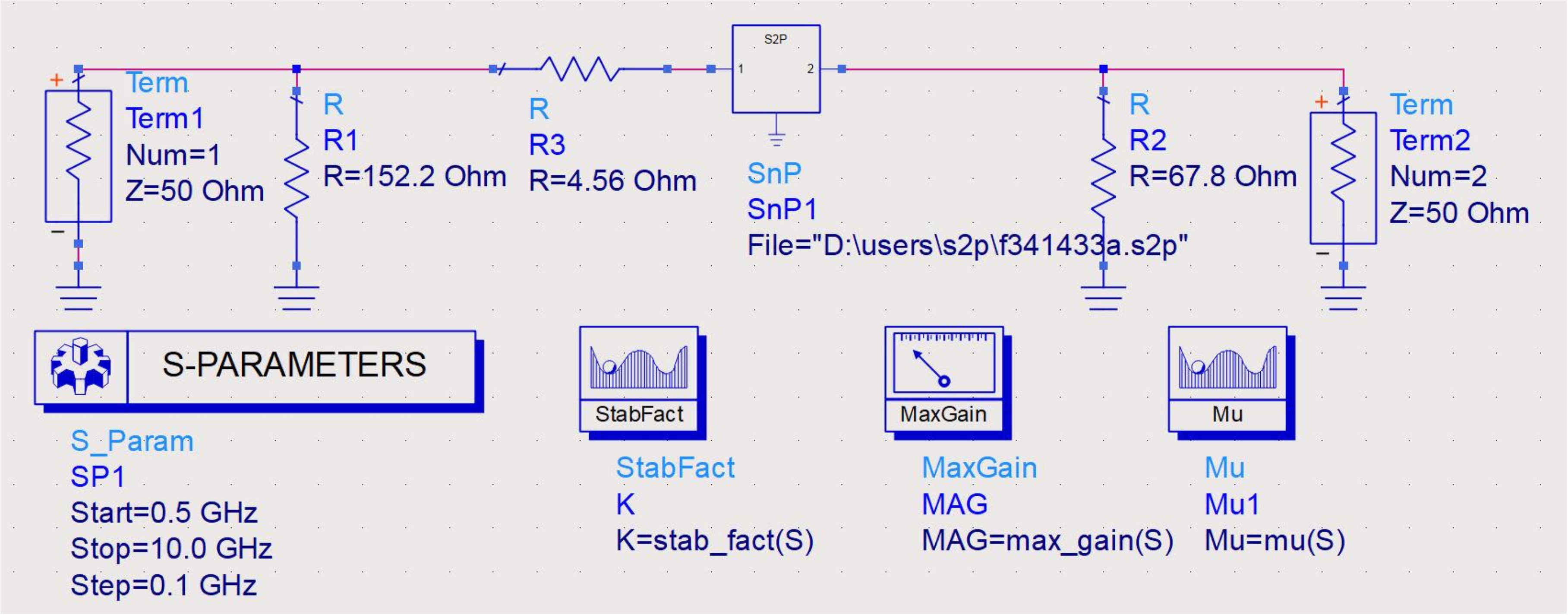




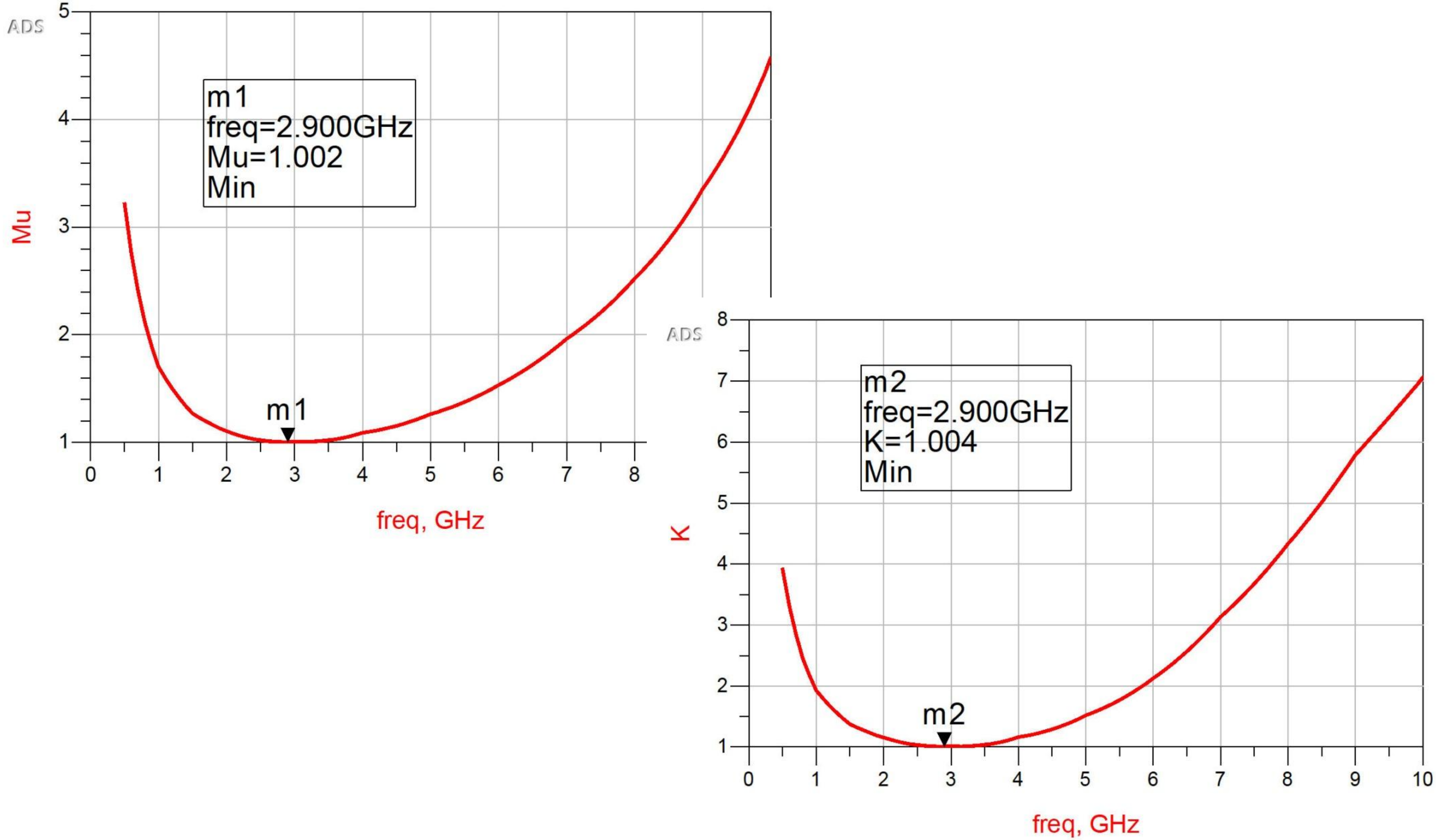
Stabilization of two-port



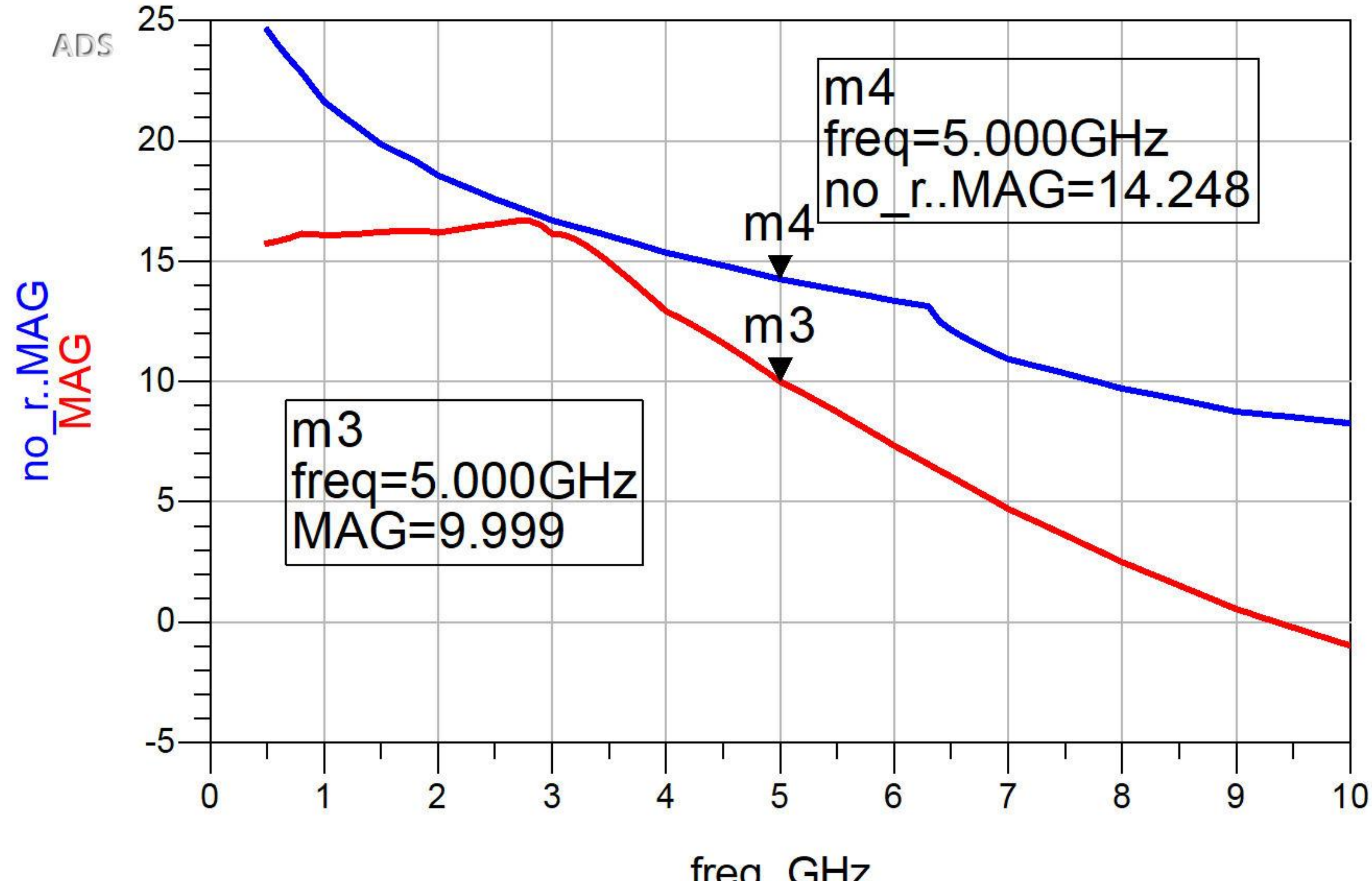
Stabilization of two-port



Stabilization of two-port



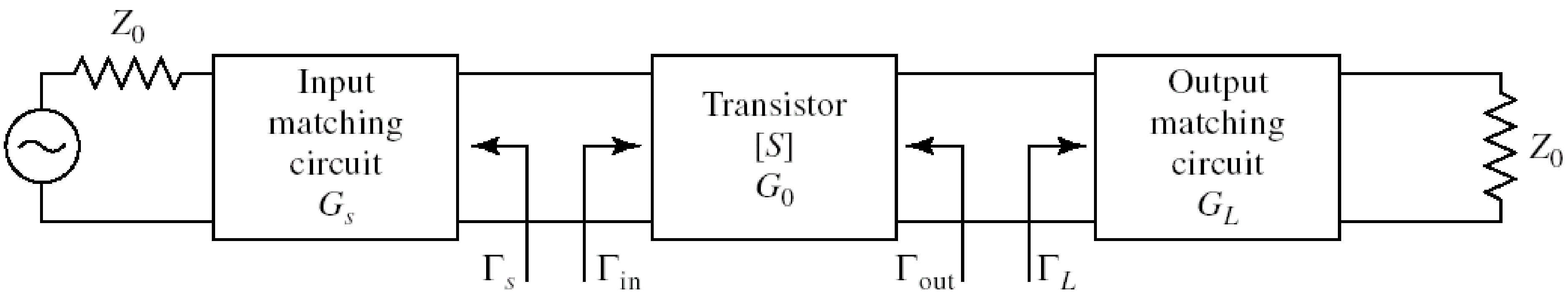
Stabilization of two-port



Power Gain of Microwave Amplifiers

Microwave Amplifiers

Design for Maximum Gain



- Maximum power gain (complex conjugate matching):

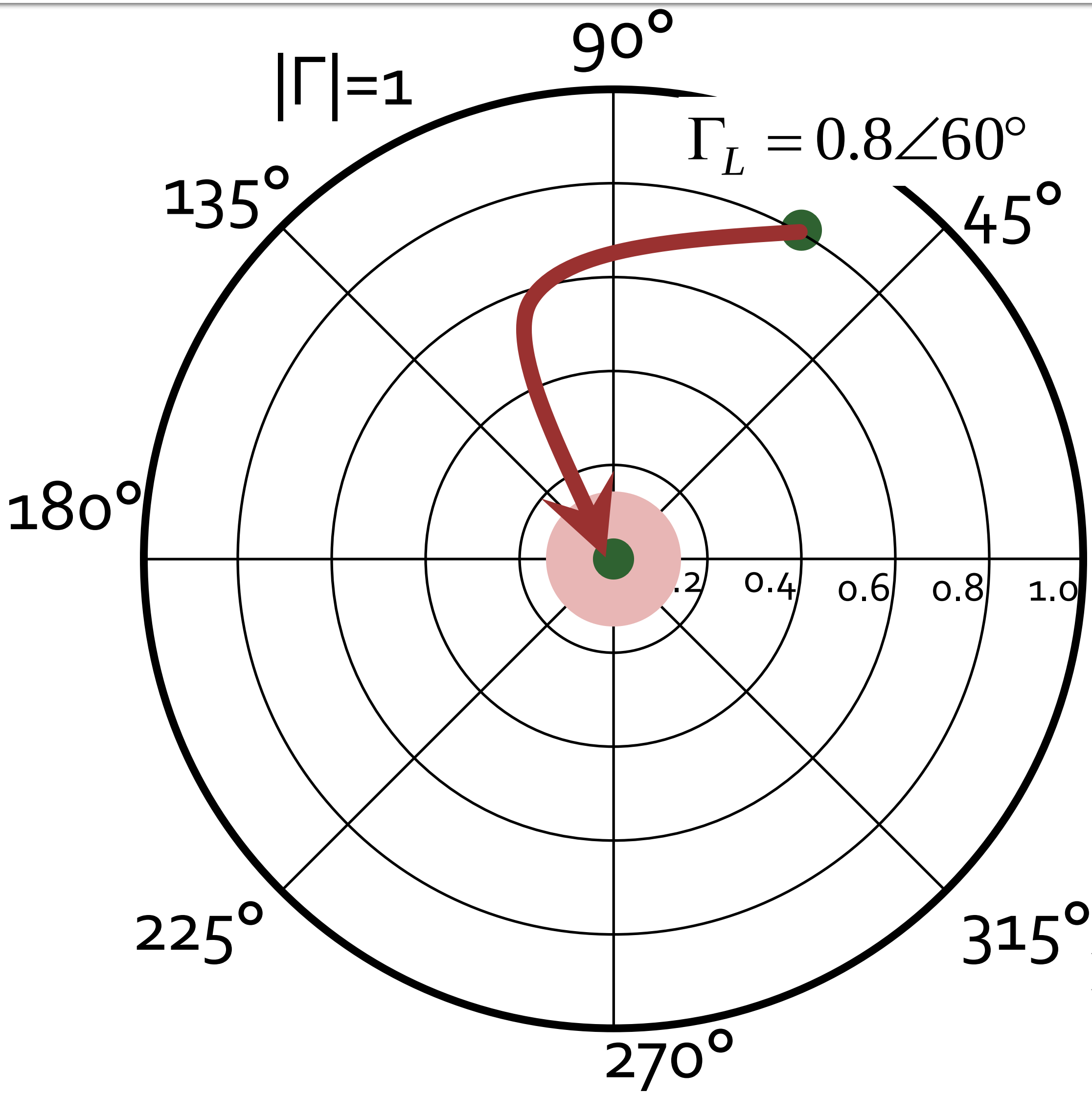
$$\Gamma_{in} = \Gamma_S^* \qquad \Gamma_{out} = \Gamma_L^*$$

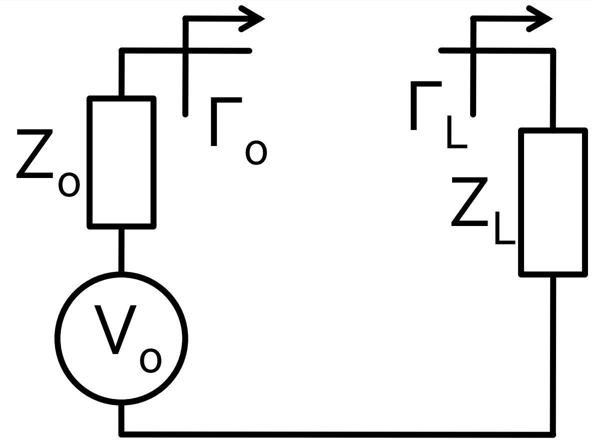
- For lossless matching sections

$$G_{T\max} = \frac{|S_{21}|^2 \cdot \left(1-|\Gamma_S|^2\right) \cdot \left(1-|\Gamma_L|^2\right)}{|1-\Gamma_S \cdot \Gamma_{in}|^2 \cdot |1-S_{22} \cdot \Gamma_L|^2} \qquad G_{T\max} = \frac{1}{1-|\Gamma_S|^2} \cdot |S_{21}|^2 \cdot \frac{1-|\Gamma_L|^2}{|1-S_{22} \cdot \Gamma_L|^2}$$

- For the general case of the bilateral transistor ($S_{12} \neq 0$) Γ_{in} and Γ_{out} depend on each other so the input and output sections must be matched simultaneously

The Smith Chart, matching, $Z_L \neq Z_o$





Matching Z_L load to Z_o source.
We normalize Z_L over Z_o

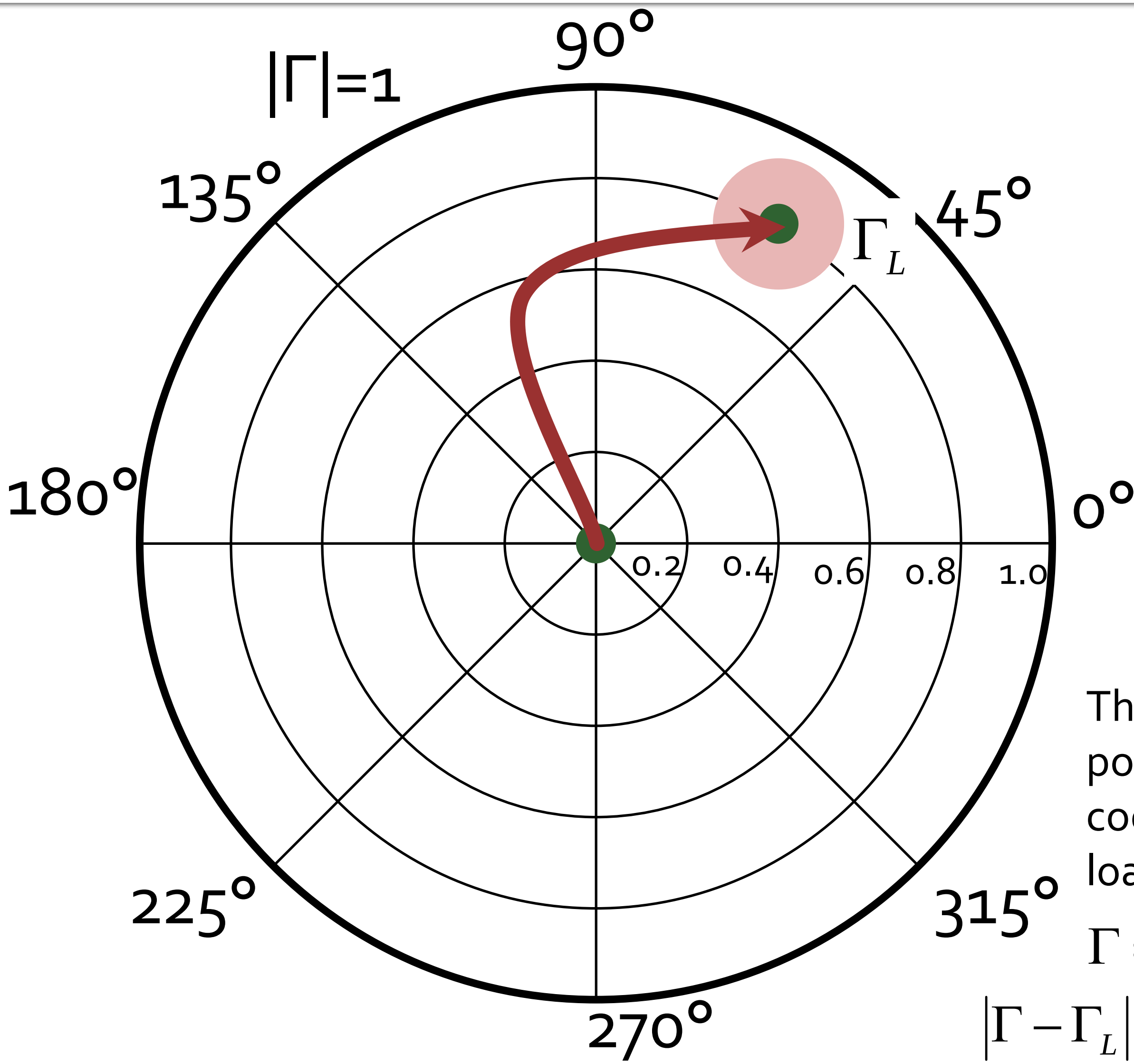
$$Z_L = 21.429\Omega + j \cdot 82.479\Omega$$
$$z_L = 0.429 + j \cdot 1.65$$
$$\Gamma_L = 0.8\angle 60°$$

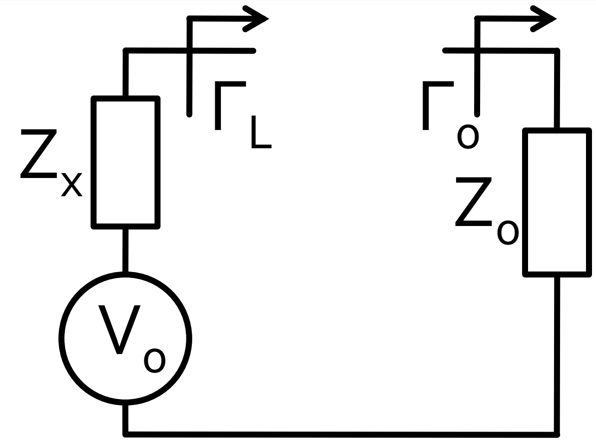
We must move the point denoting the reflection coefficient in the area where with a Z_o source we have:

$\Gamma_0 = 0$ perfect match

$|\Gamma_0| \leq \Gamma_m$ "good enough" match

The Smith Chart, matching, $Z_L=Z_o$





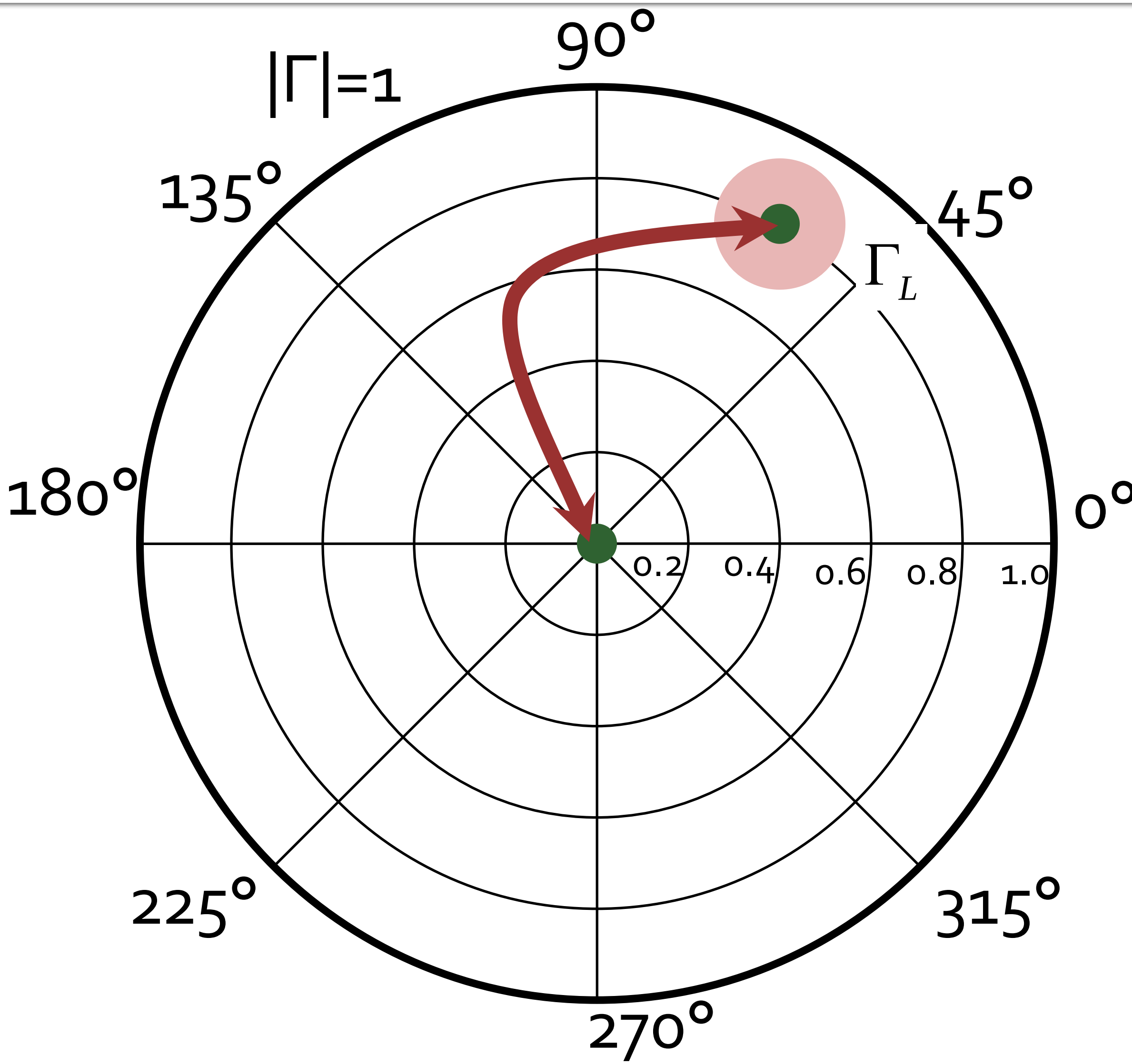
The source (eg. the transistor) having Z_X needs to see a certain reflection coefficient Γ_L towards the load Z_o

The matching circuit must move the point denoting the reflection coefficient in the area where for a Z_o load (Γ_o=0) we see towards it:

$\Gamma = \Gamma_L$ perfect match

$\left|\Gamma - \Gamma_L\right| \leq \Gamma_m$ "good enough" match

The Smith Chart, matching , $Z_L \neq Z_o$, $Z_L = Z_o$



- The matching sections needed to move
  - Γ_L in Γ_o
  - Γ_o in Γ_L
- are **identical**. They differ only by the **order** in which the elements are introduced into the matching circuit
- As a result, we can use in match design the same:
  - **methods**
  - **formulae**

Simultaneous matching

$$\Gamma_{in} = \Gamma_S^*$$

$$\Gamma_{in} = S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L}$$

$$\Gamma_S^* = S_{11} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_L}{1 - S_{22} \cdot \Gamma_L}$$

$$\Gamma_{out} = \Gamma_L^*$$

$$\Gamma_{out} = S_{22} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_S}{1 - S_{11} \cdot \Gamma_S}$$

$$\Gamma_L^* = S_{22} + \frac{S_{12} \cdot S_{21} \cdot \Gamma_S}{1 - S_{11} \cdot \Gamma_S}$$

- We find Γ_S

$$\Gamma_S = S_{11}^* + \frac{S_{12}^* \cdot S_{21}^*}{1/\Gamma_L^* - S_{22}^*}$$

$$\Gamma_L^* = \frac{S_{22} - \Delta \cdot \Gamma_S}{1 - S_{11} \cdot \Gamma_S}$$

$$\Gamma_S \cdot \left(1 - |S_{22}|^2\right) + \Gamma_S^2 \cdot \left(\Delta \cdot S_{22}^* - S_{11}\right) = \Gamma_S \cdot \left(\Delta \cdot S_{11}^* \cdot S_{22}^* - |S_{22}|^2 - \Delta \cdot S_{12}^* \cdot S_{21}^*\right) + \\ + S_{11}^* \cdot \left(1 - |S_{22}|^2\right) + S_{12}^* \cdot S_{21}^* \cdot S_{22}$$

Simultaneous matching

$$\Delta\cdot\left(S_{11}^{*}\cdot S_{22}^{*}-S_{12}^{*}\cdot S_{21}^{*}\right)=\left|\Delta\right|^{2}$$

$$\Gamma_{S}^{2}\cdot\left(S_{11}-\Delta\cdot S_{22}^{*}\right)+\Gamma_{S}\cdot\left(\left|\Delta\right|^{2}-\left|S_{11}\right|^{2}+\left|S_{22}\right|^{2}-1\right)+\left(S_{11}^{*}-\Delta^{*}\cdot S_{22}\right)=0$$

- A quadratic equation

$$\Gamma_{S}=\frac{B_{1}\pm\sqrt{B_{1}^{2}-4\cdot\left|C_{1}\right|^{2}}}{2\cdot C_{1}}$$

- Similarly

$$\Gamma_{L}=\frac{B_{2}\pm\sqrt{B_{2}^{2}-4\cdot\left|C_{2}\right|^{2}}}{2\cdot C_{2}}$$

- With variables defined as:

$$\begin{cases}B_{1}=1+\left|S_{11}\right|^{2}-\left|S_{22}\right|^{2}-\left|\Delta\right|^{2}\\C_{1}=S_{11}-\Delta\cdot S_{22}^{*}\end{cases}\quad\begin{cases}B_{2}=1+\left|S_{22}\right|^{2}-\left|S_{11}\right|^{2}-\left|\Delta\right|^{2}\\C_{2}=S_{22}-\Delta\cdot S_{11}^{*}\end{cases}$$

Simultaneous matching

- Simultaneous matching is possible if:

$$B_1^2 - 4 \cdot |C_1|^2 > 0 \qquad B_2^2 - 4 \cdot |C_2|^2 > 0$$

$$\Delta \cdot \left(S_{11}^* \cdot S_{22}^* - S_{12}^* \cdot S_{21}^*\right) = |\Delta|^2$$

$$|C_1|^2 = \left|S_{11} - \Delta \cdot S_{22}^*\right|^2 = |S_{12}|^2 \cdot |S_{21}|^2 + \left(1 - |S_{22}|^2\right) \cdot \left(|S_{11}|^2 - |\Delta|^2\right)$$

$$B_1^2 - 4 \cdot |C_1|^2 = \left(1 + |S_{11}|^2\right)^2 + \left(|S_{22}|^2 + |\Delta|^2\right)^2 -$$

$$-2 \cdot \left(1 + |S_{11}|^2\right) \cdot \left(|S_{22}|^2 + |\Delta|^2\right) - 4 \cdot |S_{12} \cdot S_{21}|^2 - 4 \cdot \left(1 - |S_{22}|^2\right) \cdot \left(|S_{22}|^2 - |\Delta|^2\right)$$

$$B_1^2 - 4 \cdot |C_1|^2 = \left(1 + |S_{11}|^2\right)^2 + \left(|S_{22}|^2 + |\Delta|^2\right)^2 -$$

$$-4 \cdot |S_{11}|^2 - 4 \cdot |S_{22}|^2 \cdot |\Delta|^2 - 2 \cdot \left(1 - |S_{11}|^2\right) \cdot \left(|S_{22}|^2 - |\Delta|^2\right) - 4 \cdot |S_{12} \cdot S_{21}|^2$$

Simultaneous matching

$$B_1^2 - 4\cdot|C_1|^2 = \left(1+|S_{11}|^2\right)^2 + \left(|S_{22}|^2 + |\Delta|^2\right)^2 - \\ -4\cdot|S_{11}|^2 - 4\cdot|S_{22}|^2\cdot|\Delta|^2 - 2\cdot\left(1-|S_{11}|^2\right)\cdot\left(|S_{22}|^2 - |\Delta|^2\right) - 4\cdot|S_{12}\cdot S_{21}|^2$$

$$B_1^2 - 4\cdot|C_1|^2 = \left(1-|S_{11}|^2\right)^2 + \left(|S_{22}|^2 - |\Delta|^2\right)^2 - 2\cdot\left(1-|S_{11}|^2\right)\cdot\left(|S_{22}|^2 - |\Delta|^2\right) - 4\cdot|S_{12}\cdot S_{21}|^2$$

$$B_1^2 - 4\cdot|C_1|^2 = \left(1-|S_{11}|^2 - |S_{22}|^2 + |\Delta|^2\right)^2 - 4\cdot|S_{12}\cdot S_{21}|^2$$

$$B_1^2 - 4\cdot|C_1|^2 = \left(K\cdot 2\cdot|S_{12}\cdot S_{21}|\right)^2 - 4\cdot|S_{12}\cdot S_{21}|^2$$

$$B_1^2 - 4\cdot|C_1|^2 = 4\cdot|S_{12}|^2\cdot|S_{21}|^2\cdot\left(K^2 - 1\right)$$

- Similarly

$$B_2^2 - 4\cdot|C_2|^2 = 4\cdot|S_{12}|^2\cdot|S_{21}|^2\cdot\left(K^2 - 1\right)$$

Simultaneous matching

$$\Gamma_S = \frac{B_1 \pm \sqrt{B_1^2 - 4\cdot|C_1|^2}}{2\cdot C_1} \qquad \Gamma_L = \frac{B_2 \pm \sqrt{B_2^2 - 4\cdot|C_2|^2}}{2\cdot C_2}$$

- Necesar pentru solutii

$$|\Gamma_S| < 1 \qquad |\Gamma_L| < 1$$

$$|\Delta| = |S_{11}\cdot S_{22} - S_{12}\cdot S_{21}| < 1 \qquad \begin{cases} B_1 > 0 \\ B_2 > 0 \end{cases}$$

$$K = \frac{1 - |S_{11}|^2 - |S_{22}|^2 + |\Delta|^2}{2\cdot|S_{12}\cdot S_{21}|} > 1 \qquad \begin{cases} B_1^2 - 4\cdot|C_1|^2 = 4\cdot|S_{12}|^2\cdot|S_{21}|^2\cdot\left(K^2 - 1\right) > 0 \\ B_2^2 - 4\cdot|C_2|^2 = 4\cdot|S_{12}|^2\cdot|S_{21}|^2\cdot\left(K^2 - 1\right) > 0 \end{cases}$$

Simultaneous matching

- Simultaneous matching can be achieved **if and only if** the amplifier is **unconditionally stable** at the operating frequency, and |Γ|<1 solutions are those with "–" sign of quadratic solutions

$$\Gamma_S = \frac{B_1 - \sqrt{B_1^2 - 4 \cdot |C_1|^2}}{2 \cdot C_1} \qquad \Gamma_L = \frac{B_2 - \sqrt{B_2^2 - 4 \cdot |C_2|^2}}{2 \cdot C_2}$$

$$\begin{cases} B_1 = 1 + |S_{11}|^2 - |S_{22}|^2 - |\Delta|^2 \\ C_1 = S_{11} - \Delta \cdot S_{22}^* \end{cases} \qquad \begin{cases} B_2 = 1 + |S_{22}|^2 - |S_{11}|^2 - |\Delta|^2 \\ C_2 = S_{22} - \Delta \cdot S_{11}^* \end{cases}$$

Simultaneous matching

- In the case of the simultaneous matching the amplifier achieves the maximum transducer power gain for the bilateral transistor

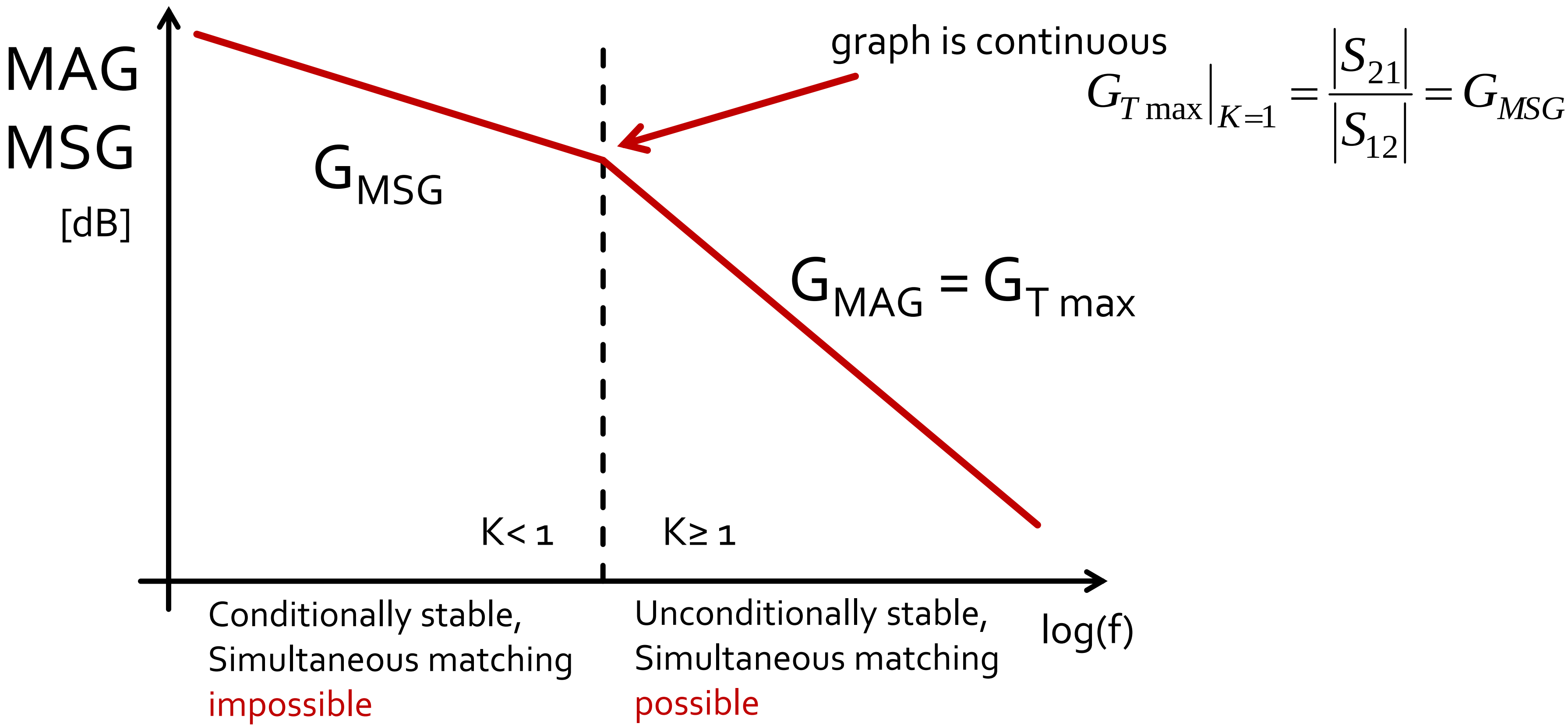
$$G_{T\max} = \frac{|S_{21}|}{|S_{12}|} \cdot \left(K - \sqrt{K^2 - 1}\right)$$

- If the device is **not unconditionaly stable** at a certain frequency we can use MSG (Maximum Stable Gain) as an indicator of the capability to obtain a power gain in stable conditions

$$G_{MSG} = \frac{|S_{21}|}{|S_{12}|}$$

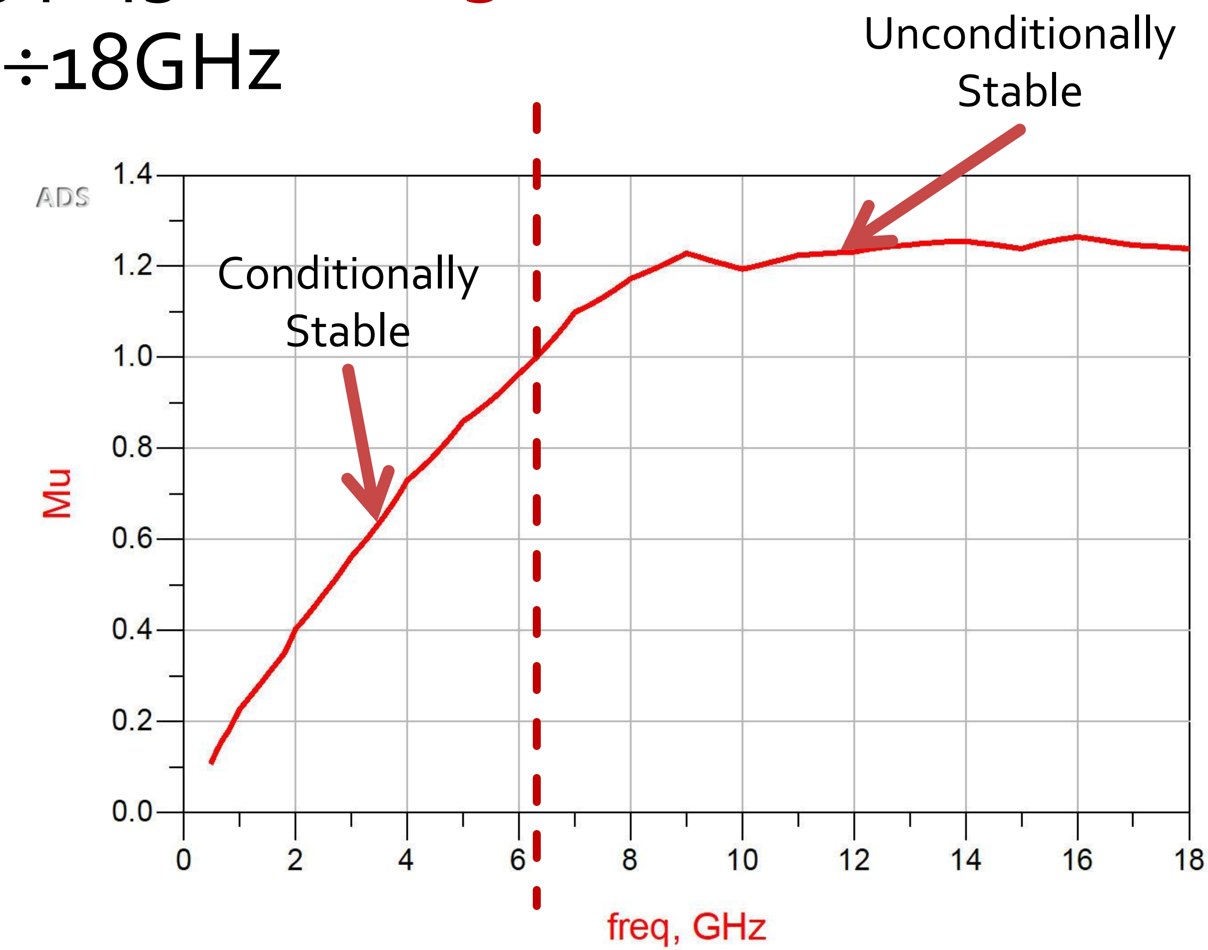
Maximum Available Gain

- Indicator across full frequency range of the capability to obtain a power gain



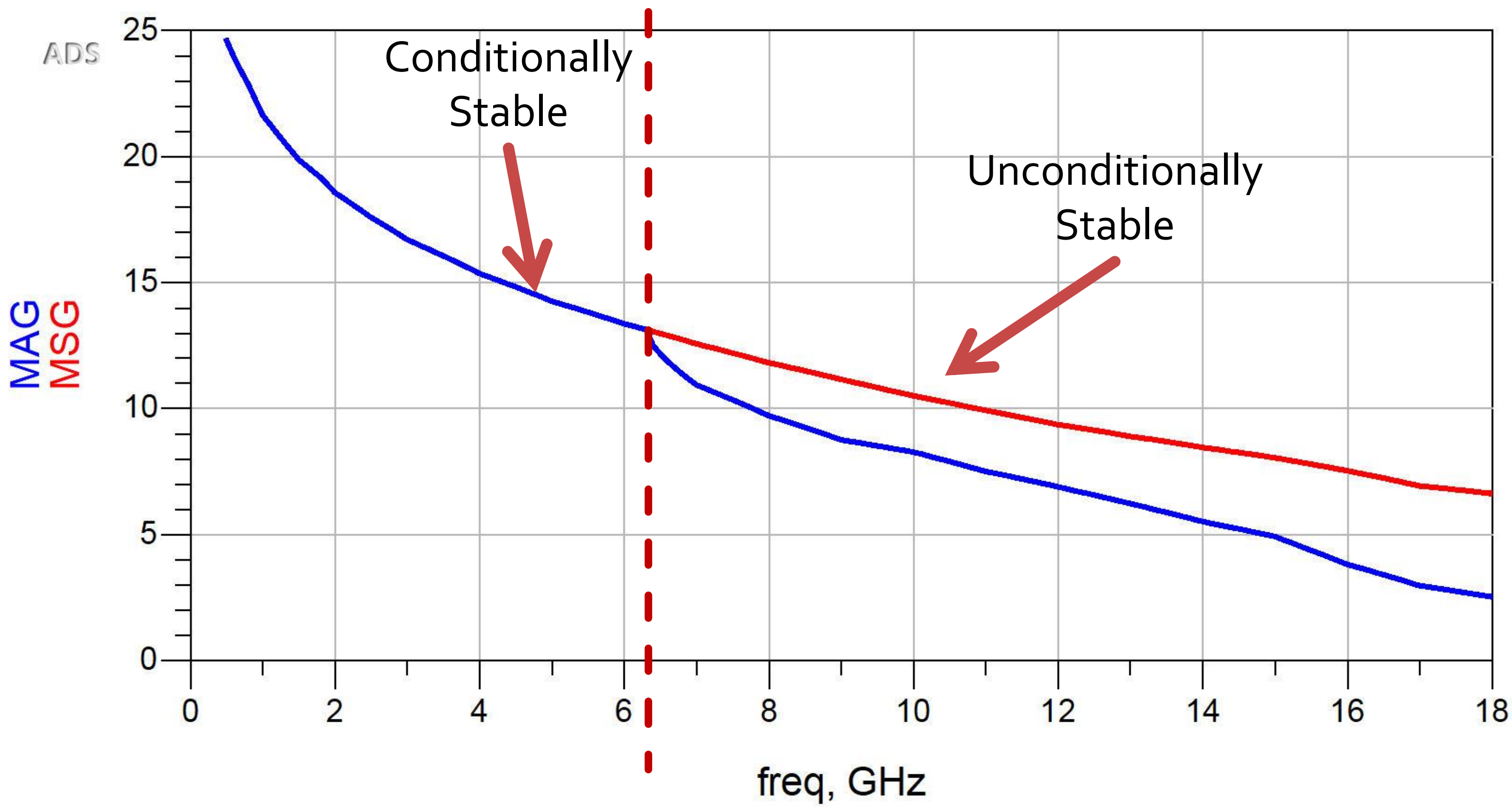
Stability

- ATF-34143 **at Vds=3V Id=20mA**.
- @0.5÷18GHz



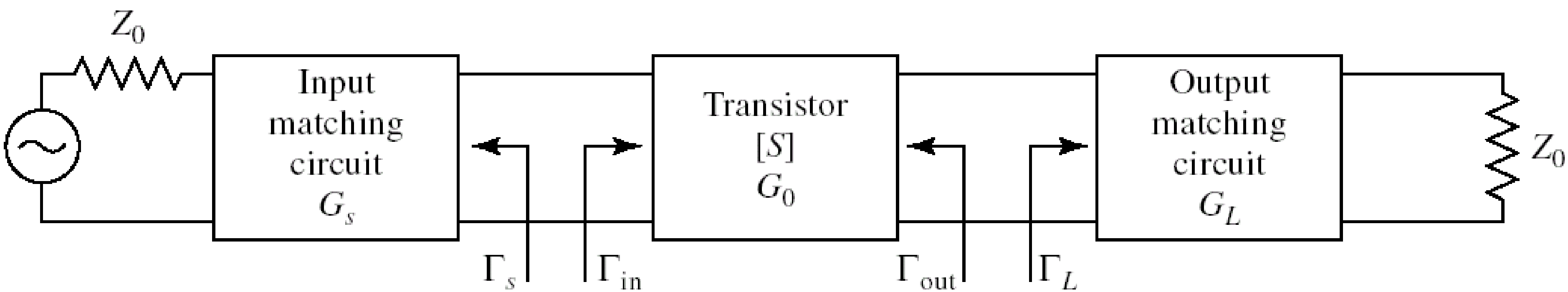
MAG/MSG

- ATF-34143 **at Vds=3V Id=20mA**.
- @0.5÷18GHz



Simultaneous matching, unilateral transistor

- In the case of **unilateral** amplifier/transistor (S12 = 0) simultaneous matching implies:



$$\Gamma_{in} = S_{11} \qquad \Gamma_{out} = S_{22}$$

$$\Gamma_S = S_{11}^* \qquad \Gamma_L = S_{22}^*$$

$$G_{T\max} = \frac{1}{1-|\Gamma_S|^2} \cdot |S_{21}|^2 \cdot \frac{1-|\Gamma_L|^2}{|1-S_{22}\cdot\Gamma_L|^2} \qquad G_{TU\max} = \frac{1}{1-|S_{11}|^2} \cdot |S_{21}|^2 \cdot \frac{1}{1-|S_{22}|^2}$$

Example

- ATF-34143 **at Vds=3V Id=20mA**.
  - without stabilization K = **0.886**, MAG = 14.248dB @ 5GHz
  - cannot be used with this bias conditions
- ATF-34143 **at Vds=4V Id=40mA**
  - without stabilization K = **1.031**, MAG = 12.9dB @ 5GHz
  - we use this bias conditions for simultaneous matching

Example

- ATF-34143 **at Vds=4V Id=40mA**.
- @5GHz
  - $S_{11} = 0.64\angle 111°$
  - $S_{12} = 0.117\angle -27°$
  - $S_{21} = 2.923\angle -6°$
  - $S_{22} = 0.21\angle 111°$

Computations

- Complex S Parameters
  - S11 = -0.229+0.597·j
  - S12 = 0.104-0.053·j
  - S21 = 2.907-0.306·j
  - S22 = -0.075+0.196·j

$$G_{T\max} = \frac{|S_{21}|}{|S_{12}|} \cdot \left(K - \sqrt{K^2 - 1}\right) = 19.497 = 12.9\,\text{dB}$$

$$G_{TU\max} = \frac{1}{1 - |S_{11}|^2} \cdot |S_{21}|^2 \cdot \frac{1}{1 - |S_{22}|^2} = 15.139 = 11.8\,\text{dB}$$

Computations

$$\begin{cases} B_1 = 1 + |S_{11}|^2 - |S_{22}|^2 - |\Delta|^2 \\ C_1 = S_{11} - \Delta \cdot S_{22}^* \end{cases}$$

$$\begin{cases} B_2 = 1 + |S_{22}|^2 - |S_{11}|^2 - |\Delta|^2 \\ C_2 = S_{22} - \Delta \cdot S_{11}^* \end{cases}$$

$$\begin{cases} B_1 = ? \\ C_1 = ? \end{cases}$$

$$\begin{cases} B_2 = ? \\ C_2 = ? \end{cases}$$

$$\Gamma_S = \frac{B_1 - \sqrt{B_1^2 - 4 \cdot |C_1|^2}}{2 \cdot C_1}$$

$$\Gamma_L = \frac{B_2 - \sqrt{B_2^2 - 4 \cdot |C_2|^2}}{2 \cdot C_2}$$

$$\Gamma_S = ?$$

$$\Gamma_L = ?$$

Computations

$$\begin{cases} B_1 = 1 + |S_{11}|^2 - |S_{22}|^2 - |\Delta|^2 \\ C_1 = S_{11} - \Delta \cdot S_{22}^* \end{cases}$$

$$\begin{cases} B_2 = 1 + |S_{22}|^2 - |S_{11}|^2 - |\Delta|^2 \\ C_2 = S_{22} - \Delta \cdot S_{11}^* \end{cases}$$

$$\begin{cases} B_1 = 1.207 \\ C_1 = -0.277 + j \cdot 0.529 \end{cases}$$

$$\begin{cases} B_2 = 0.476 \\ C_2 = -0.222 - j \cdot 0.013 \end{cases}$$

$$\Gamma_S = \frac{B_1 - \sqrt{B_1^2 - 4 \cdot |C_1|^2}}{2 \cdot C_1}$$

$$\Gamma_L = \frac{B_2 - \sqrt{B_2^2 - 4 \cdot |C_2|^2}}{2 \cdot C_2}$$

$$\Gamma_S = -0.403 - j \cdot 0.768$$

$$|\Gamma_S| = 0.867 < 1$$

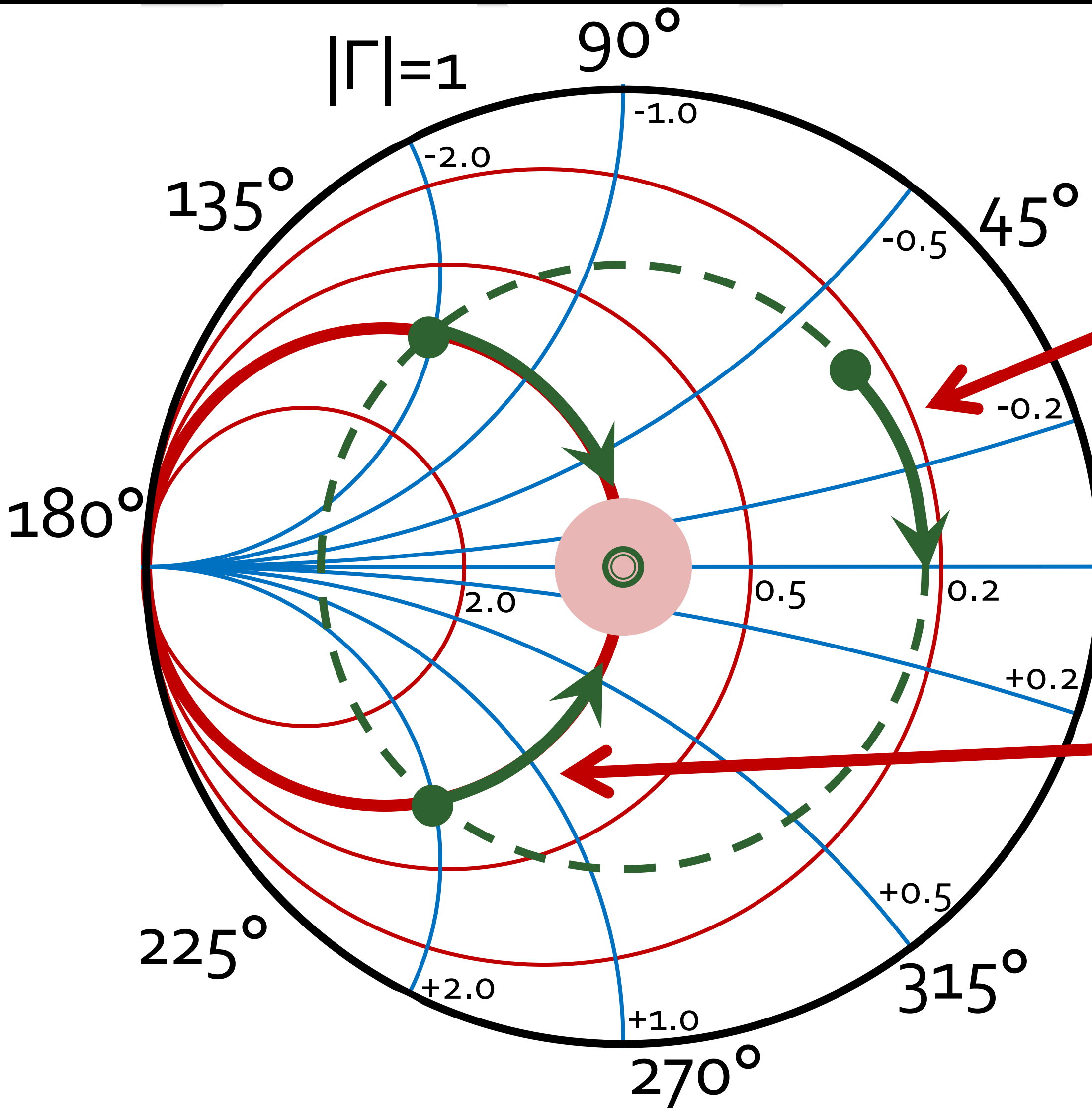
$$\Gamma_S = 0.867 \angle -117.7°$$

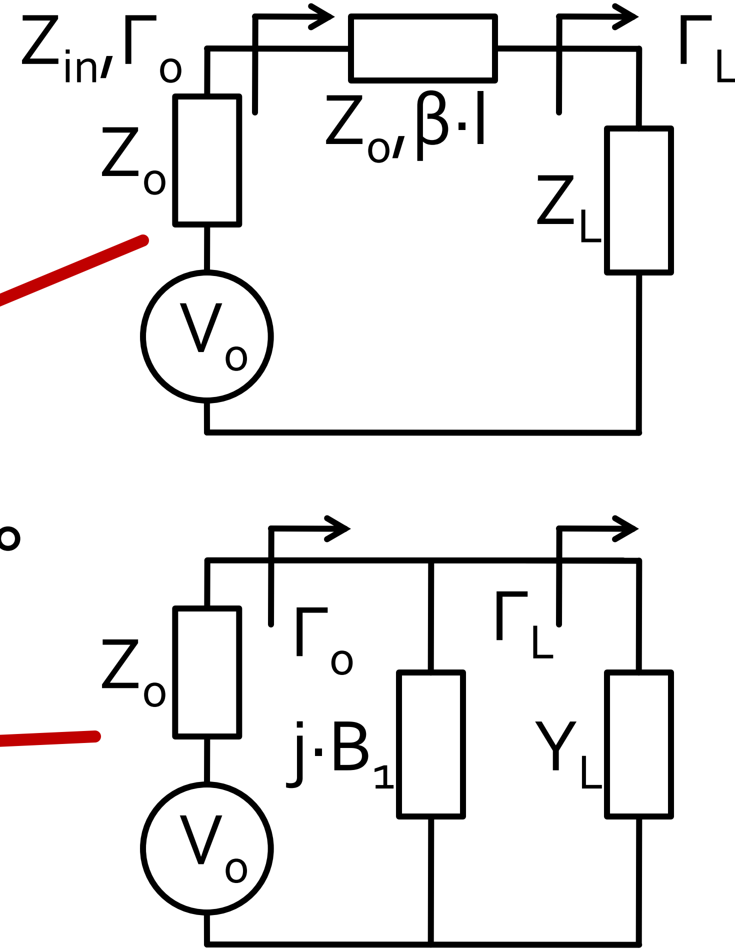
$$\Gamma_L = -0.685 + j \cdot 0.04$$

$$|\Gamma_L| = 0.686 < 1$$

$$\Gamma_L = 0.686 \angle 176.7°$$

Shunt stub matching, C6-7





$$|\Gamma_{in}| = |\Gamma_L|$$

$$g_{in} = 1$$

Analytical solution (Γ_S)

$$\cos(\varphi + 2\theta) = -|\Gamma_S|$$

$$\theta_{sp} = \beta \cdot l = \tan^{-1} \frac{\mp 2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}}$$

$$\Gamma_S = 0.867\angle -117.7°$$

$$|\Gamma_S| = 0.867; \quad \varphi = -117.7° \qquad \cos(\varphi + 2\theta) = -0.867 \Rightarrow \quad (\varphi + 2\theta) = \pm 150.1°$$

- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **shunt stub** equation
  - **"+" solution**

    $$(-117.7° + 2\theta) = +150.1° \qquad \theta = 133.9° \qquad \operatorname{Im} y_S = \frac{-2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} = -3.477$$

    $$\theta_{sp} = \tan^{-1}(\operatorname{Im} y_S) = -74°(+180°) \to \theta_{sp} = 106°$$

  - **"-" solution**

    $$(-117.7° + 2\theta) = -150.1° \qquad \theta = -16.2°(+180°) \to \theta = 163.8°$$

    $$\operatorname{Im} y_S = \frac{+2 \cdot |\Gamma_S|}{\sqrt{1 - |\Gamma_S|^2}} = +3.477 \qquad \theta_{sp} = \tan^{-1}(\operatorname{Im} y_S) = 74°$$

Analytical solution (Γ_L)

$$\cos(\varphi + 2\theta) = -|\Gamma_L|$$

$$\theta_{sp} = \beta \cdot l = \tan^{-1} \frac{\mp 2 \cdot |\Gamma_L|}{\sqrt{1 - |\Gamma_L|^2}}$$

$$\Gamma_L = 0.686\angle 176.7°$$

$$|\Gamma_L| = 0.686; \quad \varphi = 176.7°$$

- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **shunt stub** equation
  - **"+" solution**
  - **"-" solution**

Analytical solution (Γ_L)

$$\cos(\varphi + 2\theta) = -|\Gamma_L|$$

$$\theta_{sp} = \beta \cdot l = \tan^{-1} \frac{\mp 2 \cdot |\Gamma_L|}{\sqrt{1 - |\Gamma_L|^2}}$$

$$\Gamma_L = 0.686\angle 176.7°$$

$$|\Gamma_L| = 0.686; \quad \varphi = 176.7° \qquad \cos(\varphi + 2\theta) = -0.686 \Rightarrow \quad (\varphi + 2\theta) = \pm 133.3°$$

- The **sign** (+/-) chosen for the **series line** equation imposes the **sign** used for the **shunt stub** equation
  - **"+" solution**

$$(176.7° + 2\theta) = +133.3° \qquad \theta = -21.7°(+180°) \rightarrow \theta = 158.3°$$

$$\theta_{sp} = \tan^{-1}(\operatorname{Im} y_L) = -62.1°(+180°) \rightarrow \theta_{sp} = 117.9° \qquad \operatorname{Im} y_L = \frac{-2 \cdot |\Gamma_L|}{\sqrt{1 - |\Gamma_L|^2}} = -1.885$$

  - **"-" solution**

$$(176.7° + 2\theta) = -133.3° \qquad \theta = -155°(+180°) \rightarrow \theta = 25°$$

$$\operatorname{Im} y_L = \frac{+2 \cdot |\Gamma_L|}{\sqrt{1 - |\Gamma_L|^2}} = +1.885 \qquad \theta_{sp} = \tan^{-1}(\operatorname{Im} y_L) = 62.1°$$

Complete analytical solution

- We choose **one** of the two possible solutions for the input matching

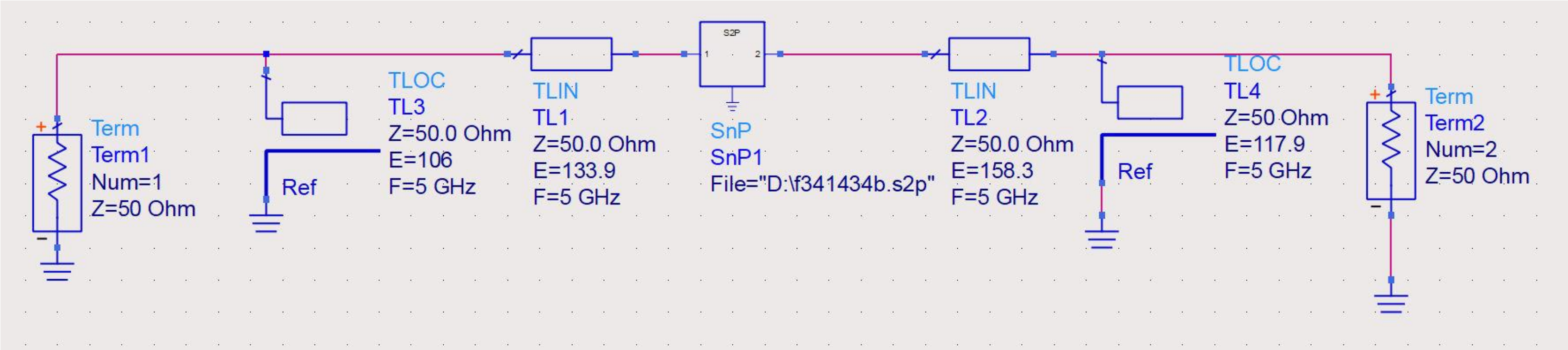
$$(\varphi + 2\theta) = \begin{cases} +150.1^\circ \\ -150.1^\circ \end{cases} \quad \theta = \begin{cases} 133.9^\circ \\ 163.8^\circ \end{cases} \quad \mathrm{Im}[y_S(\theta)] = \begin{cases} -3.477 \\ +3.477 \end{cases} \quad \theta_{sp} = \begin{cases} -74^\circ + 180^\circ = 106^\circ \\ +74^\circ \end{cases}$$

- Similarly for the output matching

$$(\varphi + 2\theta) = \begin{cases} +133.3^\circ \\ -133.3^\circ \end{cases} \quad \theta = \begin{cases} 158.3^\circ \\ 25.0^\circ \end{cases} \quad \mathrm{Im}[y_S(\theta)] = \begin{cases} -1.885 \\ +1.885 \end{cases} \quad \theta_{sp} = \begin{cases} 117.9^\circ \\ 62.1^\circ \end{cases}$$

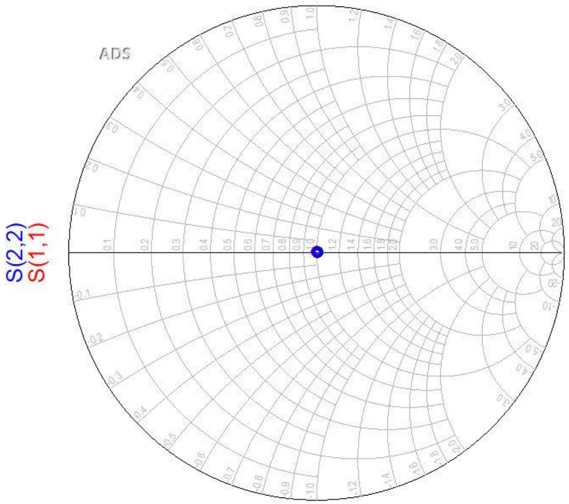
- In total there are **4** possible solutions input/output

ADS



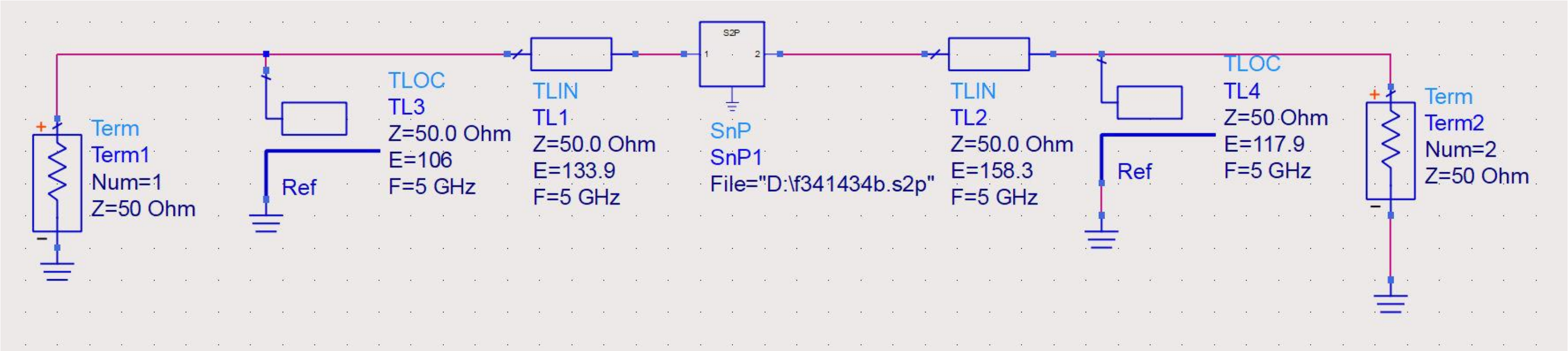
Eqn GT=10*log(mag(S(2,1))**2)

freq	S(2,1)	GT	S(1,1)	S(2,2)
5.000 GHz	4.415 / 157.353	12.900	0.004 / 86.088	0.004 / 37.766

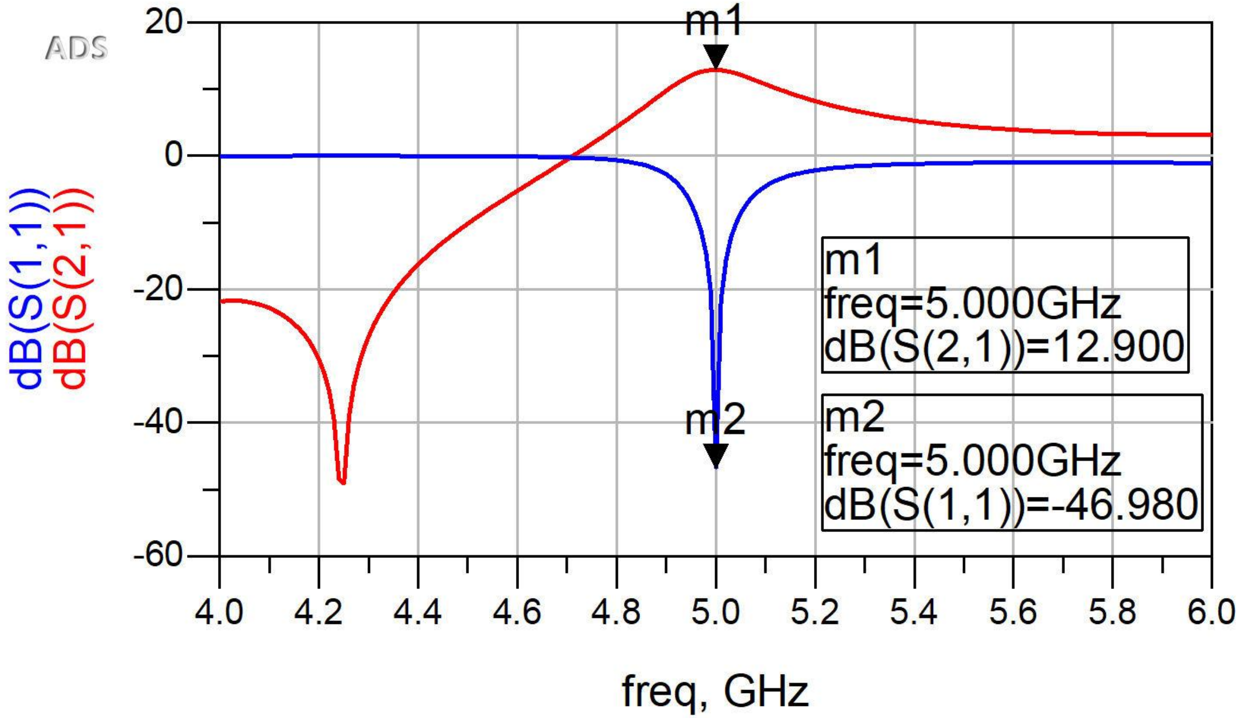


freq (5.000GHz to 5.000GHz)

ADS



Term
Term1
Num=1
Z=50 Ohm
Ref
TLOC
TL3
Z=50.0 Ohm
E=106
F=5 GHz
TLIN
TL1
Z=50.0 Ohm
E=133.9
F=5 GHz
S2P
SnP
SnP1
File="D:\f341434b.s2p"
TLIN
TL2
Z=50.0 Ohm
E=158.3
F=5 GHz
Ref
TLOC
TL4
Z=50 Ohm
E=117.9
F=5 GHz
Term
Term2
Num=2
Z=50 Ohm



ADS
dB(S(1,1))
dB(S(2,1))
m1
m2
m1
freq=5.000GHz
dB(S(2,1))=12.900
m2
freq=5.000GHz
dB(S(1,1))=-46.980
freq, GHz

Preview (for laboratories 3-4)

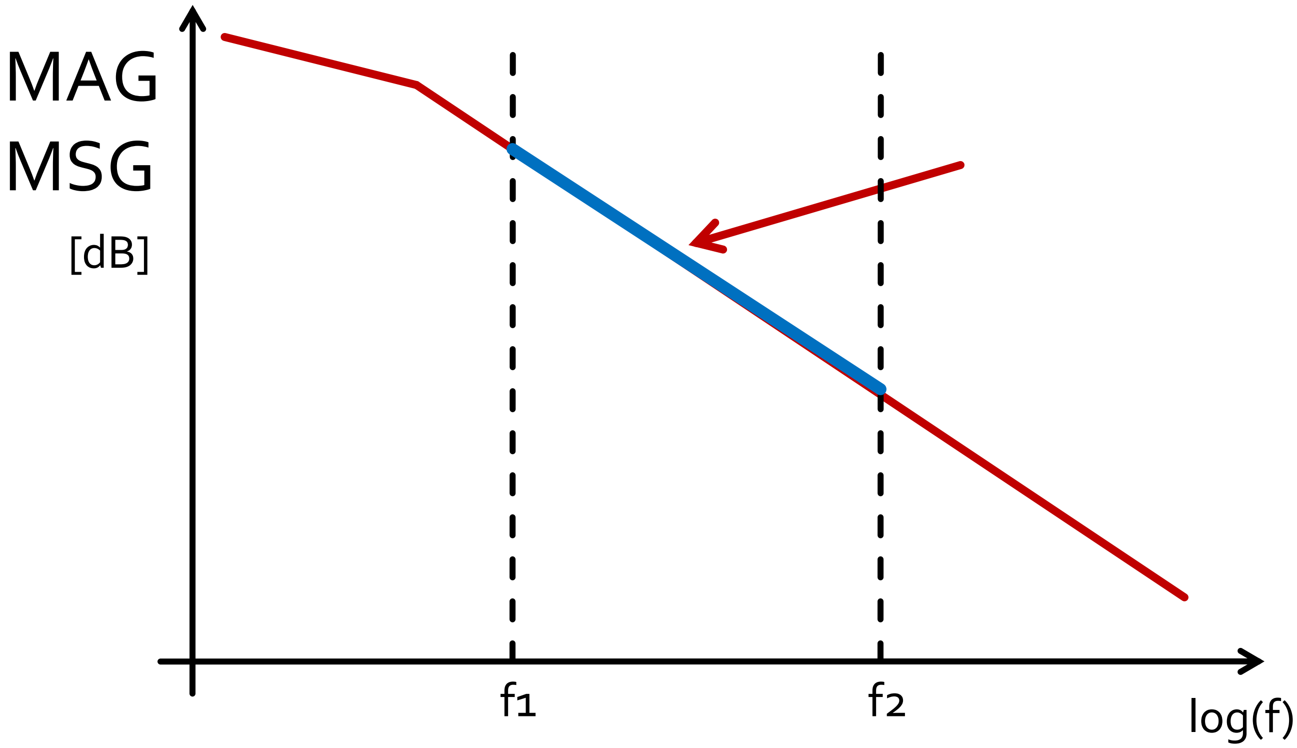
Microwave Low Noise Amplifier

Proiectare pentru castig impus

- Deseori este necesara o alta abordare decat "forta bruta" si se prefera obtinerea unui **castig mai mic** decat cel maxim posibil pentru:
  - conditii de zgomot avantajoase (L3)
  - conditii de stabilitate mai bune
  - obtinerea unui VSWR mai mic
  - controlul performantelor la mai multe frecvente
  - banda de functionare a amplificatorului

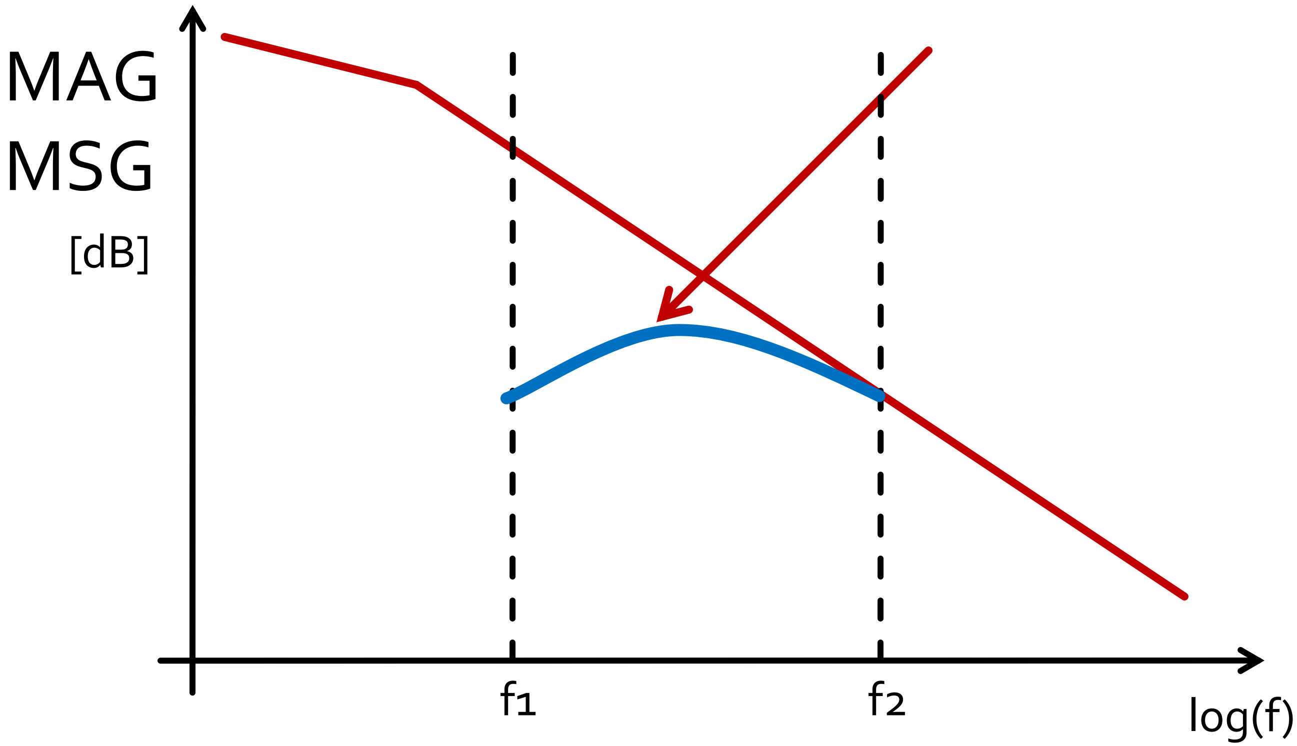
Amplificator de banda larga

- Adaptarea pentru castig maxim la doua frecvente genereaza o comportare dezechilibrata

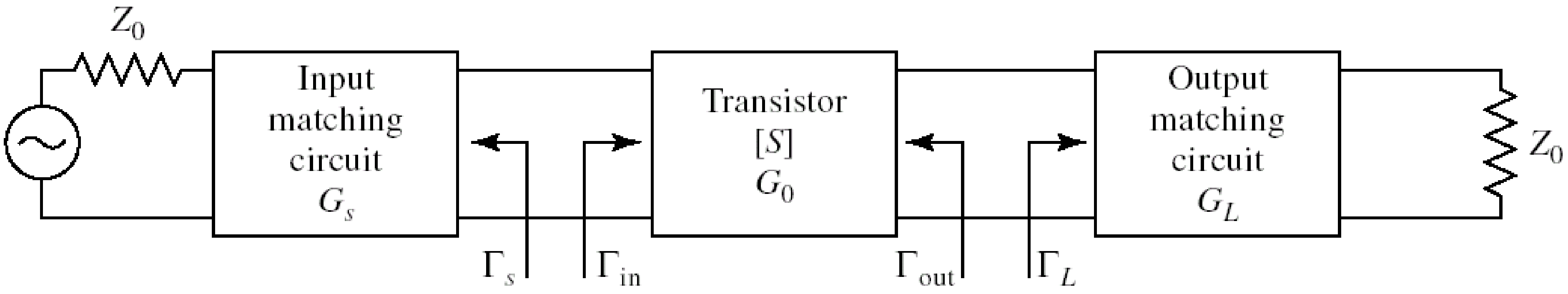


Amplificator de banda larga

- Adaptare pentru castig maxim la frecventa maxima
- Dezadaptare controlata la frecventa minima
  - eventual la mai multe frecvente din banda



Proiectare pentru castig impus

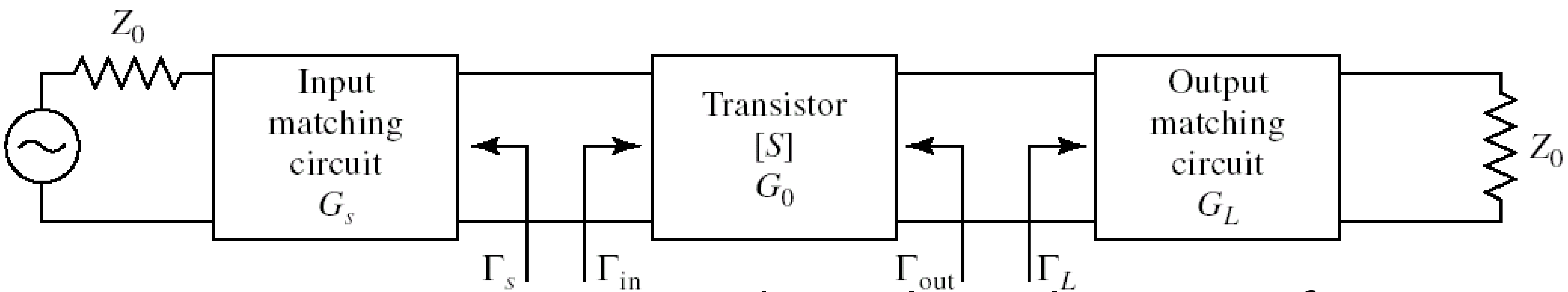


- Daca ipoteza tranzistorului unilateral este justificata:

$$G_{TU} = |S_{21}|^2 \cdot \frac{1-|\Gamma_S|^2}{|1-S_{11}\cdot\Gamma_S|^2} \cdot \frac{1-|\Gamma_L|^2}{|1-S_{22}\cdot\Gamma_L|^2}$$

$$G_S = \frac{1-|\Gamma_S|^2}{|1-S_{11}\cdot\Gamma_S|^2} \qquad G_0 = |S_{21}|^2 \qquad G_L = \frac{1-|\Gamma_L|^2}{|1-S_{22}\cdot\Gamma_L|^2}$$

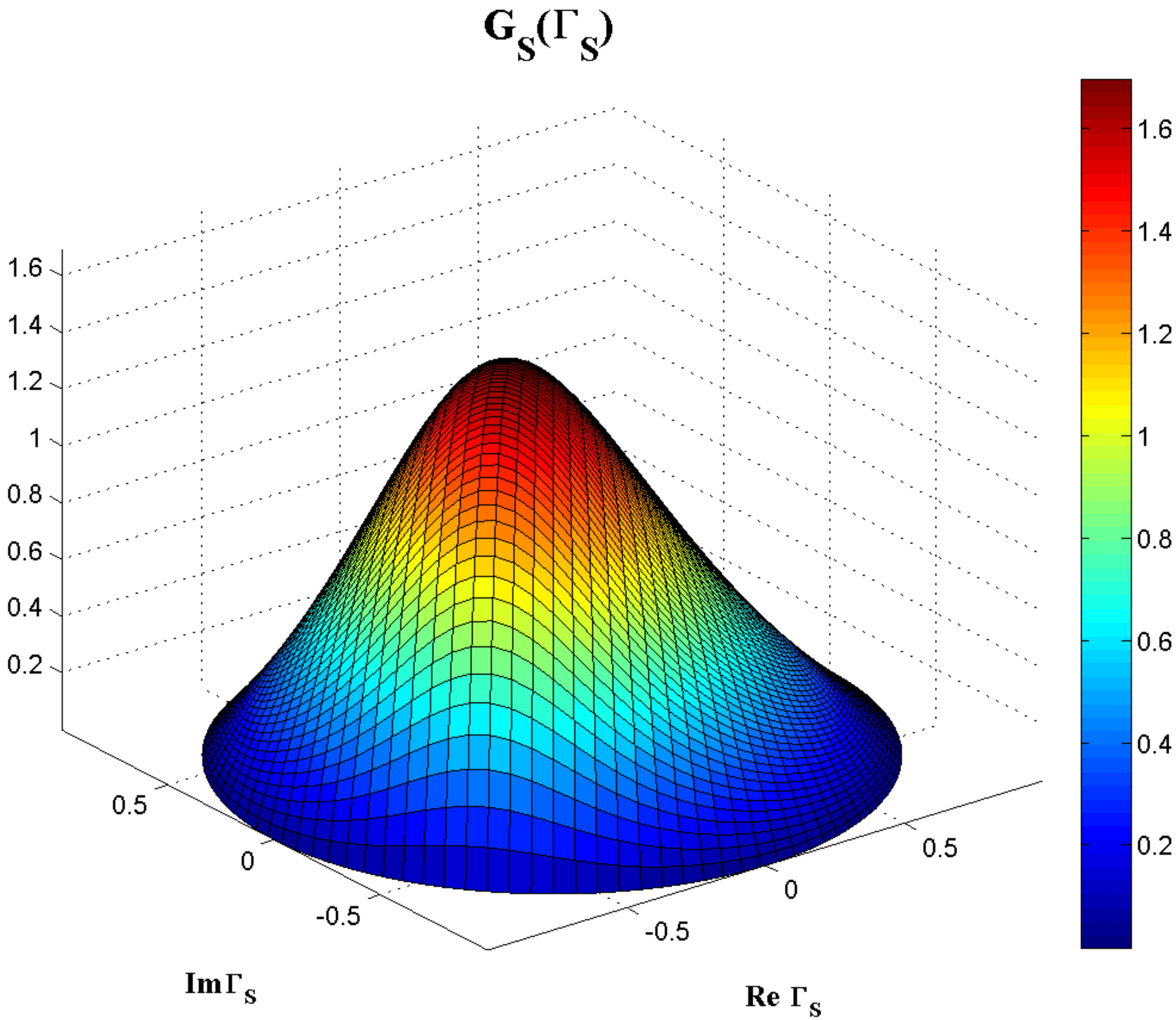
Proiectare pentru castig impus



- Daca ipoteza tranzistorului unilateral este justificata:
  - castigul adaugat prin adaptare mai buna la intrare **nu** depinde de adaptarea la iesire
  - castigul adaugat prin adaptare mai buna la iesire **nu** depinde de adaptarea la intrare
- Adaptarile la intrare/iesire pot fi tratate independent
  - Se pot impune cerinte diferite intrare/iesire
  - se tine cont de compunerea castigurilor generate

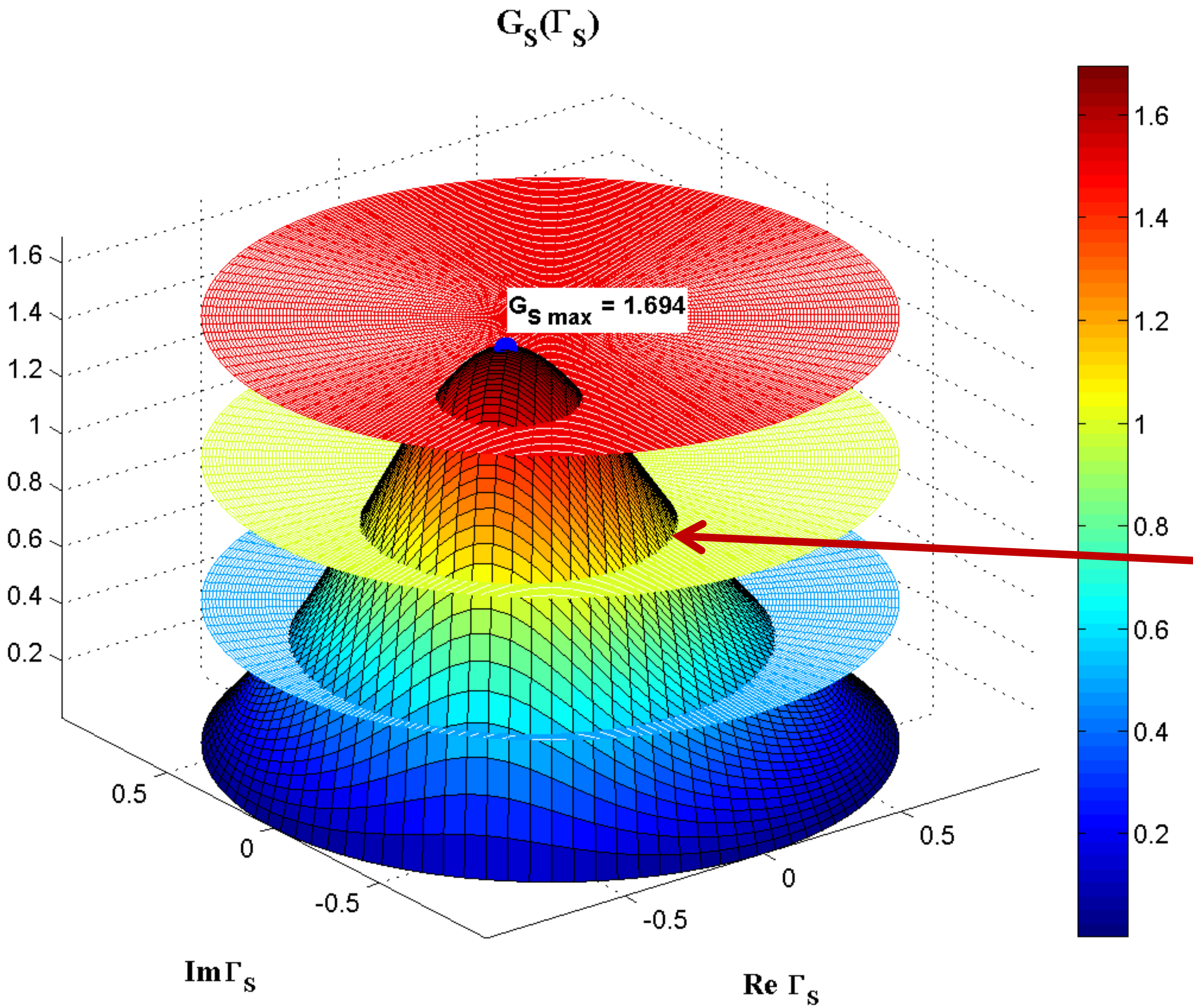
$$G_T = G_S \cdot G_0 \cdot G_L \qquad G_T[dB] = G_S[dB] + G_0[dB] + G_L[dB]$$

$G_S(\Gamma_S)$



$$G_S = \frac{1-|\Gamma_S|^2}{|1-S_{11}\cdot\Gamma_S|^2}$$

$G_S(\Gamma_S)$, nivel constant



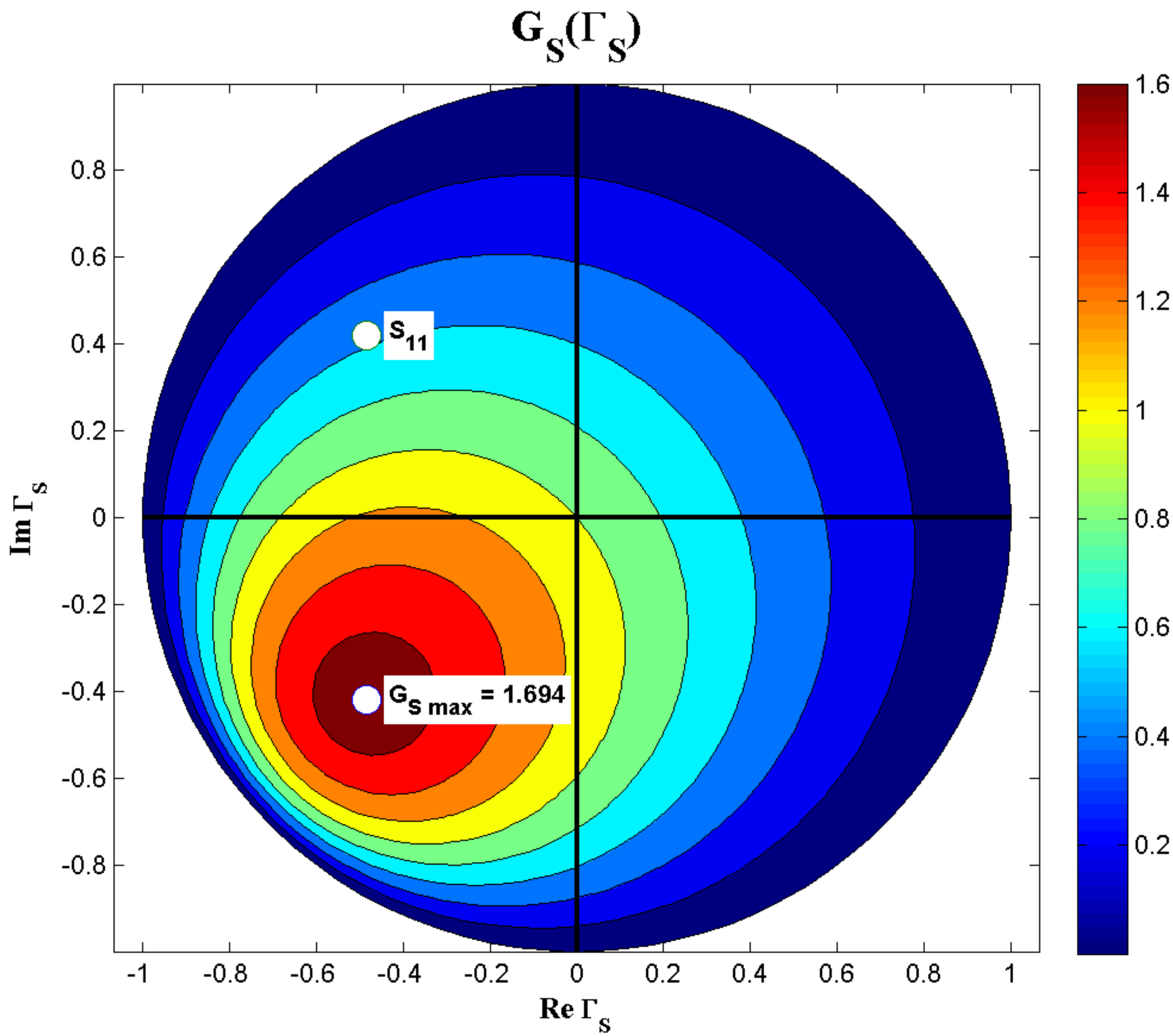
$G_S = 1.5$

$G_S = 1.0$

$G_S = 0.5$

Cercuri

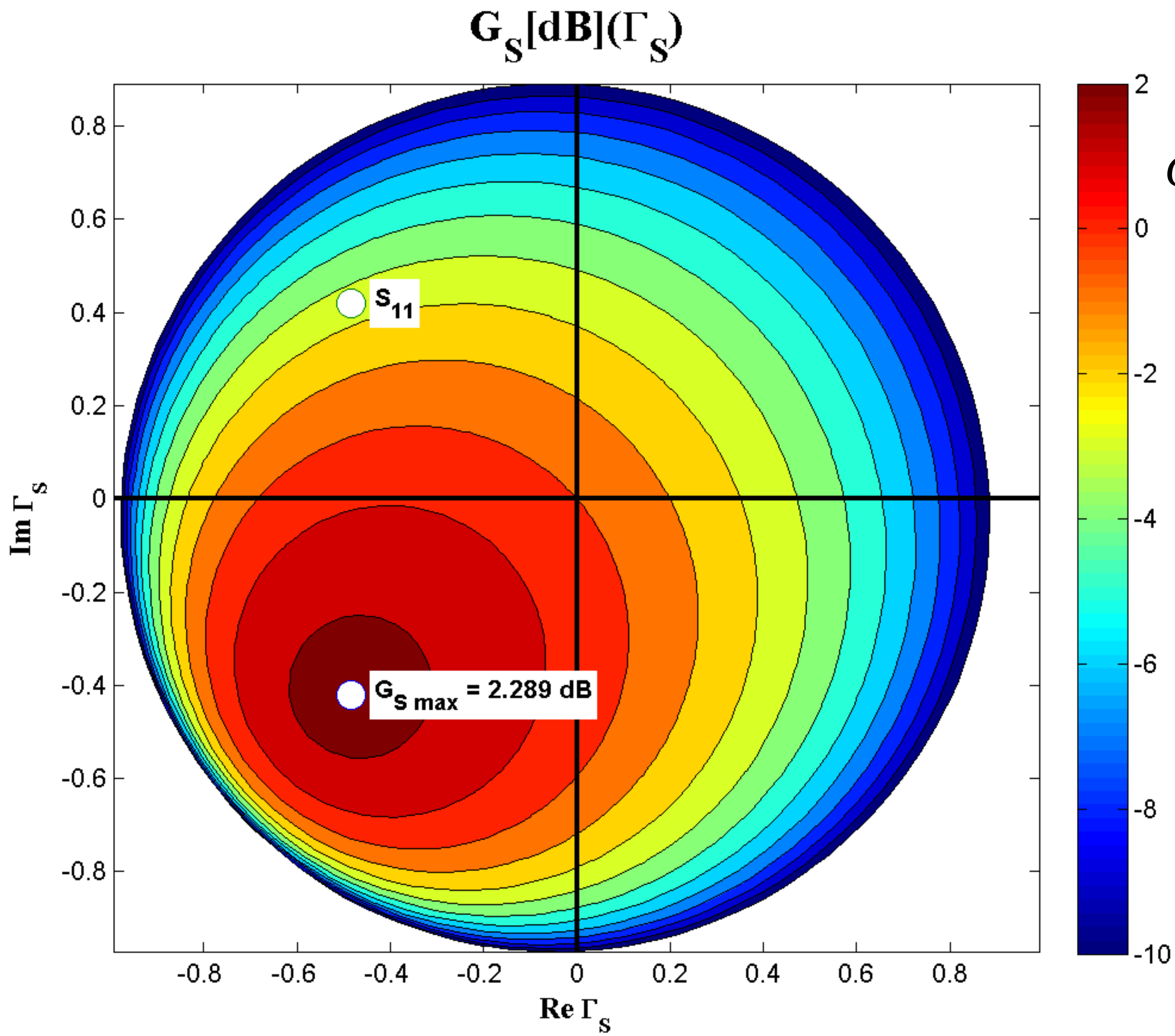
$G_S(\Gamma_S)$, diagrama de nivel



$$G_S = \frac{1-|\Gamma_S|^2}{|1-S_{11}\cdot\Gamma_S|^2}$$

$$G_{S\,\max} = G_S\Big|_{\Gamma_S = S_{11}^*}$$

G_S[dB](Γ_S), diagrama de nivel



$$G_S[dB] = 10 \cdot \log\left(\frac{1-|\Gamma_S|^2}{|1-S_{11}\cdot\Gamma_S|^2}\right)$$

$$G_{S\max} = G_S\Big|_{\Gamma_S = S_{11}^*}$$

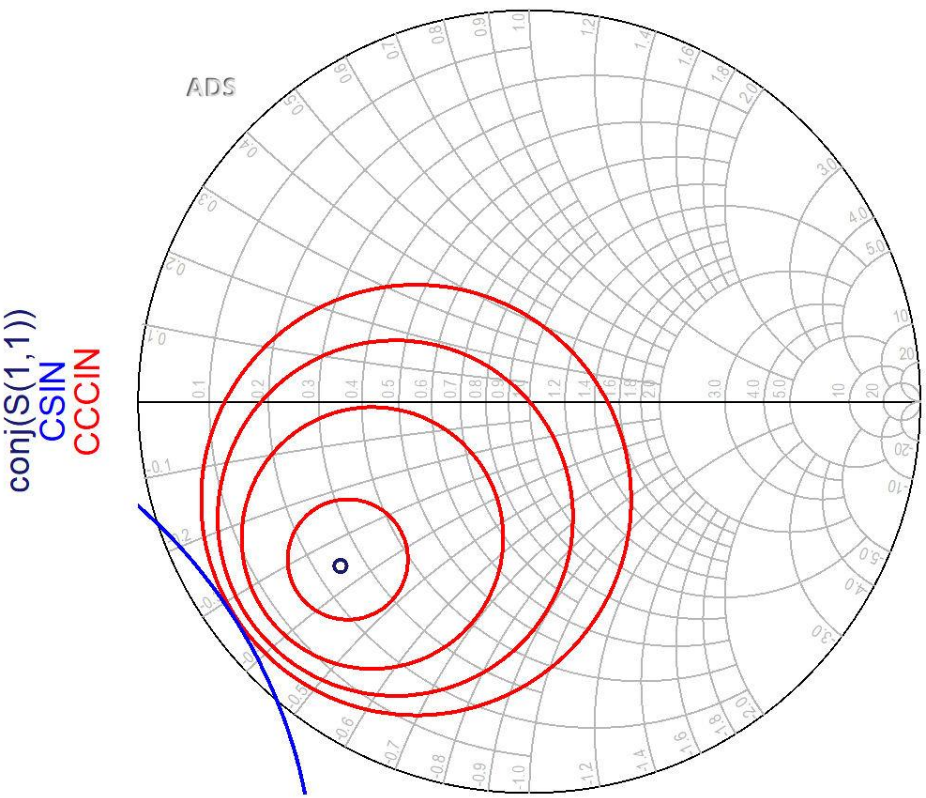
Cercuri de castig constant la intrare

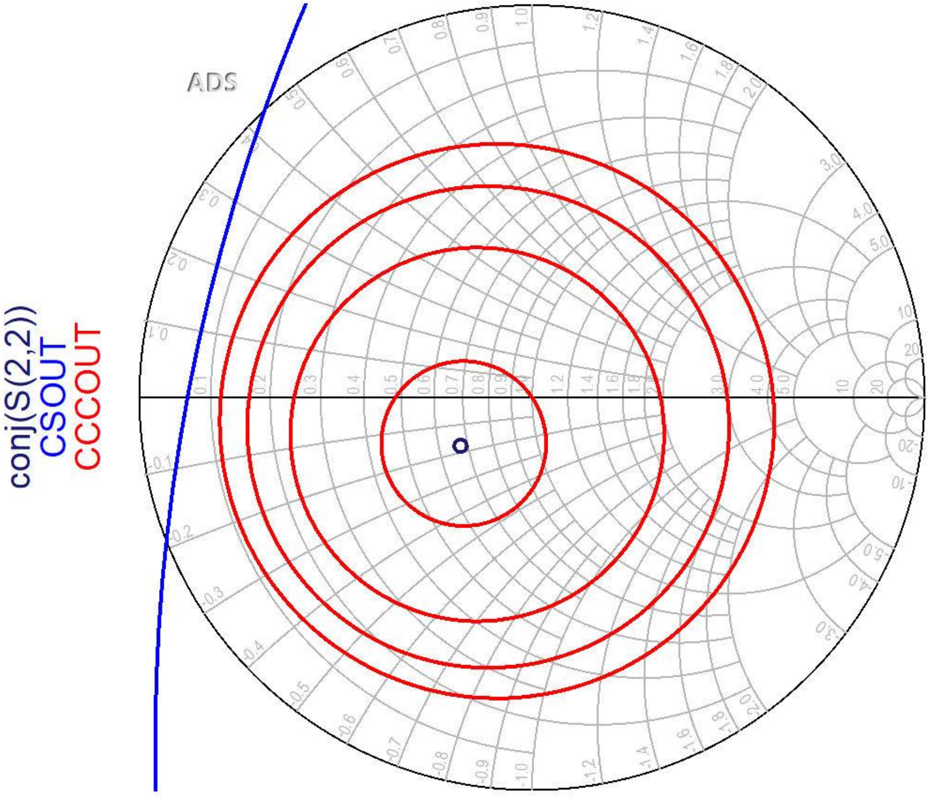
$$\left|\Gamma_S - \frac{g_S \cdot S_{11}^*}{1-(1-g_S)\cdot|S_{11}|^2}\right| = \frac{\sqrt{1-g_S}\cdot\left(1-|S_{11}|^2\right)}{1-(1-g_S)\cdot|S_{11}|^2} \qquad |\Gamma_S - C_S| = R_S$$

$$C_S = \frac{g_S \cdot S_{11}^*}{1-(1-g_S)\cdot|S_{11}|^2} \qquad R_S = \frac{\sqrt{1-g_S}\cdot\left(1-|S_{11}|^2\right)}{1-(1-g_S)\cdot|S_{11}|^2}$$

- Ecuatia unui cerc in planul complex in care reprezint Γ_S
- **Interpretare**: Orice punct Γ_S care reprezentat in planul complex se gaseste **pe** cercul desenat pentru $g_{cerc} = G_{cerc}/G_{Smax}$ va conduce la obtinerea castigului $G_S = G_{cerc}$
  - Orice punct **in exteriorul** acestui cerc va genera un castig $G_S < G_{cerc}$
  - Orice punct **in interiorul** acestui cerc va genera un castig $G_S > G_{cerc}$
- Discutie similara la iesire **CCCIN, CCCOUT**

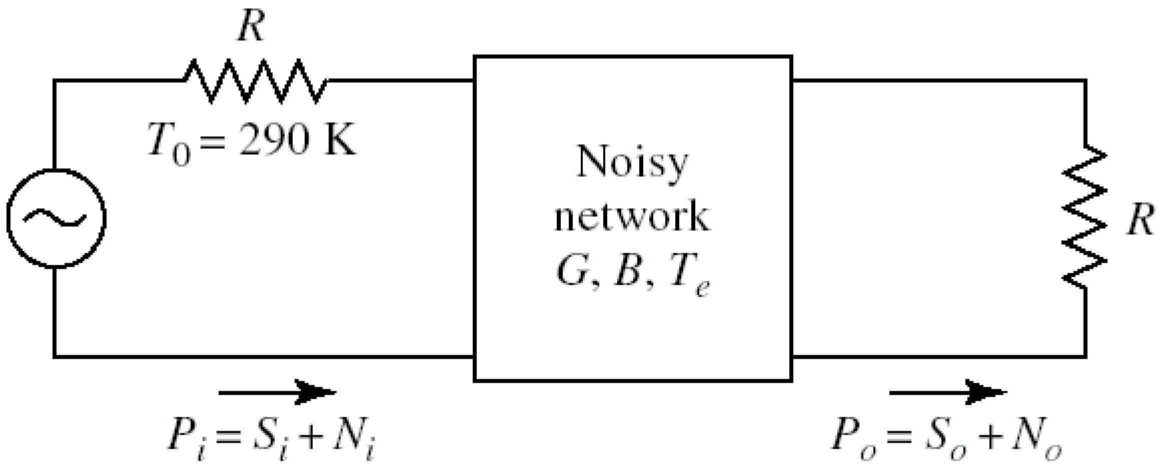
CCCIN, CCCOUT





- Cercurile se reprezinta pentru valorile cerute in dB
- Este utila calcularea G_{Smax} si G_{Lmax} anterior

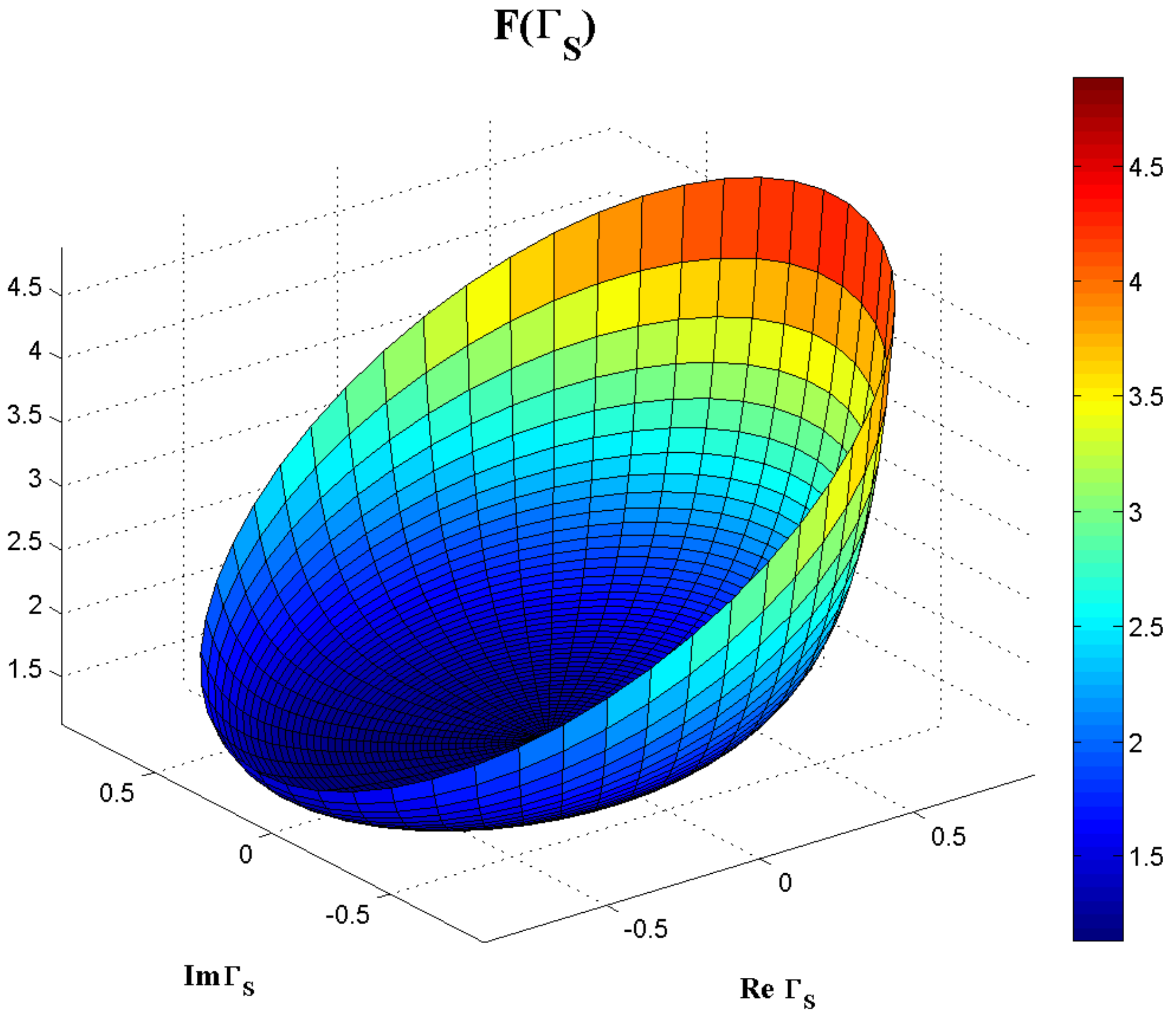
Factor de zgomot



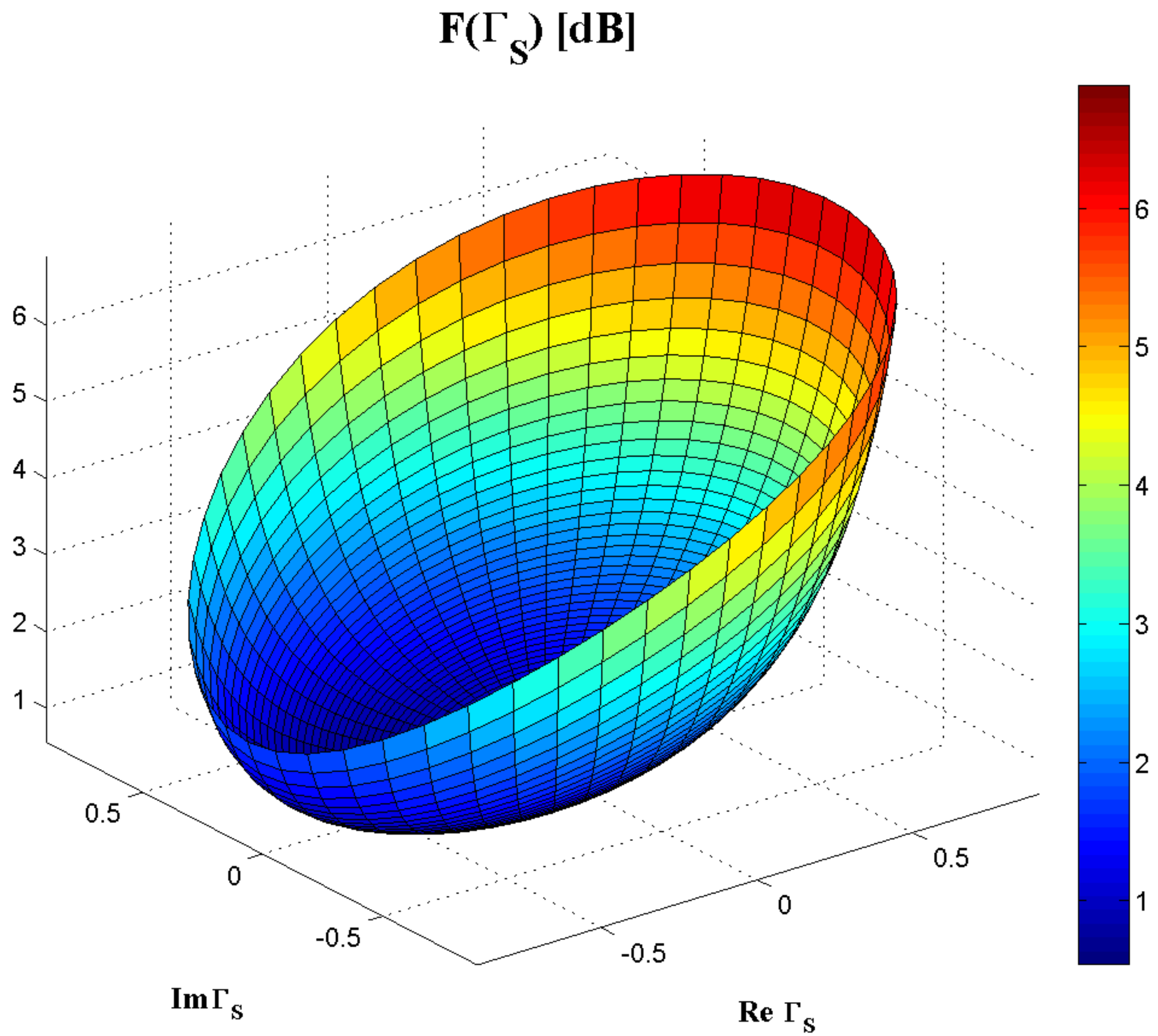
- Factorul de zgomot F caracterizeaza degradarea raportului semnal/zgomot intre intrarea si iesirea unei componente

$$F = \frac{S_i / N_i}{S_o / N_o}$$

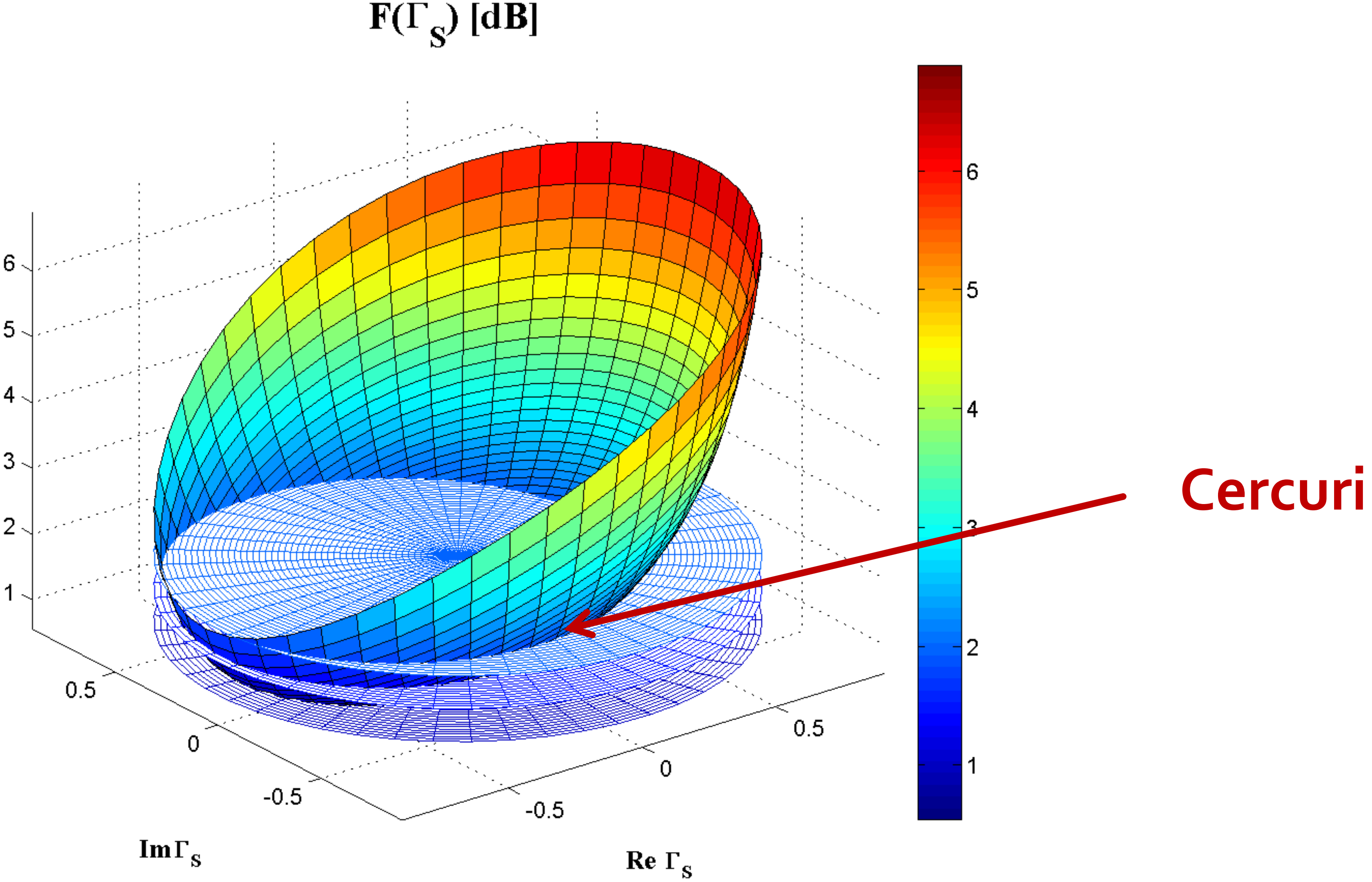
$F(\Gamma_S)$



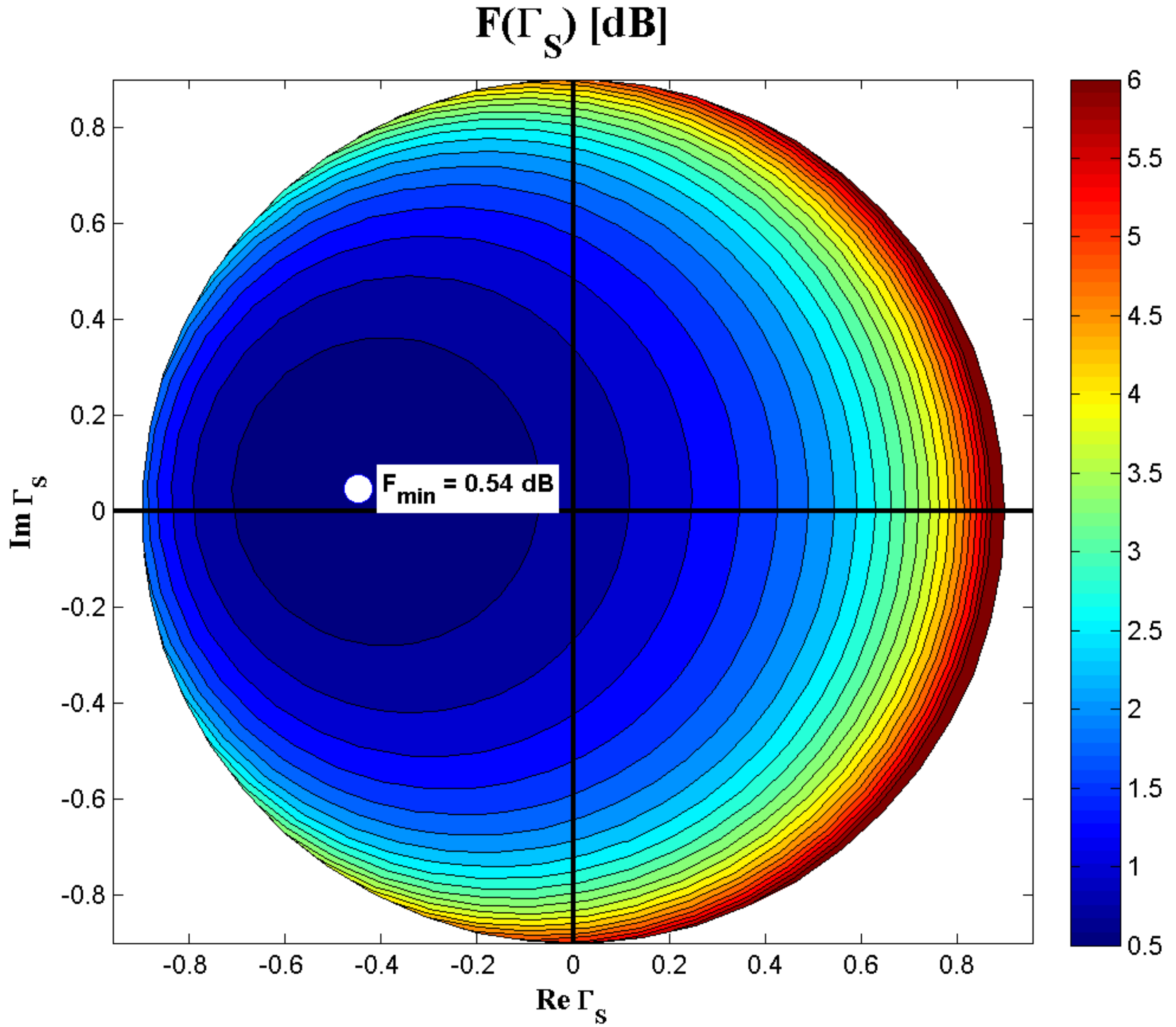
$F[dB](\Gamma_S)$



F[dB](Γ_S), diagrama de nivel

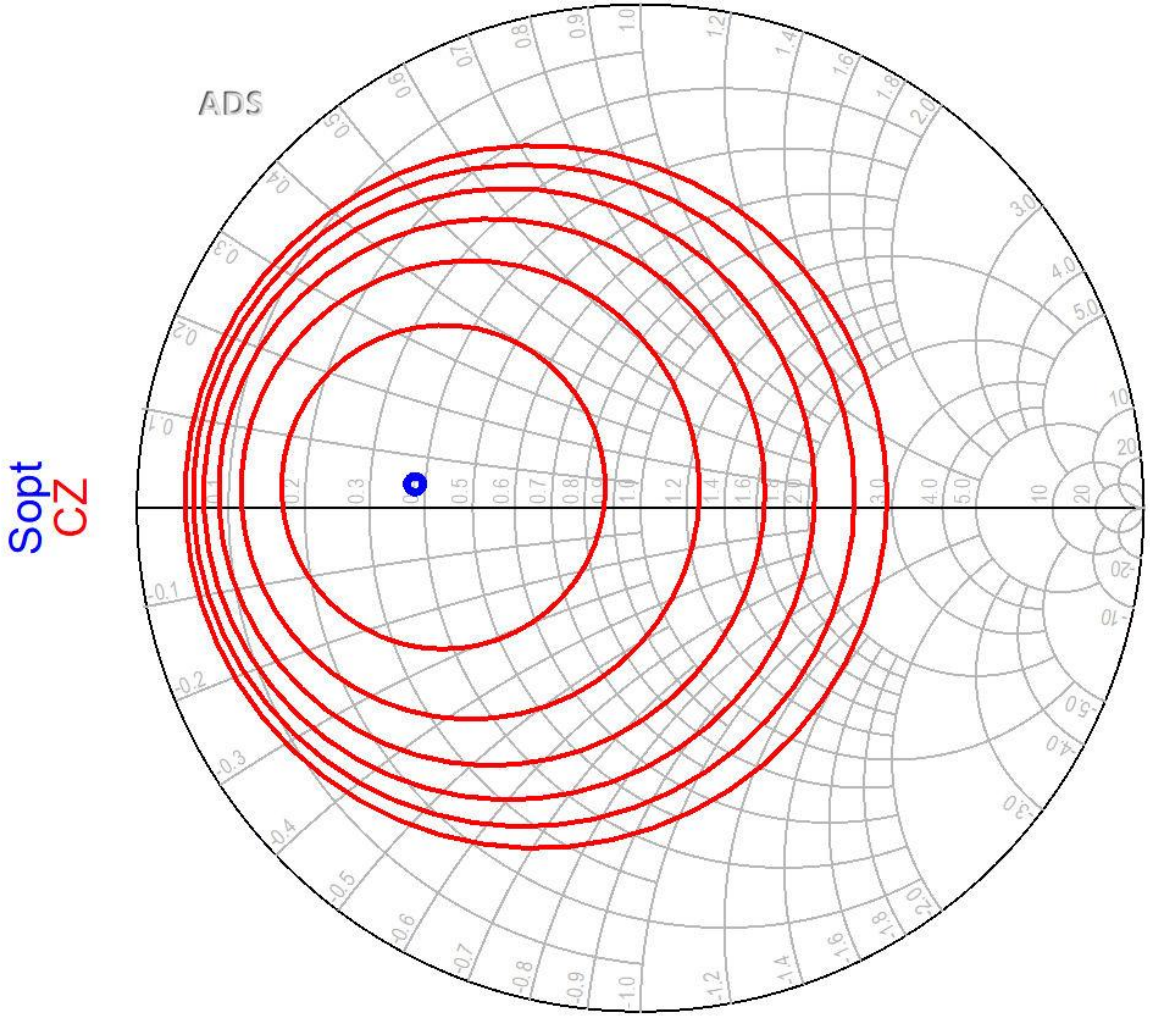


G_S[dB](Γ_S), diagrama de nivel



$\Gamma opt = 0.45 \angle 174°$

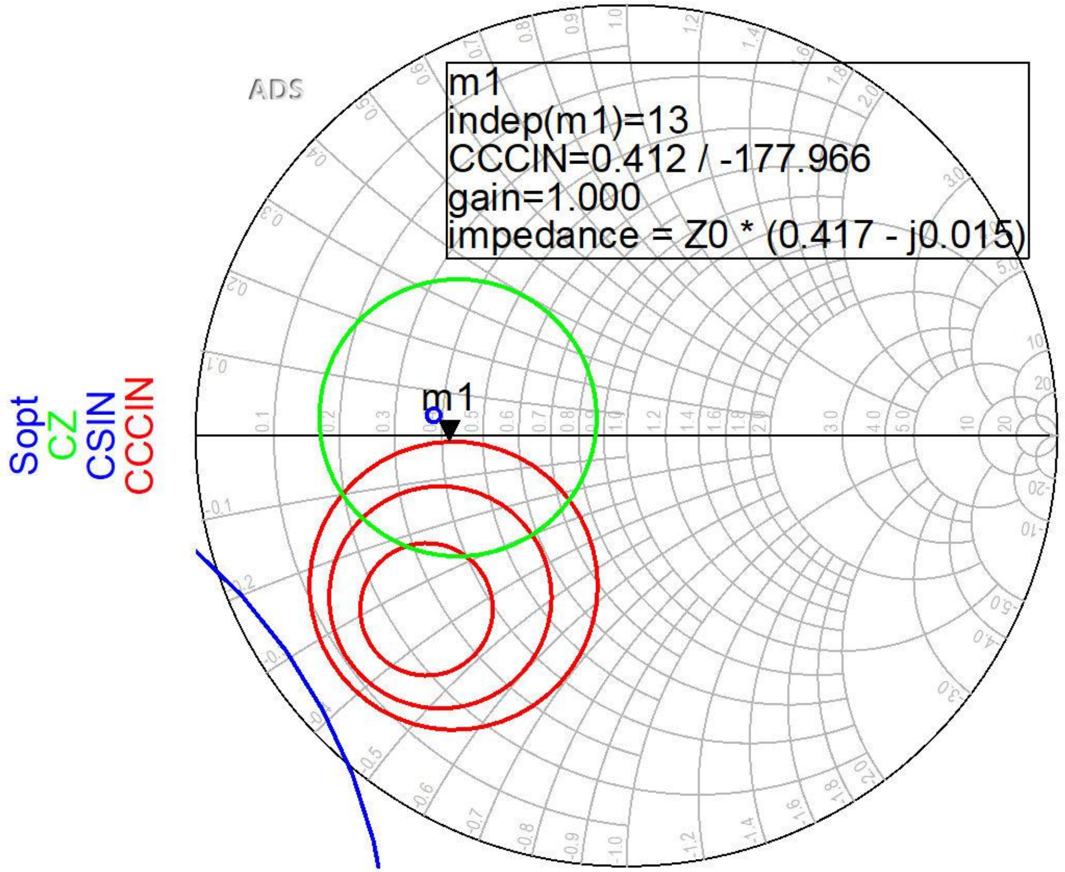
CZ – numai la intrare !



Exemplu, LNA @ 5 GHz

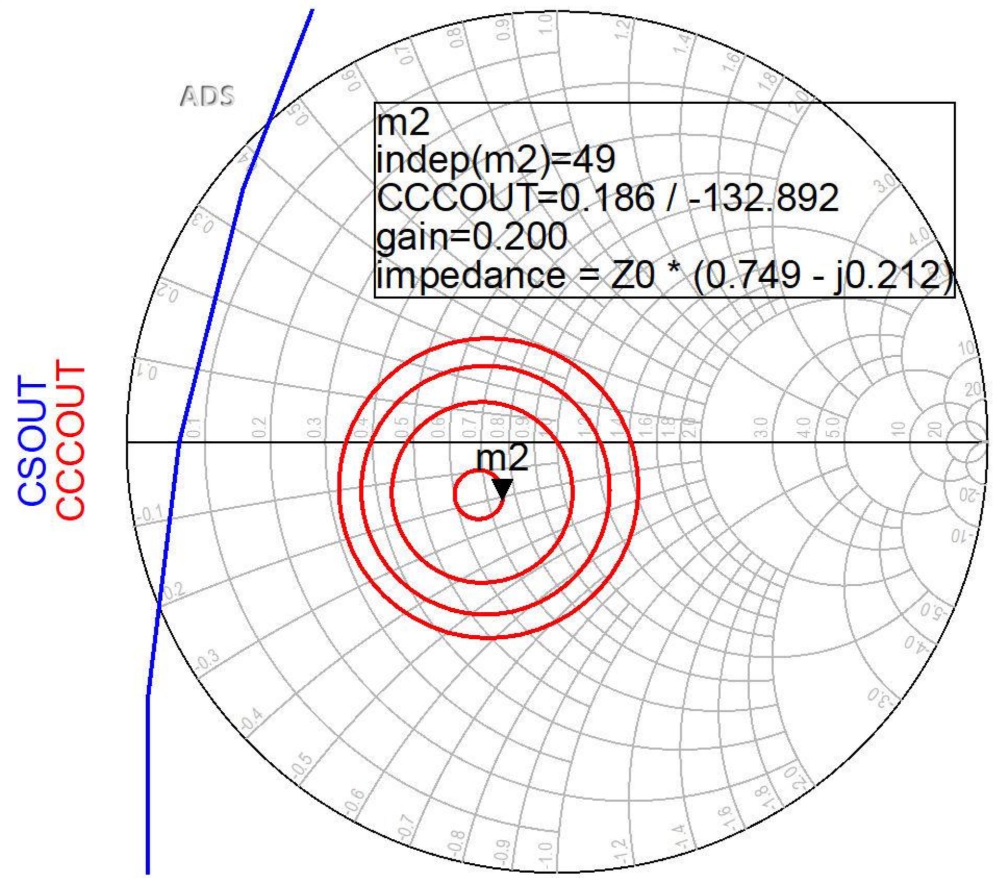
- Amplificator de zgomot redus
- La intrare e necesar un compromis intre
  - zgomot (cerc de zgomot constant ~~la intrare~~)
  - castig (cerc de castig constant la intrare)
  - stabilitate (cerc de stabilitate la intrare)
- La iesire zgomotul **nu intervine** (nu exista influenta). Compromis intre:
  - castig (cerc de castig constant la iesire)
  - stabilitate (cerc de stabilitate la iesire)

Adaptare la intrare



- Daca se sacrifica 1.2dB castig la intrare pentru conditii convenabile F,Q (Gs = 1 dB)
- Se prefera obtinerea unui zgomot mai mic

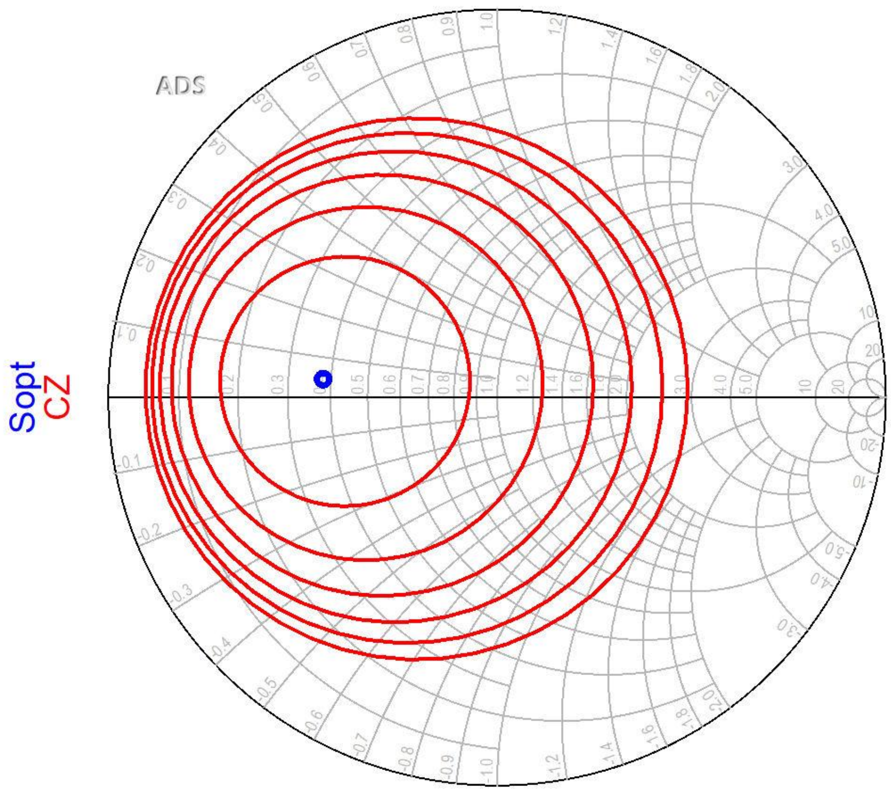
Adaptare la iesire

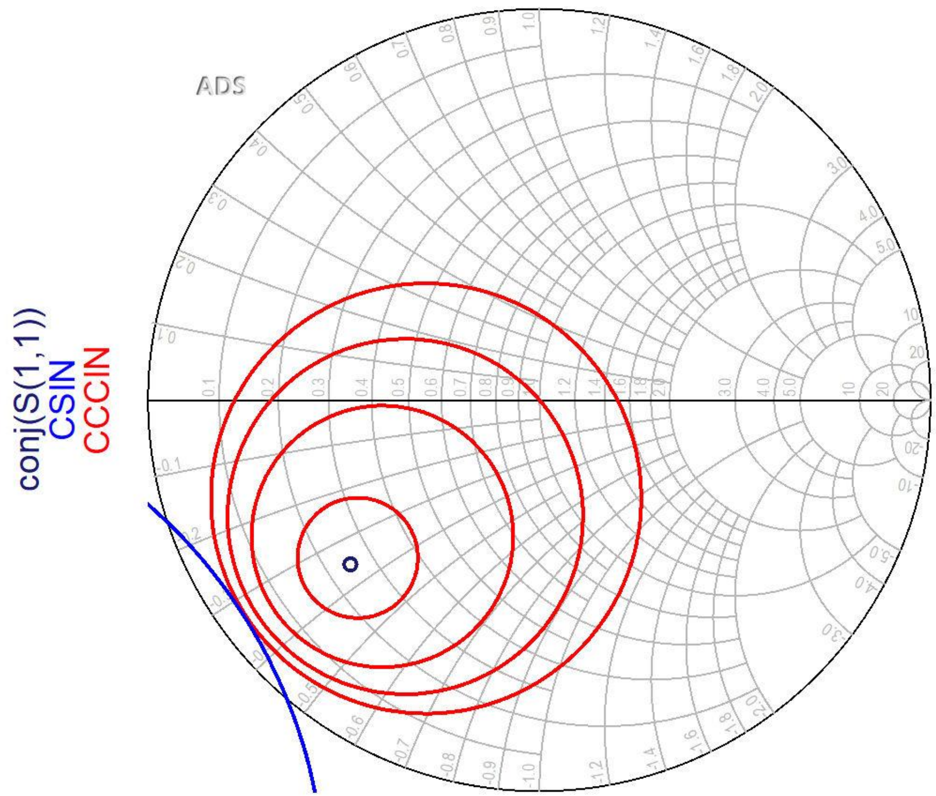


- CCCOUT: -0.4dB, -0.2dB, 0dB, +0.2dB
- Lipsa conditiilor privitoare la zgomot ofera posibilitatea obtinerii unui castig mai mare (spre maxim)

LNA

- De obicei un tranzistor potrivit pentru implementarea unui LNA la o anumita frecventa va avea cercurile de castig la intrare si cercurile de zgomot in aceeasi zona pentru Γ_S





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